

Fig. 1.28 Ultrasonic imaging is used extensively in obstetric examinations. Here we see the fetal backbone and ribs and the placenta paralleling the abdominal wall. (Courtesy of Kai Haber.)

bony skull, but this is not a commercial option yet. Before the skull calcifies at the age of two or three years, however, excellent brain images can be obtained. Thus, at the present time, ultrasound finds its major applications in abdominal, obstetrical, and cardiac imaging. Figures. 1.26–1.28 show further typical ultrasound images.

2

Theory of Linear Systems

2.1 INTRODUCTION

Mathematical modeling is the art of judicious oversimplification. A model realistic enough to quantitatively describe all facets of a physical system is often too complicated to analyze. Even when this is not the case, when an involved model eventually yields to sophisticated mathematics and powerful computers, the result is often a disappointing paucity of physical insights. A simple model is usually the most fertile.

Probably the most important simplification we can introduce in describing any physical system is to treat it as a linear system. Logic would demand that we define the term “system” before attempting to define a “linear system,” but we shall be content with the statement that a system is anything we care to analyze. For example, it could be a mass on a spring, a thermometer, an electrical filter, or a complex telecommunications network. This book deals primarily with radiological imaging systems such as chest x-ray units, scintillation cameras for nuclear medicine, and computed tomography machines.

All these systems may be represented schematically, as shown in Fig. 2.1, by a black box that receives an input stimulus $w_{in}(u)$, where u is an appropriate independent variable such as time or spatial position. (Note that u can be a vector or a set of parameters.) The system then produces an output response $w_{out}(u)$; the relationship of the response $w_{out}(u)$ to the stimulus $w_{in}(u)$ is the subject of our theory.

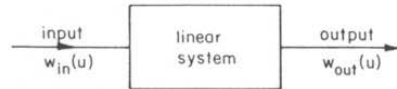


Fig. 2.1 "Black box" representation of a linear system.

For a mass on a spring, the stimulus is the total time-varying force acting on the mass, and the response might be the displacement or the velocity of the mass. In a mercury thermometer the stimulus is the temperature and the response is the height of the column of mercury. In a simple electrical filter or a complex telecommunications network, both the input and the output can be specified as voltages. In all these examples the independent variable is the time.

For a radiological system, the specification of the input and output is a little less obvious. In a chest x-ray system we could call the x-ray absorption coefficient at some point in the patient's chest the input and the optical density of the developed film the output. Alternatively, the total attenuation of an x-ray beam in traversing a particular path through the chest could be considered the input, and the x-ray photon flux at a particular location on the film could be the output. In a nuclear scintillation camera a natural choice of the stimulus $w_{in}(u)$ is the concentration of radioactive nuclei within the patient's body. The output could be a brightness distribution on a cathode ray tube display, the density of a developed film, or a matrix of numbers. In these two examples the independent variable is a spatial position.

These examples illustrate the freedom we have in specifying the system to be analyzed, but they also raise a nontrivial question about the independent variable u . This variable may be one-dimensional (time), two-dimensional (position within a specified plane), or three-dimensional (position within a volume). A difficulty arises when the same dimensionality is not appropriate for the description of both the input and the output. For example, the nuclear medicine system had a three-dimensional distribution as the input and a two-dimensional distribution as the output. Methods of dealing with this discrepancy will be developed as the need arises in subsequent chapters; for the remainder of this chapter it is assumed that the same u is appropriate for both the input and output.

It is now straightforward to define the concept of linearity. Suppose that an input $w_{in}^{(1)}(u)$ produces the output $w_{out}^{(1)}(u)$ and that a different input $w_{in}^{(2)}(u)$ produces the output $w_{out}^{(2)}(u)$. The system is said to be linear if, when both inputs are applied together so that $w_{in}(u) = w_{in}^{(1)}(u) + w_{in}^{(2)}(u)$, the output is given by $w_{out}(u) = w_{out}^{(1)}(u) + w_{out}^{(2)}(u)$. A simple corollary of this is that the input $\alpha w_{in}(u)$ will produce the output $\alpha w_{out}(u)$ if $w_{in}(u)$ produces $w_{out}(u)$. Here α is any real number.

It is important to keep in mind that linearity is an idealization. No real physical system is strictly linear. The force produced by a spring is not exactly

proportional to the displacement. The blackening of a film is not proportional to the incident photon flux. The count rate of a nuclear detector is not exactly proportional to the number of radioactive nuclei in its field of view. Nevertheless, linear systems theory, as we shall see, is an extremely powerful tool in many circumstances. The effects of the omnipresent nonlinearities can often be considered separately and grafted onto the linear theory almost as an afterthought.

2.2 IMPULSE RESPONSE

2.2.1 Nonlocal Behavior of Linear Systems

It should be evident from the examples given above that the output of a system for some value of the independent variable u cannot in general be determined from the input at that one value of u . If u is the time t , then $w_{out}(t)$ depends not only on w_{in} evaluated at the current time, but also on w_{in} at previous times. No real system responds instantaneously to a stimulus; there is always a time delay.

A similar situation occurs if u represents a spatial position. Consider a simple camera in which a planar object is imaged at unit magnification onto a planar film. The variable u is then a two-dimensional vector in either the object plane or the image plane. However, the irradiance at some point u in the image is not determined solely by the light emitted from the corresponding point on the object plane. Instead, the lens inevitably produces a more or less blurred image of the object point. We can then think of each object point contributing to the response at many image points, or equivalently of each image point receiving a stimulus from many object points.

This kind of nonlocal behavior can be described quite generally for linear systems by writing $w_{out}(u)$ as a linear superposition of the values of w_{in} for all values of u . Since u is usually a continuous variable, the most general linear superposition is an integral of the form

$$w_{out}(u) = \int_{-\infty}^{\infty} p(u; u') w_{in}(u') du'. \quad (2.1)$$

The significance of the integration kernel $p(u; u')$ is discussed below. For notational simplicity, we have written the integral as a one-dimensional one over an infinite domain. If u is a two- or three-dimensional variable, the integration must, of course, be extended over the other dimensions as well. Furthermore, if it is known a priori that $w_{in}(u')$ is nonzero only over some specific domain of u' , then the integration limits can be appropriately modified.

To interpret the quantity $p(u; u')$ of (2.1), it is useful to introduce the Dirac delta function or unit impulse. The reader unfamiliar with this mathematical device should consult Appendix A, but the important points are reviewed here. The function $\delta(u)$ is defined to be zero unless $u = 0$, at which point $\delta(u)$ is infinite. The integral of $\delta(u)$ is, however, finite and defined to be unity, i.e.,

$$\int_{-\epsilon}^{\epsilon} \delta(u) du = 1, \quad (2.2)$$

where ϵ is any nonzero positive number. [In two or more dimensions, $\delta(u)$ is to be interpreted as a product such as $\delta(x)\delta(y)$. Cartesian coordinates must be employed to achieve this factorization. Furthermore, a form like $\delta(u - u')$ becomes $\delta(x - x')\delta(y - y')$.] This then leads to the “sifting” property of the delta function,

$$\int_a^b f(u) \delta(u - u_0) du = f(u_0) \quad \text{if } a < u_0 < b, \quad (2.3)$$

where $f(u)$ is any function that is continuous at the point u_0 . If u is a two-dimensional variable, the *area* of integration must include the point u_0 for (2.3) to hold.

Returning to the interpretation of (2.1), let us suppose that the input stimulus $w_{in}(u)$ is the delta function $\delta(u - u_0)$. We shall call the output in this case $w_{out}^\delta(u)$, where the superscript serves as a reminder that the result is not general, but applies only with the delta-function input. We then have

$$w_{out}^\delta(u) = \int_{-\infty}^{\infty} p(u; u') \delta(u' - u_0) du' \quad (2.4)$$

which, by use of (2.3), becomes

$$w_{out}^\delta(u) = p(u; u_0). \quad (2.5)$$

The function $p(u; u_0)$ is thus the response of the system measured at point u when the stimulus is the unit impulse applied at point u_0 . For this reason, $p(u; u_0)$ is called the *impulse response* of the system. If the system is an imaging system, it is common to refer to the impulse response as the *point spread function* (PSF). In this case u is the two-dimensional position vector \mathbf{r} .

2.2.2 Shift Invariance and Convolution

In our camera example, $p(\mathbf{r}; \mathbf{r}_0)$ is the light distribution at point \mathbf{r} in the image plane when the scene is a point source of light at point \mathbf{r}_0 in the object plane. Of course, the concept of a point source is as much of an abstraction as a delta function, but it can often be satisfactorily approximated in practice by a very small, very bright source. If this source is small compared to the

scale of the function $p(\mathbf{r}; \mathbf{r}_0)$, then the measured response $w_{out}(\mathbf{r})$ is an adequate approximation to $p(\mathbf{r}; \mathbf{r}_0)$.

If we set out to measure the PSF of our camera in this way, with a point source in the object plane, we would, in general, have to make a large number of measurements. For each source position \mathbf{r}_0 , we would have to measure a two-dimensional distribution $p(\mathbf{r}; \mathbf{r}_0)$; then the procedure would have to be repeated for a large number of source positions. In other words, $p(\mathbf{r}; \mathbf{r}_0)$ is a function of two independent two-dimensional variables. Its complete specification therefore requires a four-dimensional space.

Fortunately this degree of complexity is often unnecessary. In many linear systems the impulse response is a function of the *difference* of its two arguments, not each argument separately. Thus we can represent $p(u; u_0)$ as $p(u - u_0)$. [Note that $p(u - u_0)$, being a function of only one argument, cannot be the same mathematical function as $p(u; u_0)$, which depends on two arguments. It does, however, represent the same physical distribution.] Systems satisfying this condition are said to be *shift-invariant* or *isoplanatic*. In the camera example, this representation is valid if the *shape* of the blurred image of a point is independent of the location of the point. The only effect of a shift in location of the point source is to shift the location of the image without changing its functional form.

Some additional insight into the meaning of shift invariance can be obtained by considering an electrical filter where u is the time t . If the parameters of the filter (its inductances, capacitances, and resistances) are independent of time, then it does not matter when a particular voltage waveform is applied to the input—the same output waveform follows inexorably. To be more precise, if the voltage input $v_{in}(t)$ produces the output $v_{out}(t)$, then a delayed input $v_{in}(t - t_0)$ produces a delayed output $v_{out}(t - t_0)$. This statement holds for any input, and in particular it holds when the input is the unit impulse $\delta(t - t_0)$.

To this point we have been rather glibly jumping back and forth between spatial and temporal variables to emphasize the universality of the theory being developed. There is, however, one major distinction between the two situations, a distinction that arises because a response cannot precede its stimulus. The temporal impulse response $p(t - t_0)$ must therefore be zero if $t < t_0$ since t is the time at which the response is measured and t_0 is the time when the stimulus occurs. The system is said to be *causal*. This asymmetry, which is of crucial importance in the analysis of electrical filters, has no counterpart in imaging systems. Indeed, it is quite common in imaging systems to find a completely symmetric PSF, i.e., $p(\mathbf{r}) = p(r)$, where $r = |\mathbf{r}|$.

Having surfaced this difference between systems involving temporal and spatial variables, we now resubmerge it and return to the general notation, where u can be whatever independent variable is appropriate. Then the

general input-output relation for a linear shift-invariant system may be written

$$w_{\text{out}}(u) = \int_{-\infty}^{\infty} p(u - u') w_{\text{in}}(u') du'. \quad (2.6)$$

This type of integral is called a *convolution* or *folding* integral. The latter designation derives from the operations carried out in performing the integral. As illustrated in Fig. 2.2, if we start with the function $p(u')$, we form

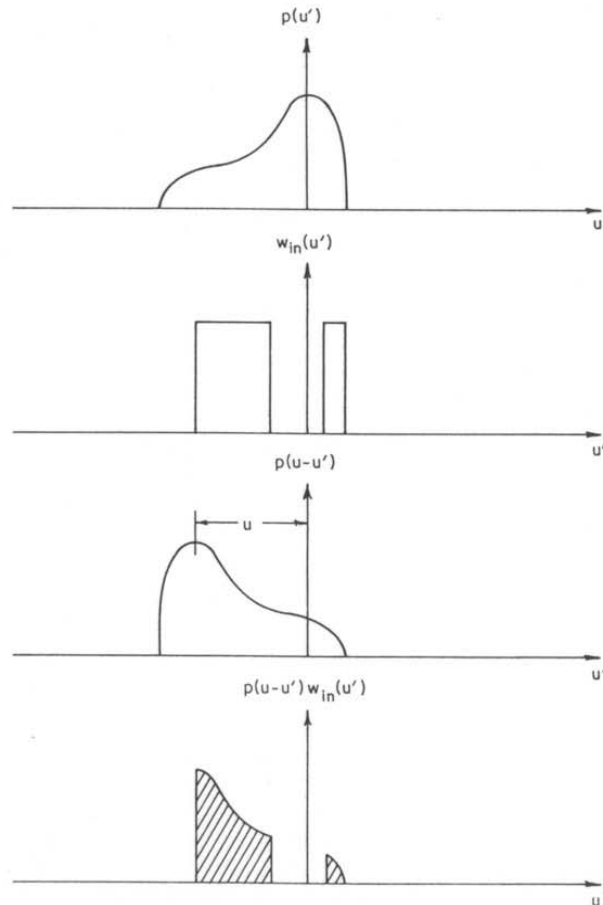


Fig. 2.2 Illustration of the convolution operations. The function $w_{\text{in}}(u')$ is a representative input to a linear system with impulse response $p(u')$. The function $p(u - u')$, drawn here for u negative, is a shifted and reversed version of $p(u')$, and the shaded area under the product $p(u - u')w_{\text{in}}(u')$ is $p(u) * w_{\text{in}}(u)$.

$p(u - u')$ by shifting the function by an amount u and then reversing its orientation (folding it) along the u' axis. This sequence of operations follows from the algebraic truism $p(u - u') = p[-(u' - u)]$. Since the reversal step often causes some confusion, it is perhaps worth pointing out that no reversal is involved if we plot $p(u - u')$ versus u rather than u' . If $p(u)$ is the response at u due to a unit impulse at $u' = 0$, then $p(u - u')$, which is simply shifted along the u axis and *not* reversed, is the response at u due to an impulse at an arbitrary u' . The reversal is necessary only when we plot $p(u - u')$ vs u' in order to visualize the overlap with $w_{\text{in}}(u')$ in the integrand of (2.6).

The arguments leading to (2.6) can be summarized by the following syllogism (see also Table 2.1):

1. If the input to a linear shift-invariant system is the unit impulse $\delta(u - u')$, the output is the impulse response $p(u - u')$.
2. However, an arbitrary input $w_{\text{in}}(u)$ can be expressed as a superposition of impulses, i.e.,

$$w_{\text{in}}(u) = \int_{-\infty}^{\infty} w_{\text{in}}(u') \delta(u - u') du'. \quad (2.7)$$

3. Therefore, the response to an arbitrary input is the *same* superposition of impulse responses, i.e.,

$$w_{\text{out}}(u) = \int_{-\infty}^{\infty} w_{\text{in}}(u') p(u - u') du'. \quad (2.8)$$

It is important for this argument to note that $w_{\text{in}}(u')$ in the integrand is simply a constant coefficient as far as the u dependence is concerned. The

TABLE 2.1

Logical Sequence of Possible Inputs to a Linear Shift-Invariant System and the Corresponding Outputs

Input	Output
$\delta(u)$	$p(u)$
$\delta(u - u')$	$p(u - u')$
$\alpha \delta(u - u')$	$\alpha p(u - u')$
$\alpha \delta(u - u_1) + \beta \delta(u - u_2)$	$\alpha p(u - u_1) + \beta p(u - u_2)$
$\sum_j \alpha_j \delta(u - u_j)$	$\sum_j \alpha_j p(u - u_j)$
$\int_{-\infty}^{\infty} w_{\text{in}}(u') \delta(u - u') du' = w_{\text{in}}(u)$	$\int_{-\infty}^{\infty} w_{\text{in}}(u') p(u - u') du' = w_{\text{out}}(u)$
	$= w_{\text{in}}(u) * p(u)$

system, being linear, converts $\delta(u - u')$ to $p(u - u')$ and $\alpha\delta(u - u')$ to $\alpha p(u - u')$. It makes no difference that the constant α is equal to $w_{in}(u')$ or that an integral over u' is carried out.

2.2.3 A Shorthand Notation

Convolutions occur so frequently in the analysis of linear systems that it is worthwhile to adopt a shorthand notation for them. We shall use asterisks to denote the convolution integral, with the number of asterisks corresponding to the dimensionality of u . For example, if $u = t$, we may write

$$w_{out}(t) = p(t) * w_{in}(t) = \int_{-\infty}^{\infty} p(t - t') w_{in}(t') dt'. \quad (2.9)$$

By a simple change of variables, we also have

$$\begin{aligned} p(t) * w_{in}(t) &= w_{in}(t) * p(t) \\ &= \int_{-\infty}^{\infty} w_{in}(t - t') p(t') dt'. \end{aligned} \quad (2.10)$$

Often, where no confusion can arise, we shall omit the output variable altogether and rewrite (2.9)

$$w_{out} = p * w_{in}. \quad (2.11)$$

In two dimensions the convolution integral is only slightly more complicated. If u is the two-dimensional position vector \mathbf{r} , we have

$$\begin{aligned} w_{out}(\mathbf{r}) &= \int_{\infty} p(\mathbf{r} - \mathbf{r}') w_{in}(\mathbf{r}') d^2 r' \\ &= p(\mathbf{r}) ** w_{in}(\mathbf{r}). \end{aligned} \quad (2.12)$$

The subscript ∞ on the integral sign indicates that the integration runs over the entire domain of the variable of integration—in this case the infinite \mathbf{r}' plane. In Cartesian coordinates the area element $d^2 r'$ becomes $dx' dy'$ and the integral becomes

$$\begin{aligned} w_{out}(x, y) &= \int_{-\infty}^{\infty} dx' \int_{-\infty}^{\infty} dy' p(x - x', y - y') w_{in}(x', y') \\ &= p(x, y) ** w_{in}(x, y), \end{aligned} \quad (2.13)$$

where x and y are the Cartesian components of \mathbf{r} , and $p(x, y)$ is the same PSF as $p(\mathbf{r})$ but expressed in Cartesian coordinates. The shift-invariant PSF $p(x, y)$ should not be confused with the shift-variant function $p(u; u_0)$ used earlier.

2.3 THE FREQUENCY DOMAIN

2.3.1 Response to a Complex Exponential Input

In Section 2.2.2 we analyzed linear shift-invariant systems by resolving the input into a superposition of delta functions and by considering the response of the system to each delta function separately. This decomposition of the input is not unique. A wide variety of different sets of orthogonal functions can be used to represent the input. In this section we consider an alternative decomposition, viz.: resolving the input into a superposition of complex exponential functions of the form $\exp(2\pi i \kappa u)$, where $i = \sqrt{-1}$ and κ is a real number, the significance of which will become clear shortly. (If u represents a two- or three-dimensional vector, κ must be a vector of the same dimensionality and κu must be interpreted as the scalar product.) The use of complex functions to represent a real input may seem odd at first, but it shouldn't strain the credulity any more than the use of such a pathological function as $\delta(u)$.

Before attempting to synthesize an arbitrary input by superposing complex exponentials, let us consider the response of the system to a single such function. If we simply set

$$w_{in}^e(u) = \exp(2\pi i \kappa u) \quad (2.14)$$

and substitute into (2.6), we obtain

$$w_{out}^e(u) = \int_{-\infty}^{\infty} p(u - u') \exp(2\pi i \kappa u') du'. \quad (2.15)$$

The superscript e indicates that these equations hold only for the specified exponential input. Now change variables by letting $u'' = u - u'$. This leads to

$$w_{out}^e(u) = \exp(2\pi i \kappa u) \int_{-\infty}^{\infty} p(u'') \exp(-2\pi i \kappa u'') du''. \quad (2.16)$$

The integrand is independent of u , so the entire integral is simply a complex constant. We now have

$$w_{out}^e(u) = \text{const} \cdot w_{in}^e(u). \quad (2.17)$$

In other words, the effect of passing a complex exponential of the specified form through a linear shift-invariant system is just to multiply it by a complex constant. The exponential functions are said to be the *eigenfunctions* of the system and the constant [the integral in (2.16)] is called the *transfer function* of the system. (The term "function" is not a misnomer here because the integral depends functionally on κ ; it is a constant as far as its u dependence is concerned.)

2.3.2 Fourier Transforms

The reader who is either conversant with Fourier analysis or has perused Appendix B will recognize the integral in (2.16) as a Fourier transform (Bracewell, 1965; Papoulis, 1962; Gaskill, 1978). The general definition of the Fourier transform of a function $f(t)$ in one dimension is

$$F(v) = \mathcal{F}_1\{f(t)\} = \int_{-\infty}^{\infty} \exp(-2\pi i v t) f(t) dt. \quad (2.18)$$

We shall use these two alternative notations for the Fourier transform as convenient: the transform of a function denoted by a particular lowercase letter is denoted by the corresponding capital letter or by application of the operator \mathcal{F}_1 .

In two dimensions the Fourier transform of a function $f(\mathbf{r})$ is

$$F(\boldsymbol{\rho}) = \mathcal{F}_2\{f(\mathbf{r})\} = \int_{\infty} \exp(-2\pi i \boldsymbol{\rho} \cdot \mathbf{r}) f(\mathbf{r}) d^2 r, \quad (2.19)$$

where $\boldsymbol{\rho}$ is a two-dimensional vector with Cartesian components ξ and η . The operator \mathcal{F} without a subscript will apply to functions of unspecified dimensionality.

The temporal function $\exp(-2\pi i v t)$ is periodic in time with period v^{-1} . The number v is therefore the *frequency* and is measured in cycles per second or Hertz. The variables v and t are said to be Fourier conjugate variables.

Similarly, the spatial function $\exp(-2\pi i \boldsymbol{\rho} \cdot \mathbf{r})$, or $\exp[-2\pi i(\xi x + \eta y)]$ in Cartesian coordinates, is periodic in space with period ξ^{-1} along the x axis and η^{-1} along the y axis. The vector $\boldsymbol{\rho}$ is therefore a two-dimensional *spatial frequency* and is measured in cycles per unit length. Once again, $\boldsymbol{\rho}$ and \mathbf{r} are called conjugate variables. The function $F(\boldsymbol{\rho})$ is said to exist in the *spatial-frequency domain*, while $f(\mathbf{r})$ is in the *space domain*.

The extension of these ideas to three or more dimensions is straightforward.

The real utility of the Fourier transform is that it has a simple inverse. The inverse of the one-dimensional transform, (2.18), is

$$f(t) = \mathcal{F}_1^{-1}\{F(v)\} = \int_{-\infty}^{\infty} \exp(+2\pi i v t) F(v) dv, \quad (2.20)$$

and for the two-dimensional transform, (2.19), we have

$$f(\mathbf{r}) = \mathcal{F}_2^{-1}\{F(\boldsymbol{\rho})\} = \int_{\infty} \exp(+2\pi i \boldsymbol{\rho} \cdot \mathbf{r}) F(\boldsymbol{\rho}) d^2 \rho. \quad (2.21)$$

A proof of these results is given in Appendix B.

2.3.3 The System Transfer Function

Having dispensed with these mathematical details, let us now return to the analysis of linear systems. Once again we subsume all questions of dimensionality and use the general variable u which can be one-, two-, or three-dimensional as required. In any case, κ is the frequency variable conjugate to u .

We define a Fourier transform of $w_{in}(u)$ by

$$W_{in}(\kappa) = \int_{-\infty}^{\infty} \exp(-2\pi i \kappa u) w_{in}(u) du, \quad (2.22)$$

and similarly for $w_{out}(u)$. The inverse Fourier transform is

$$w_{in}(u) = \int_{-\infty}^{\infty} \exp(+2\pi i \kappa u) W_{in}(\kappa) d\kappa. \quad (2.23)$$

We have now resolved an arbitrary input into a linear superposition of complex exponential functions. We have already determined the action of the linear system on one such function, with the result expressed in (2.16). Now all we have to do is to recognize that each exponential term in the superposition of (2.23) will pass through the system independently; this, in fact, is the definition of linearity. Thus the system output for the arbitrary input specified by (2.23) is just a superposition of terms like (2.16), with weighting factors $W_{in}(\kappa)$. [$W_{in}(\kappa)$ is, of course, independent of u and may be regarded as a constant coefficient (see Table 2.2).] The general output is then given formally by

$$w_{out}(u) = \int_{-\infty}^{\infty} W_{in}(\kappa) P(\kappa) \exp(2\pi i \kappa u) d\kappa, \quad (2.24)$$

TABLE 2.2

Frequency-domain Counterpart of Table 2.1
Illustrating a Sequence of Inputs to a Linear
Shift-Invariant System^a

Input	Output
$\exp(2\pi i \kappa u)$	$P(\kappa) \exp(2\pi i \kappa u)$
$\alpha \exp(2\pi i \kappa u)$	$\alpha P(\kappa) \exp(2\pi i \kappa u)$
$\sum_j \alpha_j \exp(2\pi i \kappa_j u)$	$\sum_j \alpha_j P(\kappa_j) \exp(2\pi i \kappa_j u)$
$\int_{-\infty}^{\infty} W_{in}(\kappa) \exp(2\pi i \kappa u) d\kappa$	$\int_{-\infty}^{\infty} W_{in}(\kappa) P(\kappa) \exp(2\pi i \kappa u) d\kappa$

^a Note: $P(\kappa) = \int_{-\infty}^{\infty} \exp(-2\pi i \kappa u) p(u) du$.

where $P(\kappa)$ is just the integral in (2.16), i.e.,

$$P(\kappa) = \int_{-\infty}^{\infty} \exp(-2\pi i \kappa u'') p(u'') du''. \quad (2.25)$$

The same result can be expressed more succinctly by noting that the right-hand side of (2.24) is the inverse Fourier transform of the product $W_{in}(\kappa)P(\kappa)$. Performing a Fourier transform on both sides of the equation then yields

$$W_{out}(\kappa) = W_{in}(\kappa)P(\kappa). \quad (2.26)$$

This equation, which is precisely equivalent to (2.6), is of fundamental importance in linear systems analysis. It may be derived directly from (2.6) by use of the theorem given in Appendix B that says that the Fourier transform of a convolution is the product of the Fourier transforms of the two functions being convolved, i.e.,

$$W_{in}(\kappa)P(\kappa) = \mathcal{F}\{w_{in}(u) * p(u)\}. \quad (2.27)$$

As previously noted, $P(\kappa)$, the Fourier transform of the impulse response, is called the *transfer function* of the linear system. The reason for this designation should now be evident. A particular *Fourier component*, one term in the superposition of (2.23), is transferred through the system unchanged in functional form but simply multiplied by the factor $P(\kappa)$.

However, since $P(\kappa)$ is a complex number, the physical significance of this multiplication may not be immediately clear. To remedy this deficiency, let us construct a slightly more complicated input function of the form

$$w_{in}(u) = \frac{1}{2}(1 + \cos 2\pi \kappa u) = \frac{1}{2} + \frac{1}{4}\exp(2\pi i \kappa u) + \frac{1}{4}\exp(-2\pi i \kappa u). \quad (2.28)$$

This function is obviously real, a decided asset, but moreover it is everywhere nonnegative. It can therefore be used to represent physical quantities, such as irradiance or concentration of radioactive nuclei, that cannot have negative values. This input function, however, is not a single Fourier component. Rather it contains three discrete frequencies: 0, κ , $-\kappa$. It is therefore not an eigenfunction of the system and the output is not expected to have exactly the same functional form as the input.

Since we know the Fourier decomposition of the input, (2.28), we can write down the output by inspection:

$$w_{out}(u) = \frac{1}{2}P(0) + \frac{1}{4}P(\kappa)\exp(2\pi i \kappa u) + \frac{1}{4}P(-\kappa)\exp(-2\pi i \kappa u). \quad (2.29)$$

An additional simplification is possible since $p(u)$ is a real quantity. This implies, as shown in Appendix B [see Eq. (B.7)], that

$$P(\kappa) = [P(-\kappa)]^*, \quad (2.30)$$

where the asterisk denotes the complex conjugate. Note that there is no physical requirement that $P(\kappa)$ be real except at $\kappa = 0$. In fact, we shall write

$P(\kappa)$ in modulus-phase form to emphasize its generally complex nature:

$$P(\kappa) = |P(\kappa)| \exp(i\phi_P), \quad (2.31)$$

and, from (2.30),

$$P(-\kappa) = |P(\kappa)| \exp(-i\phi_P). \quad (2.32)$$

With these results we can now rewrite (2.29)

$$w_{out}(u) = \frac{1}{2}P(0) + \frac{1}{2}|P(\kappa)| \cos(2\pi \kappa u + \phi_P). \quad (2.33)$$

The output is still a real quantity, as it must be since it comes from a real physical system. The effect of the system is to alter the amplitude of the cosine modulation term relative to the constant (zero-frequency) term and to shift its phase (see Fig. 2.3).

It is useful to define the *modulation* or *contrast* of the input signal by

$$M_{in} = \frac{w_{in}^{\max} - w_{in}^{\min}}{w_{in}^{\max} + w_{in}^{\min}}, \quad (2.34)$$

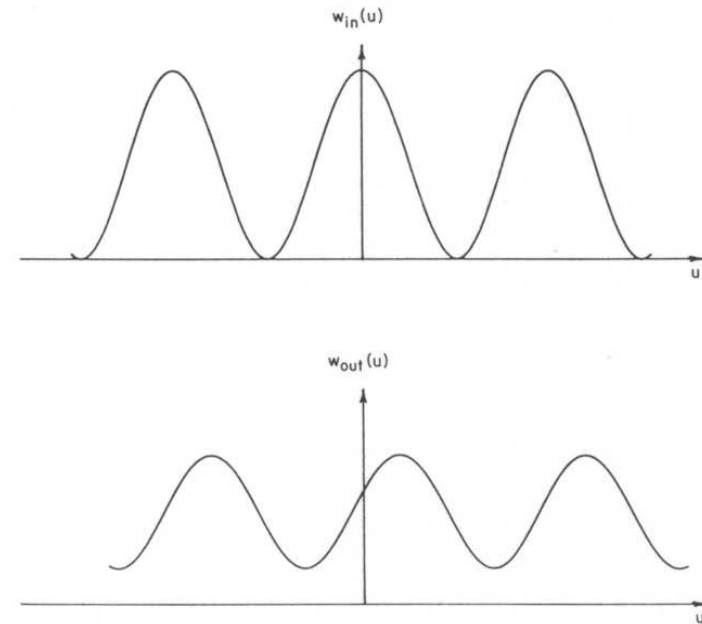


Fig. 2.3 Top: A cosinusoidal function of 100% contrast that is a possible input to a linear system. Bottom: The output of the linear system for the input shown above. Note that, in general, the contrast is reduced and the phase is shifted but the frequency is unchanged. Both $w_{in}(u)$ and $w_{out}(u)$ should be regarded as extending to $\pm \infty$.

and similarly for the output. Here w_{in}^{max} is the maximum value of $w_{in}(u)$ and w_{in}^{min} is its minimum. The input modulation M_{in} is unity for our case since $w_{in}^{max} = 1$ and $w_{in}^{min} = 0$. For the output, however, we find

$$M_{out} = \frac{[P(0) + |P(\kappa)|] - [P(0) - |P(\kappa)|]}{[P(0) + |P(\kappa)|] + [P(0) - |P(\kappa)|]} = \frac{|P(\kappa)|}{P(0)}. \quad (2.35)$$

The quantity $|P(\kappa)|/P(0)$, which is the ratio of the output modulation to the input modulation, is called the *modulation transfer function* (MTF) of the linear system. It is an important and easily measurable characterization of the performance of the system. It is not, however, a complete characterization. To specify the system completely, we need to know *both* the MTF at all κ and the phase of the transfer function ϕ_p at all κ .

An important special case occurs when the PSF is symmetrical, i.e., $p(u) = p(-u)$. Then, from (B.9) in Appendix B, $P(\kappa)$ must be real and ϕ_p can take on only the values 0 and π . Even then a plot of MTF versus κ is not, strictly speaking, a complete description of the system, but the values of κ at which ϕ_p switches from 0 to π are usually fairly evident from the plot.

2.4 LINEAR FILTERS

Most linear systems in general and most imaging systems in particular degrade the input signal in some manner. For example, the MTF of most systems is less than unity at all frequencies (other than zero) and falls rapidly at the higher frequencies. This means that the high-frequency components, often the most important features of the input signal, have a reduced contrast in the output.

A second important source of degradation is noise. In a way, our treatment of linear systems to this point has been fraudulent because it implies that there is a unique correspondence between the output and the input. In fact, in any real system, a given input applied repeatedly will produce some random distribution of outputs. The input-output relation, (2.6) or (2.26), must be regarded as applying to the mean values of the signals. The source of this noise and methods of describing it mathematically are treated in detail in Chapters 3 and 10. For the present purposes, it is sufficient to be aware of its existence.

Because of these MTF and noise limitations, a linear system may not fulfill its goal. If it is a radiological imaging system, the output image may not show the detail necessary for an accurate diagnosis. In this case, improved performance can often be obtained by feeding the output of the system into a second linear system called a *filter*. The function of the filter is

to undo some of the degradation introduced by the primary system. Of course, the distinction between the primary system and the subsequent filter is merely a semantic one. We could equally well call the primary system, or any linear system, a filter.

2.4.1 Cascaded Linear Systems

In order to analyze the effects of the filter, it is first necessary to devise a description of two linear systems in cascade as shown in Fig. 2.4. Let $p_1(u)$ and $p_2(u)$ be the impulse responses of systems 1 and 2 respectively, and let $P_1(\kappa)$ and $P_2(\kappa)$ be the corresponding transfer functions. The output from system 1, which is simply $w_{in}(u) * p_1(u)$, is also the input to system 2. The output from system 2 is then given by

$$w_{out}(u) = [w_{in}(u) * p_1(u)] * p_2(u). \quad (2.36)$$

It is instructive to write these convolution integrals out in detail. Writing out the term in brackets yields

$$w_{out}(u) = \left(\int_{-\infty}^{\infty} p_1(u - u') w_{in}(u') du' \right) * p_2(u). \quad (2.37)$$

In order to write out the second convolution integral, it is necessary to introduce a second dummy variable, which we shall call u'' . We then have

$$w_{out}(u) = \int_{-\infty}^{\infty} du'' \int_{-\infty}^{\infty} du' p_1(u'' - u') w_{in}(u') p_2(u - u''). \quad (2.38)$$

This equation can be cast into a more useful form by a change of variables. Defining $u''' = u'' - u'$, we find

$$w_{out}(u) = \int_{-\infty}^{\infty} du' w_{in}(u') \left(\int_{-\infty}^{\infty} du''' p_1(u''') p_2[(u - u') - u'''] \right). \quad (2.39)$$

The term in the large parentheses is the convolution of p_1 and p_2 evaluated at a "shift" of $u - u'$. Thus we can write

$$w_{out}(u) = \int_{-\infty}^{\infty} du' w_{in}(u') p(u - u') = w_{in}(u) * p(u), \quad (2.40)$$

where

$$p(u) = p_1(u) * p_2(u). \quad (2.41)$$

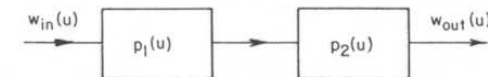


Fig. 2.4 Illustration of two linear systems in cascade.

In other words, the cascade of two linear systems is itself a linear system, and the overall impulse response is the convolution of the two constituent impulse responses.

We have also shown by this procedure that convolution is associative, for

$$w_{\text{out}}(u) = [w_{\text{in}}(u) * p_1(u)] * p_2(u) = w_{\text{in}}(u) * [p_1(u) * p_2(u)]. \quad (2.42)$$

The brackets are therefore superfluous.

The rather unwieldy derivation just presented becomes almost trivial if carried out in the frequency domain. If $w_{\text{in}}(\kappa)$ is the Fourier transform of the input signal, then the output from the first system is, by (2.26), simply $W_{\text{in}}(\kappa)P_1(\kappa)$. This product is also the input to the second system, and the final output is

$$W_{\text{out}}(\kappa) = W_{\text{in}}(\kappa)P_1(\kappa)P_2(\kappa) = W_{\text{in}}(\kappa)P(\kappa), \quad (2.43)$$

where

$$P(\kappa) = \mathcal{F}\{p(u)\} = \mathcal{F}\{p_1(u) * p_2(u)\}. \quad (2.44)$$

Equations (2.40) and (2.43) are thus completely equivalent.

2.4.2 Inverse Filters

We are now in a position to illustrate the use of a filter that has considerable conceptual importance, the so-called *inverse filter*. Suppose the goal of our filtering operation is to exactly compensate for the loss of modulation contrast introduced by the primary system. In other words, we require that $w_{\text{out}}(u) \equiv w_{\text{in}}(u)$. This would occur if the overall impulse response of the cascaded system were a Dirac delta function

$$p(u) = p_1(u) * p_2(u) = \delta(u), \quad (2.45)$$

since then we would have

$$w_{\text{out}}(u) = w_{\text{in}}(u) * \delta(u) = w_{\text{in}}(u). \quad (2.46)$$

It is presumed that $p_1(u)$ is known and that we must devise a filter [i.e., find a $p_2(u)$] so that (2.45) is satisfied. Equation (2.45) is thus a rather formidable integral equation for the unknown $p_2(u)$. Fortunately, the solution is quite simple in the frequency domain. A Fourier transform operation on (2.45) yields

$$P(\kappa) = P_1(\kappa)P_2(\kappa) = 1. \quad (2.47)$$

That the Fourier transform of $\delta(u)$ is unity follows immediately from the sifting property of the delta function, (2.3), and the definition of the Fourier transform.

Equation (2.47) says that if we choose the transfer function of the filter $P_2(\kappa)$ to be the reciprocal (inverse) of the transfer function of the primary system $P_1(\kappa)$, then the overall transfer function will have the ideal form, unity at all frequencies. The impulse response of the filter is then given by

$$p_2(u) = \mathcal{F}^{-1}\left\{\frac{1}{P_1(\kappa)}\right\} = \int_{-\infty}^{\infty} \left(\frac{1}{P_1(\kappa)}\right) \exp(2\pi i \kappa u) d\kappa. \quad (2.48)$$

An immediate difficulty with this seemingly innocuous solution is that there will *always* be some value of κ for which $P_1(\kappa) = 0$. At the very least, $P_1(\kappa)$ will approach zero as the frequency $\kappa \rightarrow \infty$, and in many cases of practical interest, $P_1(\kappa)$ will vanish at a number of finite frequencies as well. These zeros in the denominator will cause the integral in (2.48) to diverge, so the inverse filter is not physically realizable. This outcome should not be surprising since we imposed an impossible demand on the filter at the beginning, viz., (2.45). No physical system, cascaded or otherwise, can really have a delta-function impulse response since that would require an infinite bandwidth (uniform response for all frequencies). In a temporal system, infinite bandwidth means that no matter how rapidly the input varies, the output will exactly follow it. In an imaging system, infinite bandwidth means that arbitrarily small detail, even on the subatomic scale, could be faithfully reproduced.

However, some minor modifications of the integral in (2.48) can prevent the divergence and lead to a realizable filter that closely approximates the ideal inverse filter. We shall illustrate these modifications by two examples that will also be used to introduce some useful tricks in the manipulation of Fourier transforms.

2.4.3 An Example—Correction of Gaussian Blur

Suppose first that our primary system has a Gaussian impulse response of the form

$$p_1(u) = \exp(-\pi u^2/u_0^2), \quad (2.49)$$

where u_0 is a measure of the width of $p_1(u)$. [The full width of $p_1(u)$ at half its maximum value is given by $0.939u_0$.] The reason for the capricious insertion of a π in the definition of $p_1(u)$ is that it introduces a satisfying symmetry between p_1 and P_1 . More explicitly, as shown in Section B.3 of Appendix B, the Fourier transform of a Gaussian is also a Gaussian and, with the π , has the identical functional form, i.e.,

$$\mathcal{F}\{\exp(-\pi u^2)\} = \exp(-\pi \kappa^2). \quad (2.50)$$

This transform relation is not precisely the one needed in the present problem, but it can be finagled into the right form by use of the following result from Appendix B:

$$\mathcal{F}_M\{f(u/a)\} = |a|^M F(a\kappa), \quad (2.51)$$

where

$$\mathcal{F}_M\{f(u)\} = F(\kappa) \quad (2.52)$$

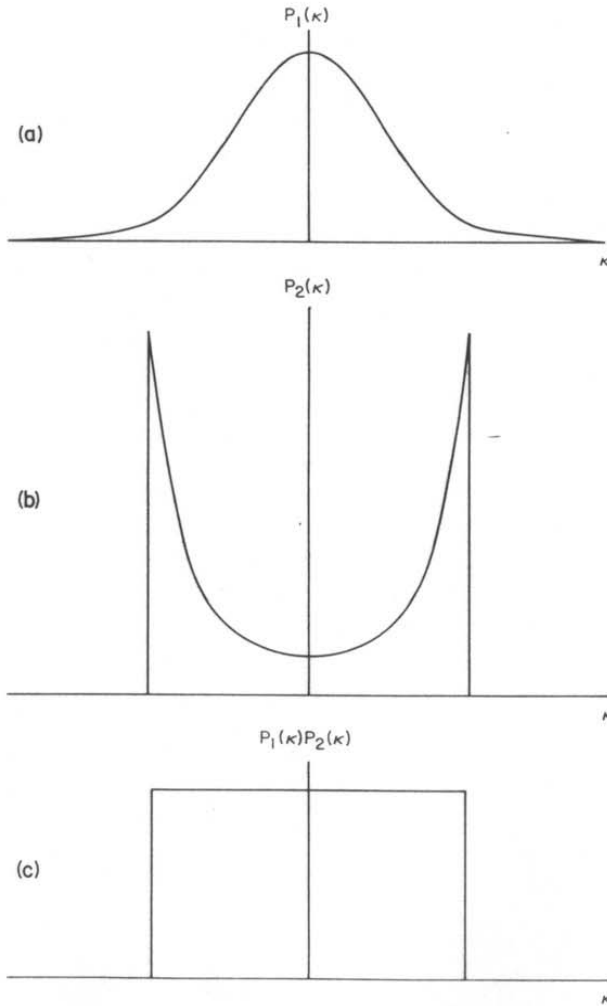


Fig. 2.5 (a) A Gaussian transfer function. (b) Inverse filter that exactly corrects for the Gaussian blur up to some cutoff frequency. (c) The final net transfer function, the product of (a) and (b).

and M is the dimensionality of u and κ . For simplicity, we shall now take M to be one. Then the transfer function of the primary system is found to be

$$P_1(\kappa) = u_0 \exp(-\pi u_0^2 \kappa^2). \quad (2.53)$$

Since we cannot hope to realize an exact inverse filter, let us somewhat arbitrarily decide to let the filter be exact up to some cutoff frequency κ_{\max} , and zero beyond that. Then our final filter transfer function (Fig. 2.5) is

$$P_2(\kappa) = \begin{cases} u_0^{-1} \exp(+\pi u_0^2 \kappa^2) & \text{if } |\kappa| < \kappa_{\max} \\ 0 & \text{if } |\kappa| > \kappa_{\max}. \end{cases} \quad (2.54)$$

The overall transfer function is

$$P(\kappa) = \begin{cases} 1 & \text{if } |\kappa| < \kappa_{\max} \\ 0 & \text{if } |\kappa| > \kappa_{\max}. \end{cases} \quad (2.55)$$

Functions of this form are so common that a special notation has been devised for them. We define

$$\text{rect}(x) = \begin{cases} 1 & \text{if } |x| < \frac{1}{2} \\ 0 & \text{if } |x| > \frac{1}{2}. \end{cases} \quad (2.56)$$

The one-dimensional Fourier transform of $\text{rect}(x)$ is easily calculated:

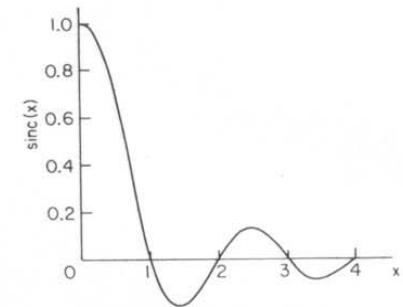
$$\mathcal{F}_1\{\text{rect}(x)\} = \int_{-1/2}^{1/2} \exp(-2\pi i \xi x) dx = \frac{\sin(\pi \xi)}{\pi \xi}. \quad (2.57)$$

Again, functions of this form are sufficiently common to justify a special notation. We define

$$\text{sinc } \xi \equiv \sin(\pi \xi)/\pi \xi. \quad (2.58)$$

This function is plotted in Fig. 2.6.

Fig. 2.6 Plot of the function $\text{sinc}(x) = \sin(\pi x)/\pi x$.



A simple convention permits the extension of these results to two or more dimensions. We define a two-dimensional rect function as a product of one-dimensional rect functions in Cartesian coordinates:

$$\text{rect}(\mathbf{r}/L) \equiv \text{rect}(x/L) \cdot \text{rect}(y/L), \quad (2.59)$$

and similarly for the sinc function

$$\text{sinc}(\mathbf{ar}) = \text{sinc}(ax) \cdot \text{sinc}(ay). \quad (2.60)$$

This vector notation will be avoided when it can cause confusion, as when the width of the function is different along the x and y axes, or when non-Cartesian coordinates are required. With these caveats, however, functions like $\text{sinc}(au)$ can be very convenient.

The general transform relations for rect and sinc functions may now be stated with the help of (2.51) as

$$\mathcal{F}_M\{\text{rect}(u/a)\} = |a|^M \text{sinc}(ak), \quad (2.61a)$$

and

$$\mathcal{F}_M\{\text{sinc}(u/b)\} = |b|^M \text{rect}(bk). \quad (2.61b)$$

Symmetrical results hold for the inverse transforms:

$$\mathcal{F}_M^{-1}\{\text{rect}(\kappa/a)\} = |a|^M \text{sinc}(au), \quad (2.61c)$$

$$\mathcal{F}_M^{-1}\{\text{sinc}(\kappa/b)\} = |b|^M \text{rect}(bu). \quad (2.61d)$$

Here a and b are arbitrary real constants and M is the dimensionality of u and κ .

In terms of these special functions, our overall transfer function, (2.55), may be rewritten

$$P(\kappa) = \text{rect}(\kappa/2\kappa_{\max}) \quad (2.62)$$

and, by use of (2.61), the overall impulse response is

$$p(u) = |2\kappa_{\max}|^M \text{sinc}(2\kappa_{\max}u). \quad (2.63)$$

We have now solved the problem of determining the inverse filter to be applied to a system with a Gaussian transfer function except for two aspects. We have not yet found a solution for the impulse response of the filter $p_2(u)$, and we have not fixed the parameter κ_{\max} . Although an explicit solution for $p_2(u)$ can be found, the problem has no redeeming social value and will not be pursued here.

The choice of κ_{\max} is of somewhat broader interest. At first blush it would appear that we should take κ_{\max} very large. This would make the sinc func-

tion in (2.63) very narrow so that $p(u)$ would be a good approximation to a delta function. The difficulty with this approach is that we have ignored noise so far. The filter transfer function (2.54) increases very rapidly with increasing frequency (see Fig. 2.5). This is precisely what is desired as far as the signal is concerned because it just compensates for the rapid decrease in $P_1(\kappa)$. However, the signal inevitably coexists with noise, and most commonly the noise does *not* exhibit a similar decrease at high frequencies. Rather, it has a very substantial high-frequency content that is greatly amplified by the action of the filter. Thus κ_{\max} must be limited in order to prevent the noise from overwhelming the signal at high frequencies. The mathematical tools needed for a more precise treatment of this question are developed in Chapter 3.

2.4.4 A Second Example

Now let us consider a slightly different inverse-filter problem. Suppose the primary system has an impulse response given by

$$p_1(u) = \text{rect}(u/2u_0), \quad (2.64)$$

where u_0 is now the full width at half-maximum (FWHM) of $p_1(u)$.

The primary system transfer function is

$$P_1(\kappa) = |2u_0|^M \text{sinc}(2u_0\kappa), \quad (2.65)$$

and a strict inverse filter transfer function would be the reciprocal of this expression. The difficulty is evident—there is an infinite set of frequencies for which the denominator of $P_2(\kappa)$ vanishes.

One solution is to simply not let the denominator vanish, i.e. to let

$$P_2(\kappa) = \begin{cases} 1/P_1(\kappa) & \text{if } |P_1(\kappa)| > \varepsilon \\ (1/\varepsilon) \text{sgn}[P_1(\kappa)] & \text{if } |P_1(\kappa)| < \varepsilon, \end{cases} \quad (2.66)$$

where ε , like κ_{\max} before it, is a parameter to be determined by noise considerations and $\text{sgn}(X) \equiv X/|X|$. There is little point in further analytical massaging of this problem, especially since we are not yet equipped to deal with the noise, but some representative results are plotted in Fig. 2.7.

One qualitative point to be noted from Fig. 2.7 is that the inverse filter has a bipolar (positive and negative valued) impulse response. The same observation holds true for all high-pass or sharpening filters. Low-pass or smoothing filters, on the other hand, can be (but do not have to be) positive definite.

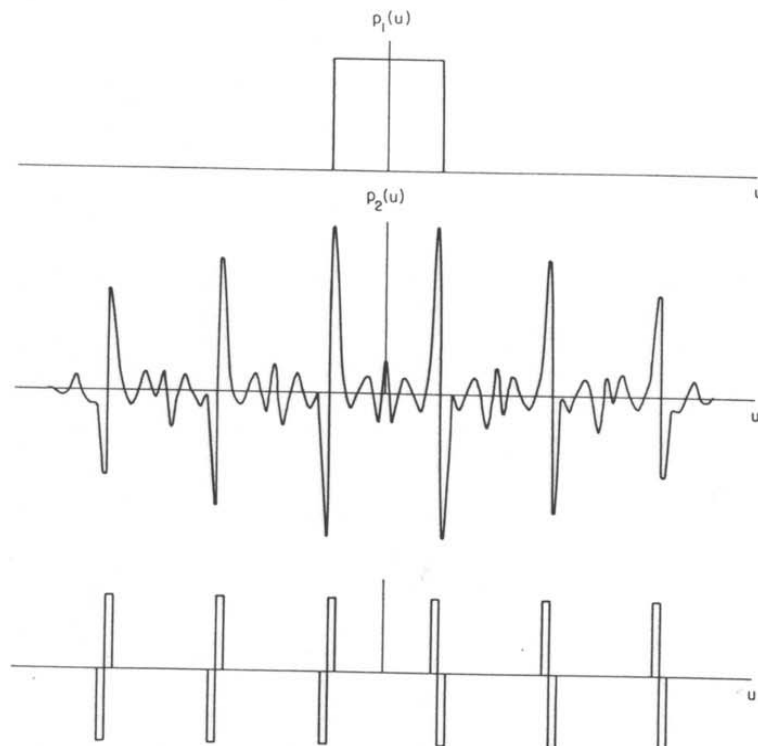


Fig. 2.7 Top: The rect function $p_1(u)$ to be corrected by inverse filtering. Center: The space-domain inverse filter $p_2(u)$ constructed according to (2.66). (see Honda and Tsujiuchi, 1975.) Bottom: A heuristic filter suggested by Swindell (1970) to approximate the inverse filter for a rect-function blur.

2.5 SAMPLING

In Section 2.4 we showed how to analyze linear filters and to calculate the overall system performance when a filter was included in the system. We have not yet said anything about the physical nature of the filter—it is still a “black box.” Part of the reason for this is that filters come in a wide variety of forms. An electrical filter may consist of inductors and capacitors, a tapped delay line, or a digital shift register. A spatial filter for images can be a camera with an appropriate pupil function, a laser system on an optical bench, or a digital computer with image scanning and display peripherals. One of the authors finds it very easy to implement a smoothing filter by removing his glasses.

Of these many possible incarnations of a linear filter, the digital versions are the ones with the greatest flexibility. Once a signal is in digital form, there is virtually no limit to the types of operations that can be performed on it. The impulse response or the transfer function can be specified at will. We are not even confined to linear operations; superior performance is often obtainable with nonlinear filters.

For these reasons digital filters are of great current interest in radiological imaging. Much of this book will be devoted to a discussion of filtering operations that are best performed digitally. But digital filters differ from their analog counterparts in one important respect: computers deal with discrete arrays of numbers, not continuous functions. In this section we develop the tools for dealing with this feature.

2.5.1 Statement of the Problem

Suppose we are dealing with an image recorded on a photographic transparency. A microdensitometer is used to measure the transmission of the film at an array of points with coordinates (x_n, y_m) given by

$$x_n = n\Delta, \quad y_m = m\Delta, \quad (2.67)$$

where n and m are the positive integers in the range $0-N$.

The microdensitometer has a finite measuring aperture which we assume to be a square of side ϵ . It responds not just to the transmission at the point (x_n, y_m) but to the average over an area ϵ^2 about the point. It thus produces a number a_{nm} given by

$$a_{nm} = \frac{1}{\epsilon^2} \int_{x_n-\epsilon/2}^{x_n+\epsilon/2} dx \int_{y_m-\epsilon/2}^{y_m+\epsilon/2} dy \cdot f(x, y), \quad (2.68)$$

where the function $f(x, y)$ represents the “true” transmission of the film, i.e., the value that would be measured with an infinitesimal aperture. Notice that $a_{nm} \rightarrow f(x_n, y_m)$ if $\epsilon \rightarrow 0$.

The array of numbers a_{nm} , along with a knowledge of the sampling interval Δ , can be used to construct another function $f_s(x, y)$ (Fig. 2.8) defined by

$$f_s(x, y) = \sum_{n,m} \frac{a_{nm}}{\epsilon^2} \text{rect}\left(\frac{x-x_n}{\epsilon}\right) \text{rect}\left(\frac{y-y_m}{\epsilon}\right). \quad (2.69)$$

The major concern of this section is how well the “sampled” function $f_s(x, y)$ represents the original function $f(x, y)$. There are two parts to this question: (1) What is the effect of the finite spacing between sample points? and (2) What is the effect of the finite sampling area ϵ^2 ? Surprisingly, we shall find that

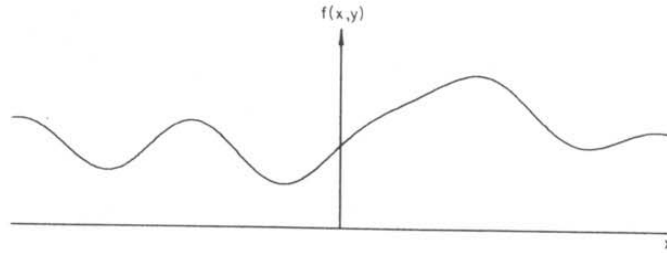


Fig. 2.8 A two-dimensional function $f(x, y)$ and its sampled version $f_s(x, y)$ along the x axis. The distance Δ is the distance between samples, while ϵ is the width of the measuring aperture.

there are some conditions under which $f_s(x, y)$ *exactly* represents $f(x, y)$ in the sense that we can find an exact prescription for reconstructing the latter from the former.

2.5.2 The Comb Function

As a mathematical preliminary, we introduce the comb function, defined as (Gaskill, 1978)

$$\text{comb}(x) = \sum_{n=-\infty}^{\infty} \delta(x - n). \quad (2.70)$$

As illustrated in Fig. 2.9, the comb function consists of an infinite array of unit impulses (delta functions) situated at integer values of the argument of the function. It is shown in Appendix B that the Fourier transform of a comb is also a comb, i.e.,

$$\mathcal{F}\{\text{comb}(u)\} = \text{comb}(\kappa). \quad (2.71)$$

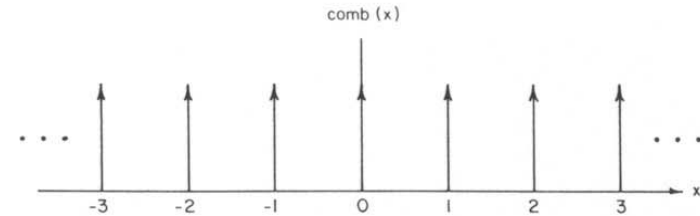


Fig. 2.9 Illustration of the function $\text{comb}(x)$. The arrows represent delta functions.

Note that this result holds in any number of dimensions. For example, if u is the two-dimensional variable \mathbf{r} with Cartesian components x and y , then $\text{comb}(u)$ is interpreted as a product in the same way as the sinc and rect functions, i.e.,

$$\begin{aligned} \text{comb}(u) &= \text{comb}(x)\text{comb}(y) \\ &= \sum_{n,m} \delta(x - n)\delta(y - m), \end{aligned} \quad (2.72)$$

and the two-dimensional Fourier transform has the same form,

$$\mathcal{F}_2\{\text{comb}(x)\text{comb}(y)\} = \text{comb}(\xi)\text{comb}(\eta) \equiv \text{comb}(\rho), \quad (2.73)$$

where ξ and η are the Cartesian components of the two-dimensional frequency vector ρ .

The array of rect functions in (2.69) is a good approximation to a comb function if ϵ is small. In fact, we can use the representation of a delta function as the limit of a rect (see Appendix A),

$$\lim_{\epsilon \rightarrow 0} (1/\epsilon^2) \text{rect}(x/\epsilon) \text{rect}(y/\epsilon) = \delta(x)\delta(y), \quad (2.74)$$

along with (A.14) and (A.17) to write (2.69) in the limit as

$$\begin{aligned} \lim_{\epsilon \rightarrow 0} f_s(x, y) &= \sum_{n,m} f(x_n, y_m) \delta(x - x_n) \delta(y - y_m) \\ &= f(x, y) \sum_{n,m} \delta(x - n\Delta) \delta(y - m\Delta) \\ &= f(x, y) \Delta^{-2} \text{comb}(x/\Delta) \text{comb}(y/\Delta). \end{aligned} \quad (2.75)$$

That the indices n and m run over an infinite range in the comb function and a finite range in $f_s(x, y)$ is of no concern if we agree that $f(x, y)$ vanishes outside the range defined by $0 < x < N\Delta$ and $0 < y < N\Delta$.

To avoid carrying along the limit, we define

$$f_{s0}(x, y) = \lim_{\epsilon \rightarrow 0} f_s(x, y). \quad (2.76)$$

2.5.3 The Whittaker–Shannon Sampling Theorem

To answer the first of the two questions posed above, the effect of the finite Δ , we must find a formula for determining $f(x, y)$ from $f_{s0}(x, y)$, a function that can be experimentally determined if ε can be made small enough (Goodman, 1968; Jerri, 1977). We begin by performing a Fourier transform on (2.75), with the result

$$F_{s0}(\xi, \eta) = \mathcal{F}_2\{f_{s0}(x, y)\} = F(\xi, \eta) ** [\text{comb}(\xi\Delta) \text{comb}(\eta\Delta)]. \quad (2.77)$$

This appears to be a step backward since a simple product is usually easier to deal with than a convolution. In this case, however, the convolution is very easy to handle since one of the functions is a sum of delta functions. The general result that is useful here is

$$F(\xi, \eta) ** [\delta(\xi - \xi_0) \delta(\eta - \eta_0)] = F(\xi - \xi_0, \eta - \eta_0), \quad (2.78)$$

which follows immediately from the definition of a convolution and the sifting property of delta functions.

Applying this general result to (2.77), we find

$$F_{s0}(\xi, \eta) = \Delta^{-2} \sum_{n=-\infty}^{\infty} \sum_{m=-\infty}^{\infty} F(\xi - n\Delta^{-1}, \eta - m\Delta^{-1}). \quad (2.79)$$

The factor Δ^{-2} in this equation arises because

$$\text{comb}(\xi\Delta) = \sum_n \delta(\xi\Delta - n) = \sum_n \delta[\Delta(\xi - n\Delta^{-1})] = \Delta^{-1} \sum_n \delta(\xi - n\Delta^{-1}),$$

and similarly for $\text{comb}(\eta\Delta)$.

The Fourier transform of the sampled function is thus a superposition of shifted replicas of the Fourier transform of the original function as illustrated in Fig. 2.10. This result is particularly useful when $F(\xi, \eta)$ is compact, so that the various replicas of $F(\xi, \eta)$ in (2.79) do not overlap appreciably. In fact, there is considerable theoretical interest in so-called *band-limited* functions whose Fourier transform vanishes identically outside a finite frequency region. The function $f(x, y)$ is said to be band-limited if

$$F(\xi, \eta) = 0 \quad \text{when} \quad |\xi| > \xi_{\max} \quad \text{or} \quad |\eta| > \eta_{\max}. \quad (2.80)$$

The rectangular region of area $2\xi_{\max} \cdot 2\eta_{\max}$ in the ξ - η plane is called the *region of support*.

The interest in band-limited functions is, strictly speaking, only theoretical because no function that describes a real physical system can truly be band-limited. It can be shown that a band-limited function *cannot* be space-limited also; if (2.80) is rigorously true, then $f(x, y)$ must extend to infinity in the x - y plane. Nevertheless, it is often a good approximation to treat phys-

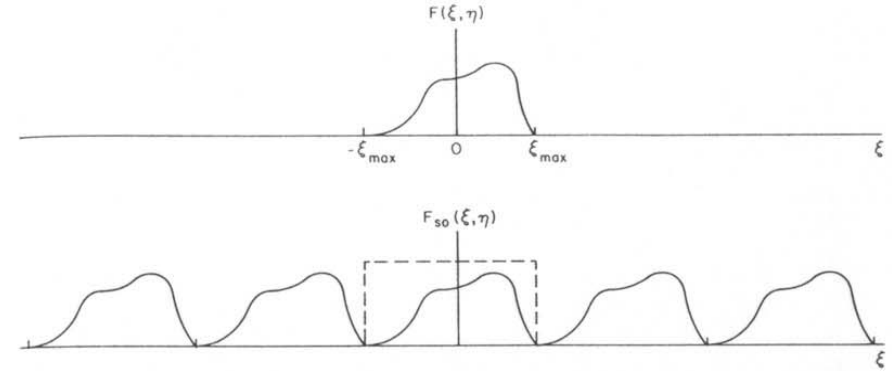


Fig. 2.10 Top: The Fourier transform of a band-limited function. Bottom: The Fourier transform of the sampled version of the function at top. Note that sampling in the space domain leads to replication in the frequency domain.

ical functions as band-limited if their transforms differ from zero by only an insignificant (whatever that means) amount outside a finite region of support. This gives rise to the designation *essentially band-limited*. We shall therefore assume that appropriate values of ξ_{\max} and η_{\max} can be chosen so that (2.80), while not rigorously true, is a valid approximation. Furthermore, for simplicity, we shall take

$$\xi_{\max} = \eta_{\max} = B/2. \quad (2.81)$$

The parameter B is called the one-dimensional *bandwidth* of the function.

Returning now to the discussion of (2.79), we see that the replicas of $F(\xi, \eta)$ do not overlap at all if $f(x, y)$ is a band-limited function and the sampling interval Δ satisfies

$$\Delta^{-1} \geq B. \quad (2.82)$$

If the equality holds in this relation, the sampling is said to be at the *Nyquist rate*. An equivalent statement to (2.82) is that the sampling rate must be at least twice the maximum frequency (ξ_{\max}) of the function being sampled. (Note that $1/\Delta$ is the sampling rate or frequency, and is measured in samples per unit length. B is a spatial frequency interval measured in cycles per unit length. Of course, both “samples” and “cycles” are pure numbers without dimensions.)

If this condition is satisfied, we can isolate a single replica of $F(\xi, \eta)$ from the infinite set of them by a low-pass filtering operation. More precisely, we then have

$$F_{s0}(\xi, \eta) \text{rect}(\xi\Delta) \text{rect}(\eta\Delta) = \Delta^{-2} F(\xi, \eta). \quad (2.83)$$

Applying (2.77) to the left-hand side of this equation, we find

$$\{F(\xi, \eta) ** [\text{comb}(\xi\Delta) \text{comb}(\eta\Delta)]\} \text{rect}(\xi\Delta) \text{rect}(\eta\Delta) = \Delta^{-2} F(\xi, \eta). \quad (2.84)$$

We now transform this equation back to the space (x - y) domain, remembering that the transform converts convolutions to multiplications and vice versa. We obtain

$$[f(x, y) \text{comb}(x/\Delta) \text{comb}(y/\Delta)] ** [\text{sinc}(x/\Delta) \text{sinc}(y/\Delta)] = \Delta^2 f(x, y). \quad (2.85)$$

To interpret this result, first note that

$$f(x, y) \text{comb}(x/\Delta) \text{comb}(y/\Delta) = \Delta^2 \sum_{n,m} f(x_n, y_m) \delta(x - x_n) \delta(y - y_m), \quad (2.86)$$

where x_n and y_m are given by (2.67), and $f(x, y)$ can be replaced by $f(x_n, y_m)$ since it is multiplied by $\delta(x - x_n) \delta(y - y_m)$. Since we are currently working in the limit $\varepsilon \rightarrow 0$, $f(x_n, y_m)$ is identical to a_{nm} [cf. (2.68)]. The Δ^2 on the right-hand side of (2.86) follows from algebra similar to that indicated in the discussion below (2.79). The convolution indicated in (2.85) is then easily performed with the help of the space-domain equivalent of (2.78). The final result is

$$\sum_{n,m} f(x_n, y_m) \text{sinc}[(x - x_n)/\Delta] \text{sinc}[(y - y_m)/\Delta] = f(x, y). \quad (2.87)$$

This equation is called the *Whittaker-Shannon sampling theorem* in two dimensions. It is illustrated graphically in Fig. 2.11.

This theorem is so important that it is perhaps worthwhile to rewrite the entire derivation, sans commentary, in terms of our arbitrarily dimensional

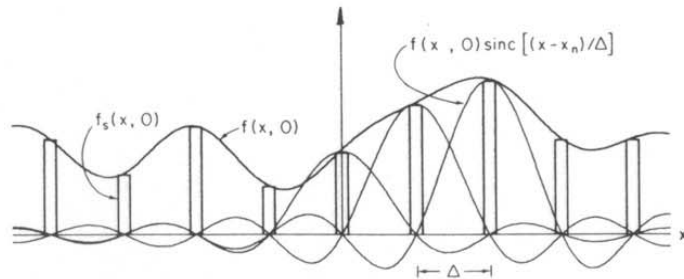


Fig. 2.11 Illustration of the sinc-function interpolation required by the Whittaker-Shannon theorem. This graph shows the components of (2.87) along the $y = 0$ axis. Although only three are shown here, a sinc function must be associated with each sample point. At a particular sample point, only one of the sinc functions has a nonzero value, but between sample points the whole infinite set of sinc functions is needed to rigorously interpolate the value of the function. In practice, however, a small number of sinc functions at each intermediate point is often sufficient.

variables u and κ . The key way stations on the road to the sampling theorem are

$$f_{s0}(u) \equiv \Delta^{-M} f(u) \text{comb}(u/\Delta), \quad (2.88)$$

$$F_{s0}(\kappa) = F(\kappa) * \text{comb}(\kappa\Delta), \quad (2.89)$$

$$F_{s0}(\kappa) \text{rect}(\kappa\Delta) = \Delta^{-M} F(\kappa), \quad (2.90)$$

$$[F(\kappa) * \text{comb}(\kappa\Delta)] \cdot \text{rect}(\kappa\Delta) = \Delta^{-M} F(\kappa), \quad (2.91)$$

$$[f(u) \cdot \text{comb}(u/\Delta)] * \text{sinc}(u/\Delta) = \Delta^M f(u), \quad (2.92)$$

$$\sum_{\substack{l=\text{all} \\ \text{sample points}}} f(u_l) \text{sinc}\left(\frac{(u - u_l)}{\Delta}\right) = f(u). \quad (2.93)$$

As before, M is the dimensionality of u and κ .

Several comments are in order concerning the sampling theorem we have just derived. First, it is an interpolation formula; it provides an *exact* way of reconstructing any band-limited function from its values at a discrete set of sample points. The self-consistency of this interpolation scheme can be checked by letting x and y be the coordinates of one of the sampling points, say $x = n'\Delta$ and $y = m'\Delta$. Then $\text{sinc}[(x - x_n)/\Delta]$ in (2.87) becomes $\text{sinc}(n' - n)$, which vanishes unless $n' = n$. Similarly the sinc function in y vanishes unless $m' = m$. Finally, since $\text{sinc}(0) = 1$, (2.87) reads $f(x_n, y_m) = f(x_n, y_m)$.

The second important comment about the theorem we derived is that it is by no means unique (Jerri, 1977). Many possible modifications occur at the step of (2.83) where we chose to isolate one of the replicas of $F(\xi, \eta)$ by a particular low-pass filter, the product of two rect functions that define a square of side Δ^{-1} in the ξ - η plane. We could have chosen a larger square or a rectangular region, provided that the region encompassed one and only one of the replicas. By the same token we could have chosen a circle, oval, or any other shape to isolate the term of interest. Each of these choices would lead to a different sampling theorem, all of which would be exact interpolation formulae for band-limited functions.

2.5.4 Aliasing

What happens if the Nyquist condition (2.82) is not satisfied? Then the replicas of $F(\xi, \eta)$ overlap each other and an exact reconstruction of $f(x, y)$ is not possible. Artificial structure, called *aliasing*, appears in the reconstruction of an image from an inadequate number of samples. We have all seen examples of aliasing on TV and in the newspapers. A television image is a

raster scan made up of a discrete set of scanning lines. The image is therefore sampled in one dimension. When a high-frequency object such as stripes on a performer's suit is displayed, a moiré pattern—aliasing—appears. Similarly, halftone reproductions of periodic patterns can evidence severe aliasing.

Since it is so important to have an adequate number of samples, it is worthwhile to state a simple rule explicitly. Consider an image contained in a square of side L in the x - y plane. If the sampling interval is Δ , a total of $(L/\Delta)^2$ samples will cover the whole image. But Δ must satisfy (2.82), the Nyquist condition. Therefore the number of sample points must be at least $(LB)^2$. This quantity, the product of the area of the object in the x - y plane and the area of its transform in the ξ - η plane, is called the two-dimensional *space-bandwidth product*. The extension of this idea to an arbitrary number of dimensions is straightforward.

2.5.5 Effect of the Measuring Aperture

The discussion of sampling to this point has considered only the $\varepsilon \rightarrow 0$ limit in which the measured numbers a_{nm} are identical with the sampled function $f(x_n, y_m)$. In the microdensitometer example, we could ensure that this approximation was valid by choosing a very small measuring aperture. In practice, however, this approach would be a very poor one because of noise. A very small aperture might view only a single photographic grain at a time so that the measured transmission would show wild point-to-point fluctuations even in a film that to the eye appeared uniformly exposed.

Fortunately, it is not difficult to modify the preceding theory to allow for nonzero values of ε . We simply define still another new function, $\bar{f}(x, y)$, by

$$\bar{f}(x, y) \equiv f(x, y) ** [\varepsilon^{-2} \text{rect}(x/\varepsilon) \text{rect}(y/\varepsilon)]. \quad (2.94)$$

It follows at once from the definition of a convolution that the measured transmission values, a_{nm} from (2.68), are related to this new function by

$$a_{nm} = \bar{f}(x_n, y_m). \quad (2.95)$$

Thus we know the values of \bar{f} at a discrete set of sample points. The Whittaker–Shannon theorem still applies since \bar{f} must be band-limited if f is, a result that follows from the frequency-domain counterpart of (2.94). Therefore we have sufficient information to reconstruct $\bar{f}(x, y)$ exactly, using (2.87) to interpolate between sample values.

The remaining problem is to go from $\bar{f}(x, y)$ to $f(x, y)$. We have already discussed this step in Section 2.4 since (2.94) describes a linear filtering operation. We merely have to find the inverse filter. Transforming (2.94) and

solving for $F(\xi, \eta)$, we find

$$F(\xi, \eta) = \frac{\bar{F}(\xi, \eta)}{\text{sinc}(\xi\varepsilon) \text{sinc}(\eta\varepsilon)}. \quad (2.96)$$

Everything on the right-hand side is known, so an inverse transform, if it exists, will suffice to find $f(x, y)$. A problem very similar to this one was discussed in Section 2.4. In that case, we concluded that an exact solution was hopeless because of the zeros of the sinc functions. In the present case, however, we have some additional information. We know that $F(\xi, \eta)$, and therefore also $\bar{F}(\xi, \eta)$, vanishes if $|\xi|$ or $|\eta|$ exceeds $B/2$. Furthermore, we shall usually have $\varepsilon \leq \Delta$ (the equality holds when the samples are just contiguous). Therefore, if the sampling satisfies the Nyquist condition, we have

$$|\xi\varepsilon| \leq B\varepsilon/2 \leq B\Delta/2 \leq \frac{1}{2}. \quad (2.97)$$

In other words, the argument of the sinc function is less than $\frac{1}{2}$ for all frequencies of interest. Thus, there are no zeros in the denominator and the inverse transform of (2.96) can be calculated with impunity. Indeed, $\text{sinc}(\frac{1}{2}) = 0.637$, so there is not even any appreciable noise amplification involved.

We have now solved the problem of determining the values of a band-limited function at all points from a discrete set of samples measured with a finite sampling aperture. To summarize the steps involved, we must first ensure that the sampling satisfies the Nyquist condition, then use the Whittaker–Shannon theorem to interpolate between samples, and finally apply a gentle inverse filter to correct for the aperture size.

2.6 OTHER MEASURES OF SHARPNESS

2.6.1 The Line Spread Function

So far we have discussed the spatial response of an imaging system in terms of its response to a point source, or point spread function (PSF). It is sometimes more convenient to use the response to a line source, or *line spread function* (LSF). One advantage of the LSF is that it is often easier to measure. When a radiation source is made so small that it approximates a point source, there may be very little radiation left. On the other hand, a source can be masked down with a thin slit to approximate a line source without such a severe loss in flux.

Mathematically, a line source oriented along the y axis may be described as a linear delta function:

$$w_{\text{in}}^{\text{line}}(x, y) = \delta(x). \quad (2.98)$$

We should think of $w_{in}^{line}(x, y)$ as a two-dimensional function that just happens to be independent of y . The line source may also be regarded as the integral of a point source, i.e.,

$$w_{in}^{line}(x, y) = \int_{-\infty}^{\infty} dy w_{in}^{\delta}(x, y) = \int_{-\infty}^{\infty} \delta(x) \delta(y) dy. \quad (2.99)$$

This equation enables us to determine the response to the line source at once. We know that the response to $w_{in}^{\delta}(x, y)$ is just $p(x, y)$. Since the system is linear the response $w_{out}^{line}(x, y)$ must be

$$l(x) \equiv w_{out}^{line}(x, y) = \int_{-\infty}^{\infty} dy w_{out}^{\delta}(x, y) = \int_{-\infty}^{\infty} dy p(x, y). \quad (2.100)$$

The line spread function $l(x)$ is thus the line integral of the point spread function $p(x, y)$ (Marchand, 1964).

There is also a simple relationship between the LSF and the MTF. The one-dimensional Fourier transfer of $l(x)$ is

$$\begin{aligned} \mathcal{F}_1\{l(x)\} &= \int_{-\infty}^{\infty} l(x) \exp(-2\pi i \xi x) dx \\ &= \int_{-\infty}^{\infty} dx \int_{-\infty}^{\infty} dy p(x, y) \exp(-2\pi i \xi x) dx \\ &= \left(\int_{-\infty}^{\infty} dx \int_{-\infty}^{\infty} dy p(x, y) \exp[-2\pi i(\xi x + \eta y)] \right)_{\eta=0} \\ &= P(\xi, 0). \end{aligned} \quad (2.101)$$

The Fourier transform of the LSF is thus the two-dimensional transfer function $P(\xi, \eta)$ evaluated on the line $\eta = 0$. A series of measurements of $l(x)$ at different orientations of the line will suffice to determine $P(\xi, \eta)$ along a series of radial lines through the origin in the ξ - η plane. Furthermore, if it is known a priori that $P(\xi, \eta)$ has circular symmetry so that it is the same on all radial lines, then a single measurement of the LSF fully characterizes the system.

2.6.2 The Edge Spread Function

An edge source is one that is bright on one side of a line and dark on the other. The response to an edge source, or *edge spread function* (ESF), is important because our eyes respond preferentially to edges in a scene.

Mathematically, an edge along the y axis is described by

$$w_{in}^{edge}(x, y) = \begin{cases} 1 & x > 0 \\ 0 & x < 0, \end{cases} \quad (2.102)$$

which can also be written

$$w_{in}^{edge}(x, y) = \int_{-\infty}^x \delta(x') dx' = \int_{-\infty}^x w_{in}^{line}(x', y) dx'. \quad (2.103)$$

Again, since the system is linear, the output must be

$$e(x) \equiv w_{out}^{edge}(x, y) = \int_{-\infty}^x w_{out}^{line}(x', y) dx' = \int_{-\infty}^x l(x') dx'. \quad (2.104)$$

Hence the edge spread function is the indefinite integral of the line spread function. Conversely,

$$l(x) = \frac{de(x)}{dx}. \quad (2.105)$$

is possible only in noncausal systems, we have

$$\begin{aligned} \mathbf{y}(t) * p(t) &= \int_{-\infty}^{\infty} \mathbf{y}(t') p(t - t') dt' \\ &= \int_{-\infty}^{\infty} \mathbf{y}(t') s(t' - t) = \mathbf{y}(t) \star s(t). \end{aligned} \quad (3.246)$$

Matched filtering is thus equivalent to correlating the data with the signal we are trying to detect.

Applications of matched filtering are discussed in Chapters 8 and 10.

Wiener-Helstrom Filter

An important variation on the Wiener filter was devised by Helstrom (1967). He considered the problem of estimating a signal that has been corrupted in two ways—by being convolved with a known filter function (usually a blurring or low-pass filter) and by the addition of signal-independent noise. The data to be filtered are of the form

$$\mathbf{y}(t) = [\mathbf{s}(t) * h(t)] + \mathbf{n}(t), \quad (3.247)$$

where $h(t)$ and the autocorrelation functions of $\mathbf{s}(t)$ and $\mathbf{n}(t)$ are presumed known. An estimate $\hat{\mathbf{s}}(t)$ of the signal is to be formed by filtering $\mathbf{y}(t)$ with a filter of impulse response $p(t)$. Again we choose the minimum mean-squared error as the optimality condition.

Helstrom showed that the optimum filter for this problem has a transfer function given by

$$P(v) = \frac{H^*(v)}{|H(v)|^2 + [S_n(v)/S_s(v)]}. \quad (3.248)$$

Several limits are of interest. First, note that if $h(t) = \delta(t)$, $H(v) = 1$, and the original Wiener filter is recovered. Second, if the signal-to-noise ratio is very good at all frequencies, such that $[S_n(v)/S_s(v)]^2 \ll |H(v)|^2$, then $P(v)$ reduces to an inverse filter, $P(v) = [H(v)]^{-1}$. Finally, if the SNR is very poor and both signal and noise are white, then $S_n(v)/S_s(v)$ is large and constant and the Wiener-Helstrom filter becomes a matched filter $P(v) \propto [H(v)]^*$.

4

Application of Linear Systems Theory to Radiographic Imaging

4.1 A GENERAL MODEL

It is our goal in this section to devise a simple model that can be used to describe transmission radiography, nuclear scanners, cameras with collimators, and cameras with pinholes. Such a model may seem an unlikely prospect since these systems are quite different in concept, intent, and performance. Nevertheless, as we shall see, the important features of all of them can be discussed within a common framework.

Consider first a simple nuclear pinhole imaging system with the geometry shown in Fig. 4.1. For now the object is assumed to be a planar gamma-ray emitter; the extension to three-dimensional objects can be made later. Additional simplifications concern the pinhole aperture and the detector, both of which are also assumed to be planar. In practice these are reasonable assumptions for very low-energy gamma rays that are absorbed in a small thickness of aperture or detector material. In general, a planar description of the aperture is not valid, since we need to know not only where the photon strikes the aperture plate, but also its angle of incidence to calculate the probability of its being transmitted through to the detector. However, if the absorption coefficient of the aperture material is so high that the aperture plate thickness can be made small compared to the pinhole diameter, then the angle of incidence becomes unimportant and a planar description of the aperture transmission suffices. Similarly, if the detector is either physically

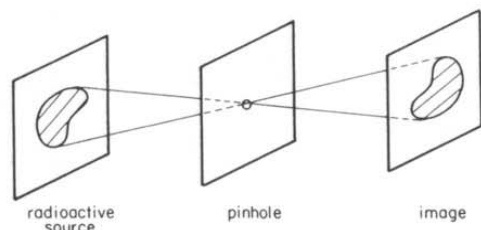


Fig. 4.1 Basic geometry for pinhole imaging of a planar emissive object.

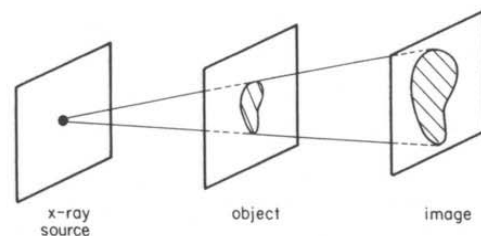


Fig. 4.2 Basic geometry for transmission radiography of a planar object.

thin, or so absorbing that all detection takes place in a thin surface layer, then again a planar description is adequate.

A simple transmission radiography system is shown in Fig. 4.2. The similarity to the pinhole system should be obvious. X rays are generated by electron bombardment of a planar anode, pass through a planar object and impinge on a planar detector. All three planes are assumed to be parallel, although in practice the x-ray anode is usually tipped at an angle to reduce

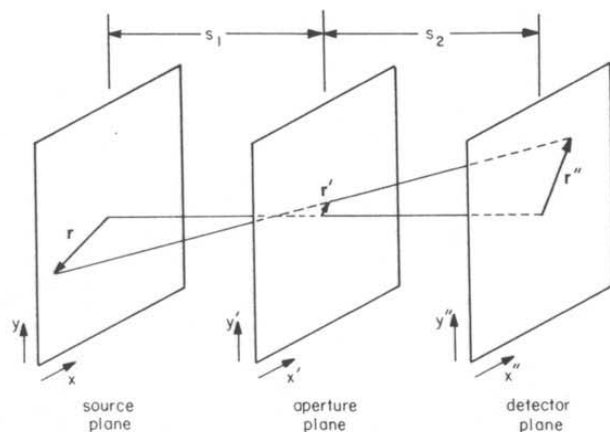


Fig. 4.3 The geometry of a general model for radiographic imaging.

the apparent focal spot size. There are some suspicious features of this model, particularly the planar object. Nevertheless we shall begin our analysis here and let the model gradually become more realistic (and hence more intractable).

The common features of the transmission radiography system and the pinhole camera, as we have modeled them, are thus a source plane, a transmitting or aperture plane, and a detector plane (see Fig. 4.3).

4.1.1 The Source

We describe the source by an *emission function* $f(\mathbf{r})$, where \mathbf{r} is a two-dimensional vector in the source plane. More precisely, $f(\mathbf{r})d^2r$ is the *mean* number of photons per unit time emitted into all space from an elemental area d^2r located at the point \mathbf{r} . It is important to note that $f(\mathbf{r})$ should really be a statistical quantity. If we observed the system for a finite time T , we would *not* expect to find exactly $Tf(\mathbf{r})d^2r$ photons emitted from the element d^2r during the observation. Indeed, the very notion of an infinitesimal number of photons, obtained by multiplying the infinitesimal area d^2r by any finite number, is a contradiction in terms. However, if we repeated the observation many times, or considered an ensemble of many identical x-ray systems, then $Tf(\mathbf{r})d^2r$ would represent the average value of all our observations. Deviations from this mean behavior are the subject of Chapter 10; in this chapter all results are to be interpreted as statistical averages.

Of course, $Tf(\mathbf{r})d^2r$ represents the mean number of photons emitted from d^2r during the interval T only if $f(\mathbf{r})$ is independent of time. Otherwise a time integral is required. Time-varying sources are occasionally desirable, as with pulsed x-ray tubes, or unavoidable, as with rapidly decaying isotopes. But a time integral would be a distinct nuisance here, so we simply assume it away and take $f(\mathbf{r})$ to be constant in time.

One final comment on $f(\mathbf{r})$ concerns the directional character of the photon emission. If the source is a radionuclide distribution there is no reason to assume any directionality at all. Photons are emitted with equal probability in all directions. The situation is very different with x-ray sources. The bremsstrahlung has a definite preferred orientation which depends on electron energy, angle of electron incidence, and target material. Clearly such complexity is incompatible with a simple model, so once again we ignore it (for now) and consider only isotropic emitters.

4.1.2 The Detector

Having described an elemental source, let us now consider an elemental detector of area d^2r'' , where \mathbf{r}'' is the two-dimensional position vector in the

detector plane. This elemental detector subtends a solid angle $d\Omega$ from the source, given by

$$d\Omega = \frac{d^2r'' \cdot \cos \theta}{R^2}. \quad (4.1)$$

Referring to Fig. 4.4, we see that R is the distance from source element to detector element and θ is the angle between the normal to the detector surface and the line of sight from source to detector. From simple geometry, we find

$$R = (s_1 + s_2)/\cos \theta, \quad (4.2)$$

so that

$$d\Omega = \frac{\cos^3 \theta}{(s_1 + s_2)^2} d^2r''. \quad (4.3)$$

If there were no absorbing material in the space between the source plane and the detector plane, the detector would intercept a fraction $d\Omega/4\pi$ of the radiation emitted from any source element since a full sphere subtends 4π steradians. The mean number of photons per unit time emitted by the area element d^2r in the source plane and intercepted by the area element d^2r'' in the detector plane would then be given by

$$f(\mathbf{r}) d^2r \frac{d\Omega}{4\pi} = f(\mathbf{r}) \frac{\cos^3 \theta}{4\pi(s_1 + s_2)^2} d^2r d^2r''. \quad (4.4)$$

Of course, not all of the photons intercepted by the detector are detected. And even when a photon is detected, its location \mathbf{r}'' cannot be measured with absolute accuracy. The detector should, in principle, be considered as an integral part of the imaging system. For now, however, we are concentrating on other portions of the system and may assume an ideal detector. This restriction will be lifted shortly.

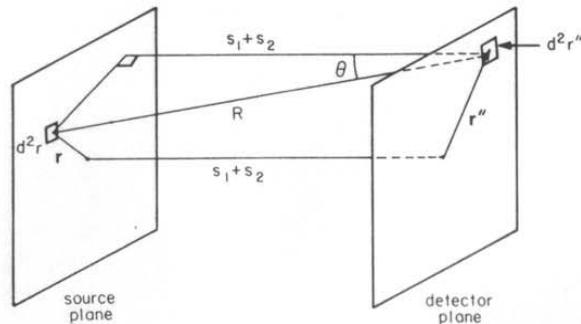


Fig. 4.4 Diagram for solid-angle calculation (aperture plane not shown).

4.1.3 The Transmitting Plane

Our description of the system is nearly complete. We have only to account for the transmitting plane situated between the source and detector. This is easily accomplished since we shall deal only with rays that travel in straight lines; scattered radiation is the subject of another chapter. Thus a ray emanating from the point \mathbf{r} and striking the detector at \mathbf{r}'' must have passed through the central plane at a specific point \mathbf{r}' (see Fig. 4.3). We shall denote by $g(\mathbf{r}')$ the transmittance of the central plane at the point \mathbf{r}' . In other words, $g(\mathbf{r}')$ is the fraction of the incident photons that is transmitted through the central plane.

We can now write down an expression for the density of detected photons $h(\mathbf{r}'')$, defined so that $h(\mathbf{r}'') d^2r''$ is the mean number of photons intercepted by the detector area d^2r'' in a time T . This definition says nothing about where the photon came from, so an integration over the source plane is required:

$$h(\mathbf{r}'') d^2r'' = \frac{T d^2r''}{4\pi(s_1 + s_2)^2} \int_{\text{source}} d^2r \cos^3 \theta f(\mathbf{r}) g(\mathbf{r}'). \quad (4.5)$$

Dimensionally, $h(\mathbf{r}'')$ is a *fluence* as defined in Appendix D. However, the term fluence is more appropriate to a beam of moving particles than to a static pattern of recorded photons. Thus, we shall call $h(\mathbf{r}'')$ a *photon density* rather than a fluence.

The vector \mathbf{r}' can be eliminated in terms of \mathbf{r} and \mathbf{r}'' . Inspection of the geometry of Fig. 4.3 reveals that

$$\frac{\mathbf{r}' - \mathbf{r}}{s_1} = \frac{\mathbf{r}'' - \mathbf{r}'}{s_2} \quad (4.6)$$

or

$$\mathbf{r}' = \frac{s_2}{s_1 + s_2} \mathbf{r} + \frac{s_1}{s_1 + s_2} \mathbf{r}'' = a\mathbf{r} + b\mathbf{r}'', \quad (4.7)$$

where

$$a = s_1/(s_1 + s_2) \quad (4.8)$$

and

$$b = s_2/(s_1 + s_2) = 1 - a. \quad (4.9)$$

Some care must be taken in interpreting (4.6) or (4.7) since \mathbf{r} , \mathbf{r}' , and \mathbf{r}'' are all two-dimensional vectors defined in different planes. If \mathbf{r} has Cartesian components (x, y) and \mathbf{r}' has components (x', y') , then by $\mathbf{r}' - \mathbf{r}$ we mean a two-dimensional vector with components $(x' - x, y' - y)$. The z dimension

does not influence this vector difference. The three-dimensional distance R is not simply $|\mathbf{r} - \mathbf{r}''|$, but is given by

$$R = [|\mathbf{r} - \mathbf{r}''|^2 + (s_1 + s_2)^2]^{1/2} \\ = [(x - x'')^2 + (y - y'')^2 + (s_1 + s_2)^2]^{1/2}. \quad (4.10)$$

In spite of this complication, the notation is still intended to be suggestive. Note that if all figures are drawn so that the radiation goes from left to right, then the letters representing the important functions (f , g , and h) progress from left to right, the number of primes on the coordinates (\mathbf{r} , \mathbf{r}' , \mathbf{r}'') increases from left to right, and the designations for both absolute spacings (s_1 and s_2) and relative spacings (a and b) increase from left to right.

Equation (4.5) now becomes

$$h(\mathbf{r}'') d^2 r'' = C d^2 r'' \int_{\text{source}} d^2 r \cos^3 \theta f(\mathbf{r}) g(a\mathbf{r}'' + b\mathbf{r}), \quad (4.11)$$

where

$$C = T[4\pi(s_1 + s_2)^2]^{-1}. \quad (4.12)$$

This equation is still rather complicated since θ is a function of \mathbf{r} and \mathbf{r}'' . However, we shall often be interested in systems, where $s_1 + s_2$ is large compared to $|\mathbf{r}|$ or $|\mathbf{r}''|$. In those cases it is a good approximation to take $\theta \approx 0$ and $\cos^3 \theta \approx 1$. We are then left with

$$h(\mathbf{r}'') \approx C \int_{\text{source}} d^2 r f(\mathbf{r}) g(a\mathbf{r}'' + b\mathbf{r}), \quad (4.13)$$

where the factor $d^2 r''$, originally inserted for didactic purposes, has been dropped from both sides of the equation.

4.1.4 Reduction to a Convolution

Equation (4.13) now resembles a convolution integral. To exploit this resemblance, let us define a new variable \mathbf{r}_0'' , given by

$$\mathbf{r}_0'' = -b\mathbf{r}/a \quad (4.14)$$

and scaled versions of f and g by

$$\tilde{f}(\mathbf{r}_0'') = f(\mathbf{r}) = f(-a\mathbf{r}_0''/b) \quad (4.15)$$

and

$$\tilde{g}(\mathbf{r}_0'') = g(a\mathbf{r}_0''). \quad (4.16)$$

We then have

$$g(a\mathbf{r}'' + b\mathbf{r}) = g(a\mathbf{r}'' - a\mathbf{r}_0'') = \tilde{g}(\mathbf{r}'' - \mathbf{r}_0''). \quad (4.17)$$

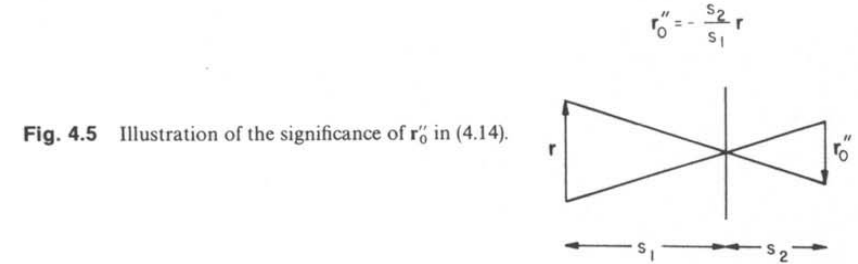


Fig. 4.5 Illustration of the significance of \mathbf{r}_0'' in (4.14).

The significance of the variable \mathbf{r}_0'' is illustrated in Fig. 4.5. Multiplication of the vector \mathbf{r} , which is measured in the source plane, by $-b/a$ (or, equivalently, $-s_2/s_1$) is the same as projecting it through a point in the aperture plane to the image plane. Similar geometric interpretations may be attached to the scaled functions \tilde{f} and \tilde{g} . As Fig. 4.6 shows, $g(a\mathbf{r}'')$ is wider than $g(\mathbf{r}'')$ since the scale factor a is less than one. The scaled function $\tilde{g}(\mathbf{r}'')$ may be thought of as the original aperture function $g(\mathbf{r}')$ projected from a point in the source plane to the image plane. By the same token, $\tilde{f}(\mathbf{r}'')$ is the original source function projected through a point in the aperture plane to the image plane. The tilde will always imply projection to the image plane.

After these manipulations (4.13) may be written

$$h(\mathbf{r}'') = \left(\frac{a}{b}\right)^2 C \int_{\infty} d^2 r_0'' \tilde{f}(\mathbf{r}_0'') \tilde{g}(\mathbf{r}'' - \mathbf{r}_0'') \\ = (a/b)^2 C \tilde{f}(\mathbf{r}'') ** \tilde{g}(\mathbf{r}''). \quad (4.18)$$

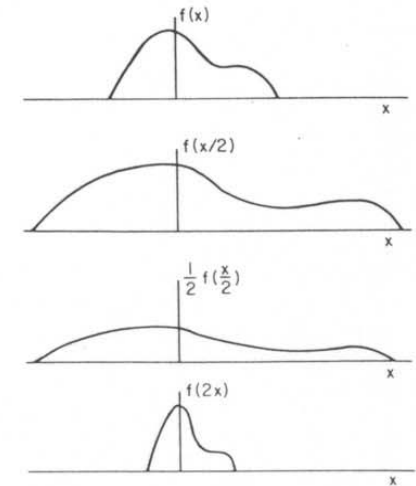


Fig. 4.6 Illustration of scaled functions. Note that $f(ax)$ is wider than $f(x)$ if $a < 1$ and narrower than $f(x)$ if $a > 1$. Note also that $af(ax)$ and $f(x)$ yield the same value when integrated over x .

(The domain of the \mathbf{r}'_0 integration may be taken as the entire two-dimensional space, indicated by the subscript ∞ on the integral sign, since f , and hence \tilde{f} , vanishes outside a finite area.) In other words, the detected photon density may be thought of as the output of a two-dimensional linear system with input \tilde{f} and impulse response proportional to \tilde{g} . As in any linear system, a frequency-domain description is very useful. A straightforward two-dimensional Fourier transform of (4.18) yields

$$\mathcal{F}_2\{h(\mathbf{r}'')\} = H(\boldsymbol{\rho}'') = (a/b)^2 C \tilde{F}(\boldsymbol{\rho}'') \tilde{G}(\boldsymbol{\rho}''), \quad (4.19)$$

where $\boldsymbol{\rho}''$ is the spatial frequency vector conjugate to \mathbf{r}'' in the image plane. The transform on the right of this equation may be evaluated in terms of the original source and transmission functions f and g by use of the scaling relation (B.94):

$$\tilde{F}(\boldsymbol{\rho}'') = \mathcal{F}_2\{f(-a\mathbf{r}''/b)\} = (b^2/a^2)F(-b\boldsymbol{\rho}''/a) \quad (4.20)$$

and

$$\tilde{G}(\boldsymbol{\rho}'') = \mathcal{F}_2\{g(a\mathbf{r}'')\} = (1/a^2)G(\boldsymbol{\rho}''/a). \quad (4.21)$$

Our final result is then

$$H(\boldsymbol{\rho}'') = (C/a^2)F(-b\boldsymbol{\rho}''/a)G(\boldsymbol{\rho}''/a). \quad (4.22)$$

Application of the basic equations (4.18) and (4.22) to various imaging systems is the subject of the remainder of this chapter.

4.2 PINHOLE IMAGING

A pinhole camera is the simplest possible imaging system. Its major features can be determined from elementary geometry without resort to the elaborate mathematics unveiled in the Section 4.1. Our goal in this section is therefore not to use the mathematics to understand the pinhole camera, but rather the reverse—to use the pinhole camera to demystify the mathematics.

4.2.1 Geometrical Treatment

Consider an ideal pinhole aperture that is perfectly transmitting over a small circular region of diameter d'_{ph} , and perfectly opaque elsewhere, so that

$$g(\mathbf{r}') = \text{circ}(2r'/d'_{ph}) = \begin{cases} 1 & \text{if } 2r'/d'_{ph} < 1 \\ 0 & \text{if } 2r'/d'_{ph} > 1, \end{cases} \quad (4.23)$$

where $r' \equiv |\mathbf{r}'|$. The prime on d'_{ph} indicates that it is measured in the \mathbf{r}' plane.

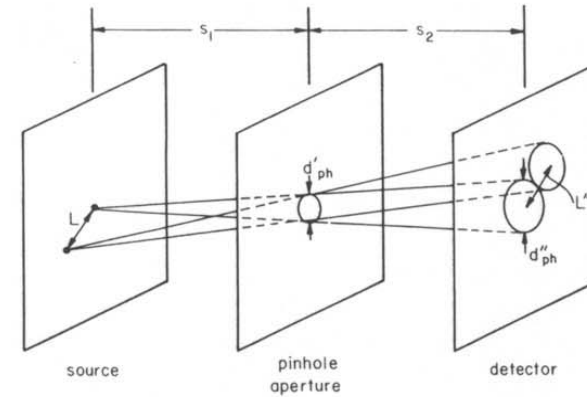


Fig. 4.7 Diagram illustrating the calculation of the point spread function for pinhole imaging.

Suppose that the source is a single emissive point. Then, since the rays must travel in straight lines, the image consists of a collection of detected photons confined to a circular region of diameter d''_{ph} (see Fig. 4.7). By comparing similar triangles, we see that

$$d''_{ph} = d'_{ph} \frac{s_1 + s_2}{s_1} = \frac{d'_{ph}}{a}. \quad (4.24)$$

Note that the value of d''_{ph} is completely independent of the position of the source. No matter what the projection angle θ is, the circular pinhole always projects to an undistorted circular image provided the aperture plane is parallel to the detector plane. In brief, the system is shift-invariant.

If we consider two point sources a distance L apart, inspection of Fig. 4.7 shows that the centers of their images in the \mathbf{r}'' plane are separated by a distance L'' given by

$$L'' = L(s_2/s_1) = L(b/a). \quad (4.25)$$

Furthermore, the image is inverted; we say that the pinhole camera has a magnification of $-b/a$ ($= -s_2/s_1$).

4.2.2 Analytical Treatment

The results of the geometrical analysis also follow easily from (4.18). We describe a point source at the location \mathbf{r}_s as a delta function, i.e.,

$$f^\delta(\mathbf{r}) = K \delta(\mathbf{r} - \mathbf{r}_s), \quad (4.26)$$

where the superscript δ reminds us we are dealing with a point source, and K is the *total* number of photons per unit time emitted by the source. Note that this definition is consistent with the interpretation of $\tilde{f}(\mathbf{r})$ as the number of emitted photons per unit time per unit area since, by the definition of the delta function,

$$\int_{\text{source}} f^{\delta}(\mathbf{r}) d^2r = K \int_{\text{source}} \delta(\mathbf{r} - \mathbf{r}_s) d^2r = K. \quad (4.27)$$

The scaled functions $\tilde{f}(\mathbf{r})$ and $\tilde{g}(\mathbf{r})$ that appear in (4.18) may be written

$$\tilde{f}^{\delta}(\mathbf{r}'') = K \delta[(-a\mathbf{r}''/b) - \mathbf{r}_s] = K(b^2/a^2) \delta[\mathbf{r}'' + (b\mathbf{r}_s/a)] \quad (4.28)$$

and

$$\tilde{g}(\mathbf{r}'') = \text{circ}(2a\mathbf{r}''/d'_{\text{ph}}), \quad (4.29)$$

where use has been made of the scaling property of delta functions, (A.37), to obtain the right-hand form of (4.28). Equation (4.18) itself is now

$$\begin{aligned} h^{\delta}(\mathbf{r}'') &= KC \int_{\infty} d^2r'_0 \delta\left(\mathbf{r}''_0 + \frac{b\mathbf{r}_s}{a}\right) \text{circ}\left(\frac{2a|\mathbf{r}'' - \mathbf{r}''_0|}{d'_{\text{ph}}}\right) \\ &= KC \text{circ}\left(\frac{2a|\mathbf{r}'' + (b\mathbf{r}_s/a)|}{d'_{\text{ph}}}\right). \end{aligned} \quad (4.30)$$

We next seek to persuade the reader that the circ function in this equation describes the same magnified pinhole image that we deduced on geometrical grounds. First, note that the center of the circ function is located at the value of \mathbf{r}'' that makes the argument of the function zero. This occurs when $\mathbf{r}'' = -b\mathbf{r}_s/a$, in agreement with the geometrical picture. Let \mathbf{r}''_s be defined as the coordinate of the center of the circ function, i.e.,

$$\mathbf{r}''_s = -b\mathbf{r}_s/a. \quad (4.31)$$

The circ function of (4.30) vanishes unless its argument is less than 1, or

$$|\mathbf{r}'' - \mathbf{r}''_s| < \frac{d'_{\text{ph}}}{2a} = \frac{d'_{\text{ph}}}{2} \frac{s_1 + s_2}{s_1}. \quad (4.32)$$

This inequality will hold provided \mathbf{r}'' lies within a circle of diameter d'_{ph}/a ($=d''_{\text{ph}}$) centered at \mathbf{r}''_s . Thus, once again the geometrical result is confirmed.

Equation (4.30) not only gives the right functional form for $h(\mathbf{r}'')$, but also the right magnitude. To see this, note that the disk of diameter d'_{ph}/a in the detector plane subtends a solid angle Ω (as seen from the source plane) given by

$$\Omega = \frac{\pi(d'_{\text{ph}}/a)^2}{4(s_1 + s_2)^2}. \quad (4.33)$$

The total number of detected photons in time T is thus the total number emitted KT times the fractional solid angle $\Omega/4\pi$. But $h(\mathbf{r}'')$ is the detected photon *density*. Within the disk region, $h(\mathbf{r}'')$ is the total number collected divided by the area of the disk, i.e.,

$$h^{\delta}(\mathbf{r}'') = \frac{KT\Omega/4\pi}{\pi(d'_{\text{ph}}/a)^2/4} = \frac{KT}{4\pi(s_1 + s_2)^2}, \quad [|\mathbf{r}'' - \mathbf{r}''_s| < d'_{\text{ph}}/2a], \quad (4.34)$$

which, with the definition of C from (4.12), is in perfect accord with (4.30).

4.2.3 Resolution

Either the geometrical or the mathematical approach can be used to determine the resolution distance of the system, i.e., the minimum resolvable spacing of two point sources. The only real problem is specifying what we mean by “minimum resolvable.” One possibility would be to adopt the full width at half-maximum (FWHM) of the PSF as our resolution criterion. In the present case, the PSF as measured in the image plane is a uniform disk of diameter d''_{ph} ; the FWHM of this function is therefore also d''_{ph} . This criterion would thus not count two points as resolved unless their separation was such that there was no overlap at all between the two disk images. This may seem to be an overly stringent condition. Surely an observer would have no difficulty in asserting that two points were present if the centers of their images were separated by, say $\frac{1}{2}d''_{\text{ph}}$. Indeed, many writers adopt this condition in discussing the resolution of a pinhole camera. Nevertheless, we believe that the FWHM criterion is defensible in most practical circumstances. Unfortunately, the defense rests largely on noise considerations and must therefore be postponed to Chapter 10. For now, we simply adopt the FWHM criterion without real justification. The reader who objects to this choice can sprinkle around factors of order unity to taste.

Our criterion thus says that the centers of the *images* of the two points must be separated by d''_{ph} for the points to be resolved. Of more interest, however, is how far apart the *points themselves* must be. In other words, we are more concerned with the PSF scaled to the actual size of the object than with the PSF as it appears in the image plane. This is an easy scaling since we have already determined that the magnification of the pinhole camera is $-b/a$ (or $-s_2/s_1$). For two points to be barely resolved (by the FWHM criterion), they must be separated in the object plane by a distance δ_{ph} , given by

$$\delta_{\text{ph}} = d''_{\text{ph}}a/b = d'_{\text{ph}}/b = d'_{\text{ph}}(s_1 + s_2)/s_2. \quad (4.35)$$

To be more formal about it, the PSF of the pinhole camera is the measured point-source image $h^{\delta}(\mathbf{r}'')$ rescaled to account for the magnification,

and normalized to unit source strength, i.e.,

$$\begin{aligned} \text{PSF}_{\text{ph}} &= p_{\text{ph}}(\mathbf{r} - \mathbf{r}_s) = K^{-1}(b/a)^2 h^{\delta}(\mathbf{r}'')|_{\mathbf{r}'' = -b\mathbf{r}/a} \\ &= C \left(\frac{b}{a}\right)^2 \text{circ}\left(\frac{2b|\mathbf{r} - \mathbf{r}_s|}{d'_{\text{ph}}}\right), \end{aligned} \quad (4.36)$$

which has a FWHM of d'_{ph}/b , in agreement with (4.35). The scaling must involve the amplitude as well as the lateral dimensions of the function. The leading factor of b^2/a^2 in (4.36) is required so that the total number of photons will be conserved, i.e., the integral of $p_{\text{ph}}(\mathbf{r})$ over the \mathbf{r} plane will be identical to the integral of $h^{\delta}(\mathbf{r}'')$ over the \mathbf{r}'' plane. The reader may verify that the constants in (4.36) are reasonable by showing that the integral of $p_{\text{ph}}(\mathbf{r})$ is simply $\Omega T/4\pi$. Notice that $p_{\text{ph}}(\mathbf{r})$ has units of time per length squared, so that $p_{\text{ph}}(\mathbf{r}) ** f(\mathbf{r})$ represents the mean number of collected photons per unit area in the rescaled image.

4.2.4 Modulation Transfer Function

The MTF of the pinhole camera may be found, as usual, by Fourier transforming the PSF. The details of the transform are given in Appendix B;

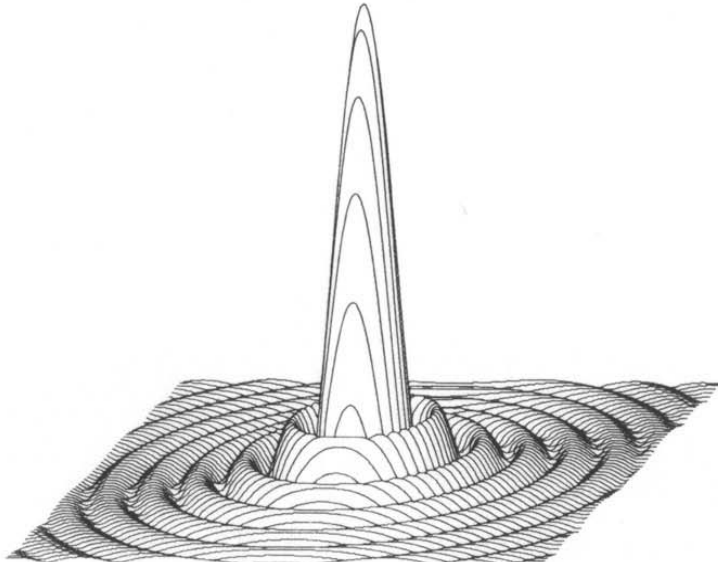


Fig. 4.8 Isometric plot of the function $2J_1(x\rho)/x\rho$.

by (B.114), the result is

$$\text{MTF}_{\text{ph}} = \frac{|P_{\text{ph}}(\rho)|}{P_{\text{ph}}(0)} = \frac{|2J_1(\pi d'_{\text{ph}}\rho/b)|}{\pi d'_{\text{ph}}\rho/b} \quad (4.37)$$

where, as in Chapter 2, ρ is the magnitude of the two-dimensional spatial-frequency vector, and $J_1(\cdot)$ is the first-order Bessel function of the first kind. The function $2J_1(x\rho)/x\rho$ is the two-dimensional, circularly symmetric counterpart of the sinc function defined in (2.58). It is sometimes referred to as a “Besinc” function or, in the southwest, as a “sombbrero” function (see Fig. 4.8). However, since the usage is not yet standardized, we shall refrain from giving this function a name.

4.2.5 The Image Detector

Since the PSF (or the transfer function) is a complete specification of a linear, shift-invariant system, it would seem that we have completed the analysis of the pinhole camera. However, we have not yet included the effects of the image detector. The problem is closely akin to the cascaded linear systems discussed in Chapter 2. The first system is the image-forming pinhole aperture. Its input is the two-dimensional source density $f(\mathbf{r})$, and its output is the photon density incident on the detector $h(\mathbf{r}'')$. If the detector were ideal, its output would be just proportional to $h(\mathbf{r}'')$. Real detectors, however, further degrade the image and must be treated as linear systems in their own right.

Cascaded linear systems are most easily analyzed in the frequency domain. The input signal to the detector system is thus given by $H(\rho'')$, the Fourier transform of $h(\mathbf{r}'')$. The transfer function of the detector will be denoted by $D(\rho'')$, so the detector output is simply $D(\rho'')H(\rho'')$. With the aid of (4.22), this becomes

$$D(\rho'')H(\rho'') = (C/a^2)D(\rho'')F(-b\rho''/a)G(\rho''/a). \quad (4.38)$$

This equation may appear strange at first since the three functions on the right all have different scale factors. But bear in mind that we are really interested in how a particular spatial-frequency component in the object is affected by the cascaded system. It is quite irrelevant to us whether the final image is displayed at a large scale or a small one. What we must do, therefore, is to rewrite this equation so that the object transform $F(\rho)$ appears without any scale factors. The coefficient of $F(\rho)$ will then be the overall transfer function of the cascaded system, referred back to the original object scale.

To accomplish this, we merely let $\rho = -b\rho''/a$ in (4.38). The result is

$$D(-a\rho/b)H(-a\rho/b) = (C/a^2)D(-a\rho/b)F(\rho)G(-\rho/b). \quad (4.39)$$

Reading off the coefficient of $F(\rho)$, we obtain the transfer function of the total system, pinhole plus detector,

$$TF_{\text{tot}} = P_{\text{tot}}(\rho) = (C/a^2)D(-a\rho/b)G(-\rho/b). \quad (4.40)$$

Note that no modification of the leading constant is necessary when rescaling functions in the frequency domain. The central ordinate theorem (B.96) guarantees that the left-hand side of (4.40), when transformed back to the space domain, will have the same spatial integral as before scaling. The factor of b^2/a^2 introduced into (4.36) is automatically taken into account in (4.40).

An inverse transform now gets us back to the space domain and to an expression for the PSF of the total system:

$$PSF_{\text{tot}} = p_{\text{tot}}(\mathbf{r}) = (C/a^2)\mathcal{F}_2^{-1}\{D(-a\rho/b)G(-\rho/b)\}. \quad (4.41)$$

This function can be broken down into its component parts by use of the convolution theorem (B.52). We then obtain

$$p_{\text{tot}}(\mathbf{r}) = p_{\text{ph}}(\mathbf{r}) ** p_{\text{det}}(\mathbf{r}), \quad (4.42)$$

where $p_{\text{ph}}(\mathbf{r})$ is the PSF due to the pinhole alone [cf. (4.36)] as given by

$$p_{\text{ph}}(\mathbf{r}) = (C/a^2)\mathcal{F}_2^{-1}\{G(-\rho/b)\} = (Cb^2/a^2)g(-b\mathbf{r}). \quad (4.43)$$

Similarly, $p_{\text{det}}(\mathbf{r})$ is the contribution of the detector to the overall PSF and is given by

$$p_{\text{det}}(\mathbf{r}) = \mathcal{F}_2^{-1}\{D(-a\rho/b)\} = (b/a)^2 d(-b\mathbf{r}/a). \quad (4.44)$$

Note that p_{det} has dimensions of (area) $^{-1}$ even though p_{ph} has dimensions of time per area. Note also that an ideal detector, for which $D(\rho'') = 1$ at all frequencies, leads to $p_{\text{det}}(\mathbf{r}) = \delta(\mathbf{r}) \equiv (b^2/a^2)\delta(-b\mathbf{r}/a)$.

It is also important to keep in mind that we are referring all PSFs to a common scale—the scale of the original object in the \mathbf{r} plane. The notation $p_{\text{det}}(\mathbf{r})$ does *not* mean the PSF of the detector; it means the contribution of the detector to the overall PSF as measured in the object plane. The PSF of the detector, as measured in the detector plane, is just $d(\mathbf{r}'')$. The scale factors in (4.44) serve to project this function through a point in the aperture plane to the object or source plane. On the other hand, we had to originally have $h(\mathbf{r}'')$ expressed in the \mathbf{r}'' plane in order to regard it as the input to the detector. Only after the cascading expressed in (4.38) was it correct to rescale the results to the \mathbf{r} plane.

4.2.6 Design Considerations

We next inquire how these results might be used to design a pinhole camera. The parameters at our disposal are the spacings s_1 and s_2 and the diameter of the pinhole. It is assumed that the size and MTF of the detector

are fixed, and that we must image an object of a specified size. Within these constraints, we must optimize the resolution and the gamma-ray collection efficiency of the pinhole camera.

The first constraint to apply is the required size of the object field (field of view, or FOV for short). If the detector is circular with diameter d''_{det} , and the object lies within a circular region of diameter d_{ob} , which is large compared to δ_{ph} , then the entire object can be imaged if

$$d''_{\text{det}} \geq \frac{s_2}{s_1} d_{\text{ob}} = \frac{b}{a} d_{\text{ob}}. \quad (4.45)$$

In other words, the magnified object must fit on the detector.

Equation (4.45) is not the only constraint on s_1/s_2 ; the resolution distance δ_{ph} also depends on that parameter. Inspection of (4.35) shows that δ_{ph} takes on its minimum of d'_{ph} when $s_1/s_2 \rightarrow 0$.

Of course, (4.35) was derived on the assumption of an ideal detector, but the same conclusion follows when a realistic detector is considered—the best resolution is obtained with the smallest s_1/s_2 . Qualitatively, the degradation due to the detector is least serious when the image is greatly magnified since then the width of the detector PSF is a small fraction of the image size. More quantitatively, our goal is to make the detector's contribution to the transfer function, $D(-a\rho/b)$ in (4.40), as large as possible. Since D will generally decrease as the spatial frequency is increased, we must make the magnitude of the argument of D , i.e., the quantity $| -a\rho/b |$, as small as possible at all frequencies. This can occur only if a/b is small. To restate the argument in the space domain, the function $d(-b\mathbf{r}/a)$ in (4.44) falls to one-half its peak value when the argument of the function equals some specified value, call it $r_{1/2}$. The FWHM of $p_{\text{det}}(\mathbf{r})$ is then given by $2(a/b)r_{1/2}$. The parameter $r_{1/2}$ is a characteristic of the detector and presumably beyond our control. The only way to minimize the FWHM of $p_{\text{det}}(\mathbf{r})$ is thus to minimize a/b .

Of course, a/b cannot be made arbitrarily small, since then (4.45) would be violated and the FOV would be inadequate. The smallest allowed a/b is the value for which (4.45) becomes an equality rather than an inequality, i.e., $a/b = d_{\text{ob}}/d''_{\text{det}}$.

To this point, we have fixed a/b , or s_1/s_2 , but not s_1 and s_2 separately; the total source-detector distance $s_1 + s_2$ is still a free parameter. It is clear from (4.3) that $s_1 + s_2$ should be small in order to efficiently collect photons [note that the factor $(s_1 + s_2)^{-2}$ appears either explicitly or implicitly though the constant C in all of our imaging equations]. There is, however, a penalty to be paid if $s_1 + s_2$ is made too small. The problem lies in the obliquity factor $\cos^3 \theta$ that last appeared in (4.11). The subsequent treatment was based on the approximation $\cos^3 \theta \approx 1$, an approximation that breaks down for large objects and small spacings. The planar model for the aperture can also break down under these same conditions. The upshot is that gamma rays

are collected less efficiently from the periphery of the object plane than from the center; a uniform object produces an image that is less intense at the edges (see Fig. 4.9). The system designer must decide how much of this shading can be tolerated and set $s_1 + s_2$ accordingly.

An additional consideration affecting the choice of $s_1 + s_2$ arises when three-dimensional objects are considered. In that case, s_1 is a variable specifying depth within the object. If the pinhole is close to the surface of the object, then the magnification and the collection efficiency will both vary rapidly with depth in the object. Therefore, both lateral spatial dimensions and intensities will be distorted, possibly confusing the diagnostic process. A value judgment, not readily amenable to quantification, is required to set tolerable bounds on these distortions.

The last parameter we must consider is d'_{ph} . Once again a trade-off is involved—a large d'_{ph} will increase collection efficiency but degrade spatial resolution. In general, determination of just where to set this trade-off is an extraordinarily difficult problem that ultimately comes down to the psychophysical question: Does the human observer perform better with a sharp, noisy image or with a blurred but less noisy one? We do not propose to answer this question in this book, although some possible approaches to the

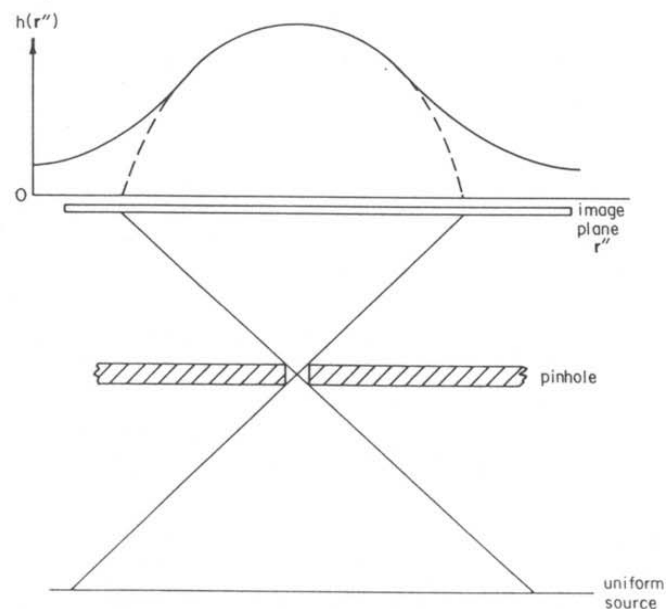


Fig. 4.9 Illustration of image shading due to obliquity and vignetting in the pinhole camera. Solid line: obliquity alone. Dashed line: obliquity plus vignetting. For this drawing, the pinhole material is assumed to be perfectly opaque.

problem are briefly discussed in Chapter 10. Even if we confined our attention to purely physical measures of image quality, we could not give a very complete discussion at this point because we have not yet included noise in our formulation. Therefore, we shall postpone the discussion of this problem until Chapter 10. For now, it is sufficient to bear in mind that radiological images in general, and nuclear pinhole images in particular, are almost always severely limited by the small number of detected photons. Collection efficiency is of paramount importance.

4.3 TRANSMISSION RADIOGRAPHY

It is a simple matter to recast the pinhole-imaging equations into a form applicable to transmission radiography. The basic difference is that in the pinhole case the source function $f(\mathbf{r})$ represents the object being imaged, and the aperture function $g(\mathbf{r}')$ is under the control of the system designer. The reverse is true in transmission imaging where $g(\mathbf{r}')$ represents the object and $f(\mathbf{r})$ is the more-or-less controllable focal spot of the x-ray tube (Ter-Pogossian, 1967; Rossmann, 1968, 1969; Doi, 1965; Doi and Rossman, 1975).

4.3.1 Disk Focal Spot

To accentuate the similarity, let us suppose that the focal spot is a uniform, emissive disk of diameter d_{fs} , i.e.,

$$f(\mathbf{r}) = f_0 \text{circ}(2r/d_{fs}), \quad (4.46)$$

where f_0 is the emission density (photons per unit area per unit time) within the disk region (see Fig. 4.10).

To find the PSF of the system, we must consider the input to be a point object described by

$$g^{\delta}(\mathbf{r}') = \delta(\mathbf{r}' - \mathbf{r}'_1). \quad (4.47)$$

where \mathbf{r}'_1 is the location of the point in the \mathbf{r}' plane. This input function may offend the reader's intuition somewhat since $g(\mathbf{r}')$ is supposed to represent a transmission, which is a dimensionless number in the range 0–1. The unit-impulse transmission $g^{\delta}(\mathbf{r}')$, on the other hand, has dimensions of $(\text{length})^{-2}$ (see Appendix A) and has a peak value of infinity rather than unity. If a mental picture is required, one can imagine a pinhole aperture whose area is allowed to approach zero while the exposure time is increased in inverse proportion to the area, so that the total x-ray flux transmitted through the pinhole during the exposure is constant. This metaphor corresponds to the notion of a point source, which we viewed as a very small, very bright source.

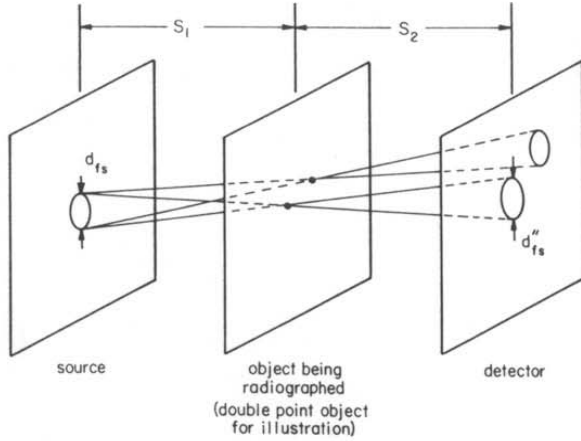


Fig. 4.10 Diagram illustrating the calculation of the point spread function for transmission radiography with a disklike focal spot.

In the limit, it became infinitesimally small and infinitely bright in such a way that the total number of emitted photons remained constant. In the transmission case, the object becomes “infinitely transmissive” over an infinitesimal area.

We can now see that the PSF of the transmission radiography system, as measured in the detector plane, is simply the pinhole image of the focal spot. Substituting (4.46) and (4.47) into (4.13), we find

$$\begin{aligned} h^\delta(\mathbf{r}'') &= C \int_{\text{source}} d^2r f_0 \text{circ}\left(\frac{2r}{d_{fs}}\right) \delta(a\mathbf{r}'' + b\mathbf{r} - \mathbf{r}'_1) \\ &= \left(\frac{C}{b^2}\right) f_0 \text{circ}\left[\frac{2|a\mathbf{r}'' - \mathbf{r}'_1|}{bd_{fs}}\right] \\ &= \left(\frac{C}{b^2}\right) f_0 \text{circ}\left[\frac{2|\mathbf{r}'' - (\mathbf{r}'_1/a)|}{bd_{fs}/a}\right]. \end{aligned} \quad (4.48)$$

This equation describes a uniform disk image of diameter d''_{fs} , given by

$$d''_{fs} = d_{fs} \frac{s_2}{s_1} = d_{fs} \frac{b}{a}. \quad (4.49)$$

The disk is centered at $\mathbf{r}'' = \mathbf{r}'_1/a = \mathbf{r}'_1(s_1 + s_2)/s_1$; the magnification m_i is therefore $(s_1 + s_2)/s_1$. Note that the magnification is always greater than one and that it is a positive number. The image inversion encountered in the pinhole camera does not occur here.

Two points are said to be just resolvable, on the FWHM criterion, if the center-to-center spacing of their images is equal to d''_{fs} . As in the pinhole

camera case, we then scale the spacing back to the object plane (in this case, the \mathbf{r}' plane) by dividing by the magnification. Formally, we set $d''_{fs} = r'_1/a$ and solve for r'_1 , which is then identified as the resolution distance δ'_{fs} . (The subscript fs indicates that we are considering only the contribution of the focal spot to the resolution, and the prime shows that the resolution is measured in the \mathbf{r}' plane.) The result is

$$\delta'_{fs} = d_{fs} b = d_{fs} \frac{s_2}{s_1 + s_2}. \quad (4.50)$$

The symmetry between (4.50) and (4.35) should not be overlooked. One is obtained from the other by transposing the object dimension and the resolution-determining system parameter (d_{fs} or d'_{ph}).

4.3.2 General Analysis

We may generalize our description to include an arbitrary focal-spot distribution and also include the effect of the detector by again using (4.38). This time, however, $G(\rho''/a)$ represents the object. Since we are interested in how a particular spatial-frequency component in the object is affected by the system, we must rescale (4.38) so that $G(\rho')$ appears on the right-hand side. To accomplish this, we let $\rho' = \rho''/a$ in (4.38). The result is

$$D(a\rho')H(a\rho') = (C/a^2)D(a\rho')F(-b\rho')G(\rho'). \quad (4.51)$$

This is the transmission-imaging counterpart of (4.39). The coefficient of $G(\rho')$ is the overall transfer function of the system:

$$TF_{\text{tot}} = P_{\text{tot}}(\rho') = \frac{C}{a^2} D(a\rho')F(-b\rho'). \quad (4.52)$$

Returning to the space domain, we find that the overall PSF is given by

$$\begin{aligned} \text{PSF}_{\text{tot}} &= p_{\text{tot}}(\mathbf{r}') = \frac{C}{a^2} \mathcal{F}_2^{-1}\{D(a\rho')F(-b\rho')\} \\ &= p_{fs}(\mathbf{r}') ** p_{\text{det}}(\mathbf{r}'), \end{aligned} \quad (4.53)$$

where $p_{fs}(\mathbf{r}')$ is the PSF due to the focal spot alone,

$$p_{fs}(\mathbf{r}') = \frac{C}{a^2} \mathcal{F}_2^{-1}\{F(-b\rho')\} = \left(\frac{C}{a^2 b^2}\right) f\left(\frac{-\mathbf{r}'}{b}\right). \quad (4.54)$$

The detector contribution to the PSF is

$$p_{\text{det}}(\mathbf{r}') = \mathcal{F}_2^{-1}\{D(a\rho')\} = (1/a^2) d(\mathbf{r}'/a). \quad (4.55)$$

Note that the scaling factors in this equation are different from those in the pinhole case [cf. (4.44)] even though the same symbol $p_{\text{det}}(\mathbf{r}')$ is used. Note also that both p_{fs} and p_{tot} have dimensions of $(\text{length})^{-4}$, in contrast to p_{ph} which had dimensions of time per $(\text{length})^2$. However, p_{fs} is to be convolved with a dimensionless quantity, a transmission, to get the image h , while p_{ph} is to be convolved with a source density having dimensions $(\text{length})^{-2}$ $(\text{time})^{-1}$. Thus in both cases, h has dimensions $(\text{length})^{-2}$ and represents the mean number of photons per unit area in the image.

4.3.3 Design Considerations

With these basic equations, we are now in a position to discuss the design tradeoffs in transmission imaging. The first thing we shall discover is that there is an optimum magnification even if there is no limitation imposed by the finite detector size. This is in marked contrast to the pinhole camera case where we found that the magnification should be as large as possible. A large magnification (small s_1/s_2) served to minimize the widths of both $p_{\text{ph}}(\mathbf{r})$ and $p_{\text{det}}(\mathbf{r})$. In the transmission case, on the other hand, a large magnification ameliorates the detector contribution to the overall blur but exacerbates the focal spot contribution. To see this, recall that the magnification m_t is given by

$$m_t = \frac{1}{a} = \frac{1}{1-b}, \quad (4.56)$$

or

$$b = 1 - \frac{1}{m_t} = \frac{m_t - 1}{m_t}. \quad (4.57)$$

Therefore,

$$p_{\text{fs}}(\mathbf{r}') \propto f\left(\frac{-m_t \mathbf{r}'}{m_t - 1}\right), \quad (4.58)$$

and

$$p_{\text{det}}(\mathbf{r}') \propto d(m_t \mathbf{r}'). \quad (4.59)$$

The width of $p_{\text{fs}}(\mathbf{r}')$ is the smallest when the coefficient of \mathbf{r}' in the argument of (4.58) is the largest, which occurs when $m_t = 1$. This corresponds to the "contact print" limit when the detector is in direct contact with the object being radiographed. In that case the size of the focal spot is irrelevant and a sharp shadow is always cast on the detector. Of course, this limit may not be physically possible, as when the object of interest lies deep within the patient's body. Nor is it necessarily desirable to have a contact print when the detector limitations are considered. Just as in the pinhole case, a large magnification serves to minimize the width of $p_{\text{det}}(\mathbf{r}')$, a result that should be readily evident from (4.59).

An explicit solution for the optimum magnification is possible when both the detector and the focal spot can be represented as Gaussian functions—always a convenient mathematical artifice and occasionally a realistic one as well. The problem is easiest in the frequency domain. Therefore let us assume that

$$D(\rho'') \propto \exp[-\pi(\rho''/\rho_d'')^2] \quad (4.60)$$

and

$$F(\rho) \propto \exp[-\pi(\rho/\rho_f)^2], \quad (4.61)$$

where ρ_d'' and ρ_f are characteristic widths of the MTF of the detector and focal spot, respectively. From (4.52), we find for the overall MTF,

$$\text{MTF}_{\text{tot}} = \frac{|P_{\text{tot}}(\rho')|}{P_{\text{tot}}(0)} = \exp[-\pi(a\rho'/\rho_d'')^2] \exp[-\pi(b\rho'/\rho_f)^2] \quad (4.62)$$

By virtue of (4.56) and (4.57),

$$\text{MTF}_{\text{tot}} = \exp\left[-\pi\rho'^2\left(\frac{1}{(m_t\rho_d'')^2} + \frac{(m_t - 1)^2}{m_t^2\rho_f^2}\right)\right]. \quad (4.63)$$

The width of MTF_{tot} will be an extremum if

$$\frac{d}{dm_t} \left[\frac{1}{(m_t\rho_d'')^2} + \frac{(m_t - 1)^2}{m_t^2\rho_f^2} \right] = 0, \quad (4.64)$$

which has the solution

$$m_t^{\text{opt}} = 1 + (\rho_f/\rho_d'')^2. \quad (4.65)$$

It is easily verified that the extremum corresponds to a maximum width for MTF_{tot} and hence an optimum configuration as implied by the superscript.

The behavior of (4.65) in two limits is of interest. First, note that a very large focal spot ($\rho_f \rightarrow 0$) requires the contact-print configuration, $m_t = 1$. Second, a very poor detector ($\rho_d'' \rightarrow 0$) requires large magnification.

As with the pinhole camera, an additional design consideration arises when we consider the finite detector area. This problem is relatively unimportant when x-ray film or a film-screen system is used since a large area is easy to obtain. With x-ray image intensifiers, on the other hand, the detector area is very limited, which is unfortunate since the MTF is also relatively poor and (4.65) shows that a large magnification is desirable.

4.3.4 Realistic Focal Spots

While some x-ray tubes do have focal spots that approximate Gaussian functions, they are the exception rather than the rule. A more realistic focal spot is illustrated in Fig. 4.11, and its associated MTF is shown in Fig. 4.12.

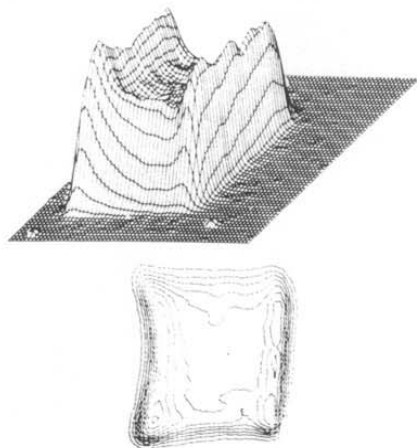


Fig. 4.11 Pinhole image of an actual x-ray tube focal spot, isometric and contour representations. (From Wagner *et al.*, 1974.)

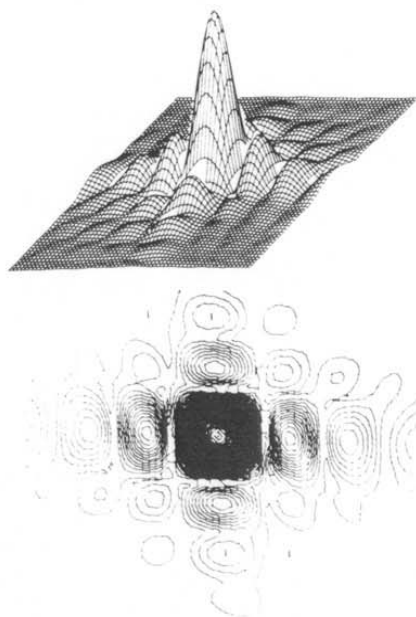


Fig. 4.12 MTF obtained with the focal spot shown in Fig. 4.11, isometric and contour representations (From Wagner *et al.*, 1974.)

Many attempts have been made to reduce these complicated functions to single numbers—something akin to our d_{fs} in (4.46) or p_f in (4.61). Frequently, manufacturers and medical physicists will differ by as much as a factor of 3 when asked to specify the “effective focal spot size” of a given x-ray tube. We do not propose to enter this rather sterile debate. Suffice it to say that the complete PSF or transfer function is required to properly specify the characteristics of the focal spot; any lesser description provides less information.

One qualitative difference between the Gaussian focal spot and the realistic one in Fig. 4.11 concerns the phase of the transfer function. A Gaussian transfer function has zero phase at all spatial frequencies, which is seldom true with realistic focal spots. The existence of these phase shifts is revealed in a radiograph of a bar target as shown in Fig. 4.13. The origin of



Fig. 4.13 Radiograph of a bar target illustrating phase shifts. Note that the modulation of the bars vanishes at 4.5 lp/mm, and that the phase of the modulation at lower frequencies is opposite that at the higher frequencies. (Courtesy of Meryll Frost.)

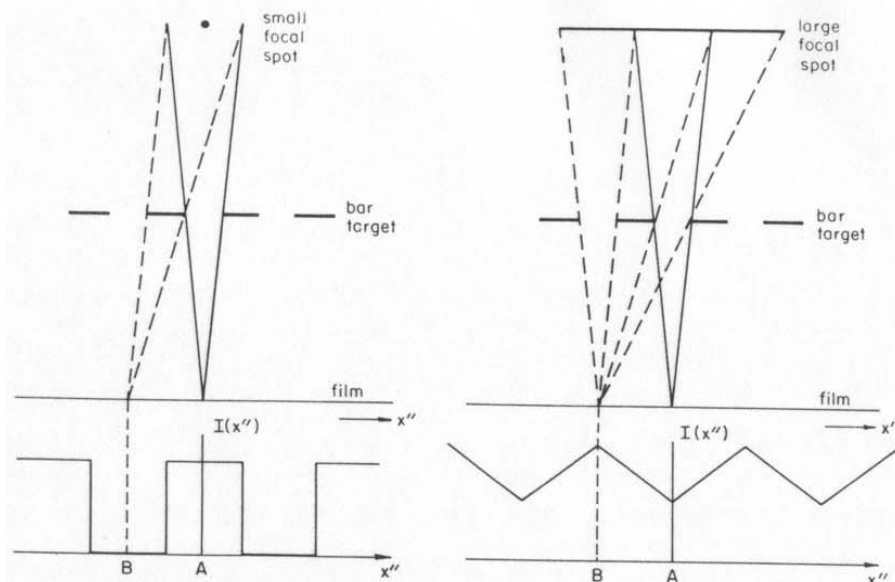


Fig. 4.14 Geometric explanation of the origin of the phase shifts seen in Fig. 4.13. At left, a small focal spot gives a sharp shadow and 100% modulation. The maximum intensity is at point A, and the intensity at point B is zero. At right, point A "sees" only half as much of the large square focal spot as point B does. Thus, the intensity at B is twice as large as at A, which is now a *minimum* instead of a maximum.

the reversals can be seen from the geometric construction given in Fig. 4.14.

Our discussion of transmission radiography to this point is by no means complete. We are, however, approaching the limits of what can be learned from a linear, shift-invariant model. We therefore conclude this section here, but we shall return to the subject of transmission imaging in Section 4.8 where the various factors that invalidate our simple model are discussed.

4.4 SCANNERS

Our ultimate goal for this section is to give a fairly rigorous analysis of a scanner incorporating a multihole focused collimator of the type illustrated in Fig. 1.19 (Barber, 1973; Beck, 1964a,b, 1968b). However, much insight can be gained by starting with a decidedly nonrigorous analysis of a scanner using a single-bore collimator.

4.4.1 Definition of PSF

In order to calculate the PSF of a scanner, we must first state just what we mean by PSF in this case. A rather obvious definition would take the PSF to be the instantaneous count rate of the detector, considered as a function of the position of a point source. There are two difficulties with this definition. The first is that the term "instantaneous count rate" must be understood in a statistical average sense. If the same measurement is repeated many times, or an ensemble of identical systems is considered, then the count rate of concern is $\Delta \bar{N}_c / \Delta t$, where $\Delta \bar{N}_c$ is the mean number of photons detected in a vanishingly small time interval Δt . Of course, in real life one does not have an ensemble of identical systems at his disposal, nor does he normally have the opportunity to repeat the measurement many times. A single measurement over a very small Δt would probably yield only zero or one detected photon and give practically no information about the mean rate. Some sort of averaging is clearly required.

In a practical scanner, this problem is solved by use of a count-rate meter which can take one of several forms. An idealized count-rate meter was discussed in Chapter 3, but a more practical form is the RC network shown in Fig. 4.15. The operation of this circuit will be discussed more fully in Section 4.4.7, but for now we simply note that it serves to average the count-rate over a time interval $R_1 C_1$ which is under the operator's control. It might seem that a large value of $R_1 C_1$ would be desirable since then the measured count rate would be an accurate estimate of the instantaneous rate defined above. However, we must not forget that the scanner is moving. A long averaging time will blur the point image in the direction of the scan. The count-rate meter is not just an optional accessory; it is an integral part of the scanner and makes its own contribution to the overall PSF. A full analysis of a scanner must, therefore, include a calculation of both the collimator and ratemeter contributions to the PSF. We shall accomplish both in due course (Beck, 1968a,b; Rao and Wagner, 1967; Mozley, 1968).

The second difficulty with defining the PSF as an instantaneous count rate is that it is dimensionally inconsistent with the definition of PSF used

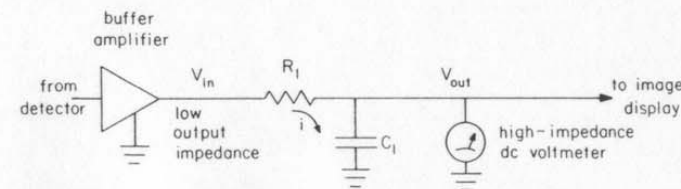


Fig. 4.15 Simple count-rate meter for use with a rectilinear scanner.

in the pinhole imaging discussion. In that case, we arranged for the detected photon density (i.e., the number detected per unit area) to be the emission function $f(\mathbf{r})$ convolved with the PSF. This required the PSF to have dimensions of time per unit area. Since the number of detected photons per unit area will be a key parameter when we come to a discussion of noise, it is highly desirable to standardize our definitions in such a way that this parameter is easy to calculate.

In a scanner, the conversion from counts (detected photons) per unit time to counts per unit area must involve two mechanical parameters, viz., the linear scan speed v_s and the number of scan lines per unit length (in the direction perpendicular to the rapid scan). The latter parameter will be denoted by n_l . Straightforward dimensional analysis then shows that the number of counts per unit area is the instantaneous count rate times n_l/v_s . (The scan lines are assumed to be contiguous and have width $1/n_l$, and v_s is assumed to be constant. Furthermore, no consideration is given to the behavior at the end of a raster line where the direction of scan is reversed.) We shall include this factor n_l/v_s in our definition of PSF for the scanner.

4.4.2 Geometrical Analysis of the PSF of a Single-Bore Collimator

Consider the geometry shown in Fig. 4.16 where a collimator of constant bore diameter D_b and bore length L_b is viewing a point source a distance z from the face of the collimator. In practice, the collimator will usually be scanned in a rectilinear raster over the source. For ease of analysis, however,

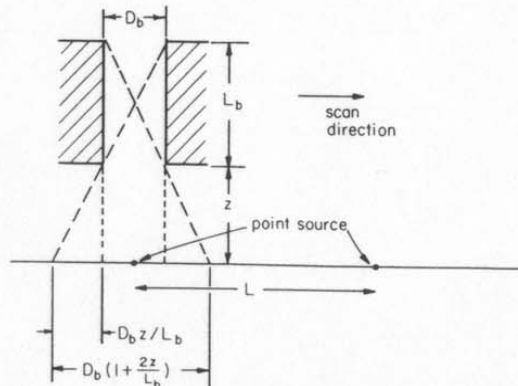


Fig. 4.16 Geometry for the calculation of the PSF of a single-bore collimator.

we assume that the collimator is stationary and the source is scanned; only relative motion is important, so this procedure is still quite general.

A great deal can be learned about the collimator PSF without elaborate calculations. To illustrate, consider first the case $z = 0$, where the source point is virtually in contact with the face of the collimator. Then, assuming there is no penetration of the gamma rays through the walls of the collimator, the count rate must be zero when the point source lies outside the disk region of diameter D_b directly in front of the bore. Furthermore, since L_b will normally be much larger than D_b , the collection solid angle will, to a good approximation, be independent of the location of the point within the disk region. (This approximation is nothing more than a restatement of the $\cos^3 \theta \approx 1$ condition that we have been using all along.) Finally, note that the scanner has a magnification of one since the count rate will be a maximum when the collimator is positioned directly over the point source. To image a second point source a lateral distance L away, the collimator must be moved by L . Of course, the final image can be *displayed* at any desired magnification, but this is of no concern since we shall always refer the PSF back to the scale of the object anyway. The main point here is that the magnification inherent in the gamma-ray collection system, in contrast to that obtained with a pinhole, is unity.

With these simple observations, we can now write down an expression for the PSF of the single-bore collimator:

$$p_{sb}(\mathbf{r}; z = 0) = p_{sb}(\mathbf{r}; z = 0) = \text{const} \cdot \text{circ}(2r/D_b). \quad (4.66)$$

The vector \mathbf{r} , of course, represents the two-dimensional position of the point in the plane $z = 0$; the collimator is assumed to be centered on $\mathbf{r} = 0$.

To fix the constant in (4.66), consider a point source emitting K photons per second. Its emission density function is $K \delta(\mathbf{r})$ and the instantaneous count rate within the disk region is $K\Omega/4\pi$, where Ω is the solid angle subtended by the detector. The PSF must thus satisfy

$$p_{sb}(\mathbf{r}; z = 0) ** K \delta(\mathbf{r}) = \frac{n_l}{v_s} \cdot \frac{K\Omega}{4\pi} \cdot \text{circ}\left(\frac{2r}{D_b}\right). \quad (4.67)$$

Since the solid angle in this case is $\pi D_b^2/4L_b^2$, the PSF is given by

$$p_{sb}(\mathbf{r}; z = 0) = \frac{n_l}{v_s} \cdot \frac{D_b^2}{16L_b^2} \cdot \text{circ}\left(\frac{2r}{D_b}\right). \quad (4.68)$$

Note that p_{sb} has dimensions of time per area, so that we can directly convolve p_{sb} with $f(\mathbf{r})$ to get the number of detected photons per unit area. It is not necessary to insert an exposure time T as we did in the pinhole camera and transmission radiography cases.

The general behavior of $p_{sb}(\mathbf{r}; z)$ for $z \neq 0$ is also easy to determine. We need to distinguish three regions in the source plane. The first, which we shall call the *umbra* by analogy with lunar eclipses, is the disk-shaped region of diameter D_b directly in line with the collimator bore. (The term "umbra" is a decided misnomer here since the detector is completely *unobscured* by the walls of the collimator in this region; we could call it an inverse umbra or negative umbra, but let's not be any more pedantic than necessary.) The PSF in the umbra region is approximately constant.

The second region to be discussed will be termed the *penumbra*. It is the region between the umbra and a circle of diameter $D_b[1 + (2z/L_b)]$ as shown in Fig. 4.16. In this region, part of the detector is obscured by the collimator, reducing the collection solid angle and hence the PSF. In the third region, outside the circle of diameter $D_b[1 + (2z/L_b)]$, all of the detector is obscured and the PSF is zero (again neglecting penetration of gamma rays through the collimator).

From these considerations, we can sketch the PSF for any z . In Fig. 4.17 we show the image of two well-resolved point sources. The sloping lines in the penumbra region have been drawn as straight, but the more careful analysis to be given below will show that they have a slight curvature. It should also be kept in mind that we have not yet discussed the effect of the count-rate meter. The image shown in Fig. 4.17 is that which would be obtained with an infinitesimally slow scan.

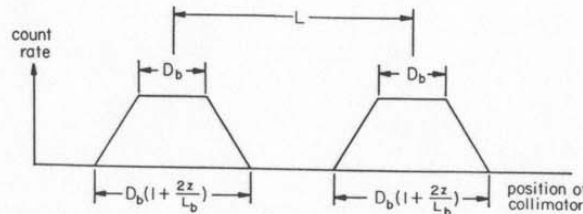


Fig. 4.17 Image of two points with a single-bore collimator.

4.4.3 Analytical Treatment of the Single-Bore Collimator

To complete the analysis of the single-bore collimator we must find an analytical expression for $p_{sb}(\mathbf{r}; z)$ for $z \neq 0$ and Fourier transform it to find the MTF. For this purpose, we again invoke the general model set up in Section 4.1. To show the correspondence between the model and the present problem, we note that the collimator can be replaced by a pair of thin

apertures as shown in Fig. 4.18. If the apertures are made of a hypothetical material that is absolutely opaque to gamma rays, then the aperture pair is equivalent* to the collimator. (The collimator material is also still being treated as impenetrable.)

With this equivalence, the problem closely resembles the pinhole camera problem. One important difference, however, arises because the pinhole aperture is used with an *imaging* detector that measures the coordinates of each gamma ray impinging on it. The scanner detector, on the other hand, is a spatially *integrating* detector that simply counts all gamma rays incident on it, irrespective of their coordinates. The only position dependence is imposed by the upper aperture in Fig. 4.18; a photon is counted only if it falls within the transparent area of that aperture.

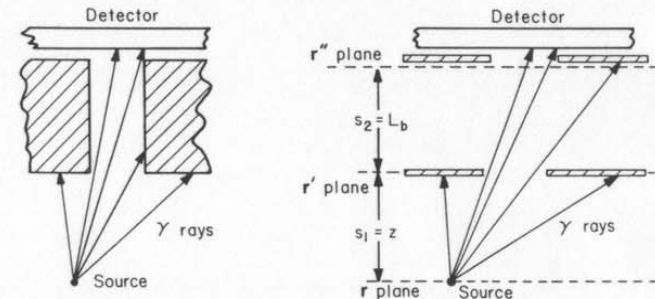


Fig. 4.18 Diagram showing the equivalence between a single-bore collimator and a pair of circular apertures. Left: actual collimator. Right: equivalent apertures.

We can apply the pinhole-camera equations to the single-bore collimator by taking the r'' plane to be just in front of the upper aperture as shown in Fig. 4.18. The function $h(r'')$ then specifies the photon density incident on the upper aperture. The lower aperture, whose transmission we shall designate $g_1(r')$, plays the role of the pinhole. The source-to-aperture spacing s_1 then corresponds to z , while the aperture-to-detector distance s_2 is L_b . The

* To be completely realistic, we should admit that there is one type of event for which the two geometries are not exactly equivalent. A gamma ray incident on the wall of the collimator can be either Compton scattered or photoelectrically absorbed. In either case a lower-energy photon is produced, and there is some small probability that it will escape from the wall and strike the detector. In practice, such events will usually be rejected by the pulse height analyzer.

In the equivalent aperture geometry, the collimator walls are not present, so a photon which would strike the wall instead strikes the underside of the upper aperture. The scattered x ray is then shielded from the detector and is not counted even without a pulse height analyzer.

function $h(\mathbf{r}'')$ is given by (4.13), which in the present notation becomes

$$h(\mathbf{r}'') = C \int_{\infty} f(\mathbf{r}) g_1(a\mathbf{r}'' + b\mathbf{r}) d^2r, \quad (4.69)$$

where

$$a = z/(L_b + z), \quad b = L_b/(L_b + z). \quad (4.70)$$

However $h(\mathbf{r}'')$ is the number of photons per unit area in an observation time T . For scanner problems we are often more interested in the number per unit area per unit time. Therefore we define a *flux density* or *fluence rate* by

$$\dot{h}(\mathbf{r}'') \equiv \frac{h(\mathbf{r}'')}{T} = \dot{C} \int_{\infty} f(\mathbf{r}) g_1(a\mathbf{r}'' + b\mathbf{r}) d^2r, \quad (4.71)$$

where

$$\dot{C} = C/T = [4\pi(L_b + z)^2]^{-1}. \quad (4.72)$$

Since the two apertures are identical and have diameter D_b , we may write

$$g_i(\mathbf{r}') = \text{circ}(2\mathbf{r}'/D_b), \quad i = 1 \text{ or } 2. \quad (4.73)$$

By retaining two separate subscripts, we may easily generalize the results later so that they apply to a collimator with a tapered bore.

The instantaneous count rate is found by multiplying the photon flux density incident on the upper aperture, $\dot{h}(\mathbf{r}'')$, by the transmission of that aperture, $g_2(\mathbf{r}'')$, and integrating over \mathbf{r}'' , i.e.,

$$\begin{aligned} \text{count rate} &= \int_{\infty} \dot{h}(\mathbf{r}'') g_2(\mathbf{r}'') d^2r'' \\ &= \dot{C} \int_{\infty} d^2r'' \int_{\infty} d^2r f(\mathbf{r}) g_1(a\mathbf{r}'' + b\mathbf{r}) g_2(\mathbf{r}''). \end{aligned} \quad (4.74)$$

We may take the domains of both integrations to be infinite planes since $f(\mathbf{r})$ and $g_2(\mathbf{r}'')$ are zero outside a finite region. To calculate the PSF, we let $f(\mathbf{r})$ be the point source $\delta(\mathbf{r} - \mathbf{r}_s)$. The integration over \mathbf{r} in (4.74) is now trivial, and we find for the PSF

$$\begin{aligned} p_{sb}(\mathbf{r}_s; z) &= \frac{n_i \dot{C}}{v_s} \int_{\infty} d^2r'' g_2(\mathbf{r}'') g_1(a\mathbf{r}'' + b\mathbf{r}_s) \\ &= \frac{n_i \dot{C}}{v_s} \int_{\infty} d^2r'' \text{circ}\left(\frac{2\mathbf{r}''}{D_b}\right) \text{circ}\left(\frac{2|a\mathbf{r}'' + b\mathbf{r}_s|}{D_b}\right) \\ &= \frac{n_i \dot{C}}{v_s} \int_{\infty} d^2r'' \text{circ}\left(\frac{2\mathbf{r}''}{D_b}\right) \text{circ}\left[\frac{2a|\mathbf{r}'' + (b\mathbf{r}_s/a)|}{D_b}\right]. \end{aligned} \quad (4.75)$$

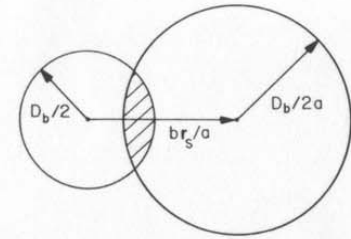


Fig. 4.19 Diagram to aid in interpreting Eq. (4.75).

The integrand in this equation is a product of a circ function of diameter D_b with a second circ function of diameter D_b/a as illustrated in Fig. 4.19; since the parameter a is less than one, the second circ function is larger than the first. The interpretation of this result is that the larger circ function represents the lower aperture as projected from the source point onto the upper aperture. The PSF is proportional to the area of overlap between the two circ functions, or the portion of the detector that can be seen from the source location.

Examine (4.75) in the limit $z \rightarrow 0$, or equivalently, $a \rightarrow 0$ and $b \rightarrow 1$. Then the first circ function is much smaller than the second and may be treated as a delta function:

$$\text{circ}\left(\frac{2\mathbf{r}''}{D_b}\right) \approx \frac{\pi D_b^2}{4} \delta(\mathbf{r}''), \quad (4.76)$$

where the constant $\pi D_b^2/4$ is necessary so that both sides of this equation will have the same integral over \mathbf{r}'' . This approximation allows us to perform the integral in (4.75) with the result

$$p_{sb}(\mathbf{r}_s; z = 0) = \left(\frac{n_i \dot{C}}{v_s}\right) \frac{\pi D_b^2}{4} \text{circ}\left(\frac{2\mathbf{r}_s}{D_b}\right), \quad (4.77)$$

which agrees with (4.68) since $\dot{C} = (4\pi L_b^2)^{-1}$ if $z = 0$.

At this point we can drop the subscript s denoting source point on \mathbf{r}_s and refer to the PSF as $p_{sb}(\mathbf{r}; z = 0)$. There are two justifications for this step. The first is that we can call the argument of a function whatever we please so long as we are consistent. But the more important reason is that we shall want to use $p_{sb}(\mathbf{r}, z = 0)$ in convolutions that are carried out in the \mathbf{r} plane. Recall that in the usual definition of the PSF for a shift-invariant imaging system, $p(\mathbf{r})$ represents the response at some image point due to the source point a vector distance \mathbf{r} away. In the above development, the image point was at the collimator location—the origin of coordinates—and the source point was at \mathbf{r}_s . The vector \mathbf{r}_s thus has the same meaning as the usual vector \mathbf{r} in $p(\mathbf{r})$.

The behavior of $p_{sb}(\mathbf{r}; z)$ for nonzero values of z is illustrated in Fig. 4.20. Note the curvature of the sloping edges in the penumbra region.

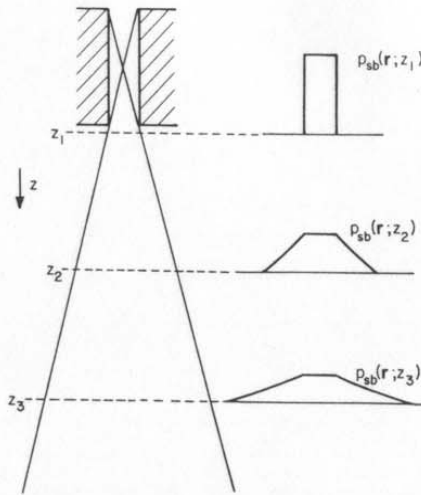


Fig. 4.20 PSF of a single-bore collimator for various values of z , the distance from the source plane to the collimator face.

4.4.4 Modulation Transfer Function

The MTF is proportional to the Fourier transform of (4.75). To perform this transform, it is convenient to first finagle the equation into the form of a convolution. The required manipulations are similar, but not identical, to those carried out in Section 4.1.4. As before, we define

$$\tilde{g}_1(\mathbf{r}'') = g_1(a\mathbf{r}'') \quad (4.78)$$

so that

$$g_1(a\mathbf{r}'' + b\mathbf{r}) = \tilde{g}_1[(b/a)\mathbf{r} + \mathbf{r}'']. \quad (4.79)$$

Equation (4.75) then becomes

$$P_{sb}(\mathbf{r}; z) = (n_l \dot{C}/v_s) [g_2(\mathbf{r}'') ** \tilde{g}_1(\mathbf{r}'')]_{\mathbf{r}'' = -b\mathbf{r}/a}. \quad (4.80)$$

The MTF appropriate to the plane z is now readily found by use of (B.52), (B.94), and (B.114). The result is

$$\text{MTF}_{sb} = \frac{|P_{sb}(\rho; z)|}{|P_{sb}(0; z)|} = \left| \frac{2J_1(\pi a D_b \rho / b)}{\pi a D_b \rho / b} \right| \cdot \left| \frac{2J_1(\pi D_b \rho / b)}{\pi D_b \rho / b} \right|. \quad (4.81)$$

The $z = 0$ limit is again of some interest. In that limit $a \rightarrow 0$ and $b \rightarrow 1$. Then, since

$$\lim_{X \rightarrow 0} [2J_1(X)/X] = 1, \quad (4.82)$$

we find

$$\lim_{z \rightarrow 0} \text{MTF}_{sb} = |2J_1(\pi D_b \rho) / \pi D_b \rho|. \quad (4.83)$$

This result could, of course, have been obtained directly by transforming (4.68). Note that it depends on only the bore diameter D_b and on no other geometrical parameter.

4.4.5 The Focused Collimator

Extension of our previous results to the case of a focused collimator (Fig. 4.21) is rather straightforward since each bore can be treated separately.

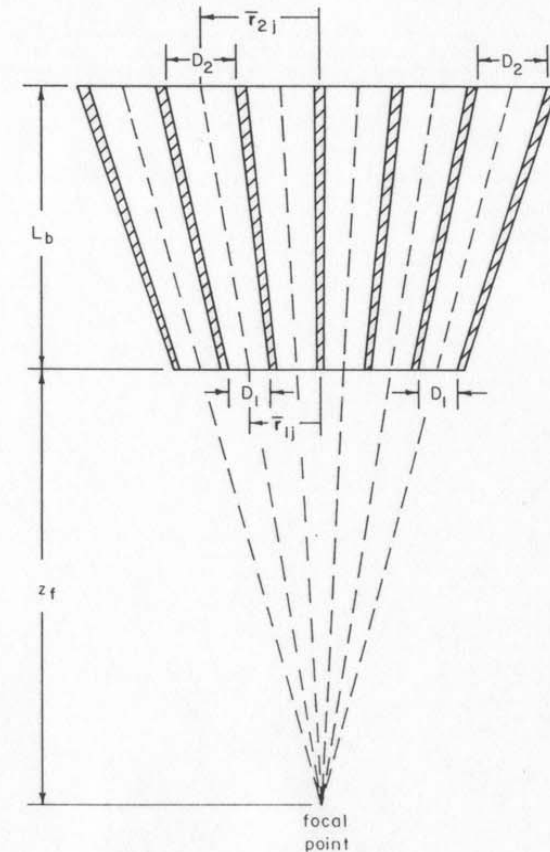


Fig. 4.21 Geometry of the focused collimator.

We need merely to generalize the single-bore results to allow for a nonconstant bore diameter and an overall tilt. As in the single-bore case, we can model each bore in a focused collimator by a pair of circular apertures. (In practice, the bores often have a hexagonal cross section, but little error occurs if we treat them as circular.) The lower aperture of the j th bore is described by

$$g_{1j}(\mathbf{r}') = \text{circ}(2|\mathbf{r}' - \bar{\mathbf{r}}_{1j}|/D_1), \quad (4.84)$$

while the upper aperture for the j th bore is given by

$$g_{2j}(\mathbf{r}'') = \text{circ}(2|\mathbf{r}'' - \bar{\mathbf{r}}_{2j}|/D_2). \quad (4.85)$$

Note that D_1 and D_2 are assumed to be the same for all bores.

If each bore is to point exactly to a common focal point at $z = z_f$ (a condition that is sometimes deliberately violated in practice), then we must have $\bar{\mathbf{r}}_{1j}$ parallel to $\bar{\mathbf{r}}_{2j}$, and their magnitudes must satisfy

$$\bar{r}_{2j}/\bar{r}_{1j} = (L_b + z_f)/z_f \quad \text{for all } j. \quad (4.86)$$

Usually the walls will also be tapered so that the aperture diameters are in the same proportions:

$$D_2/D_1 = (L_b + z_f)/z_f. \quad (4.87)$$

We can now write down a rather formidable expression for the PSF of the focused collimator by analogy with (4.75). The result is

$$p_{fc}(\mathbf{r}; z) = \frac{n_l \dot{C}}{v_s} \int_{-\infty}^{\infty} d^2 r'' \sum_{j=1}^{M_b} \text{circ}\left(\frac{2|\mathbf{r}'' - \bar{\mathbf{r}}_{2j}|}{D_2}\right) \text{circ}\left(\frac{2|a\mathbf{r}'' + b\mathbf{r} - \bar{\mathbf{r}}_{1j}|}{D_1}\right), \quad (4.88)$$

where a and b have the same meaning as before, and M_b is the number of bores in the collimator. The more masochistically inclined readers may proceed to Fourier-transform this equation and find the general expression for the MTF.

There is, however, one condition under which (4.88) can be considerably simplified, viz., $z = z_f$. This condition implies that the object being imaged lies entirely in the focal plane. Since we set up the problem so that all bore sights exactly overlap in the focal plane, we would expect the PSF in this case to be exactly proportional to the PSF of a single bore. To verify this conjecture, define

$$\mathbf{r}_j'' \equiv \mathbf{r}'' - \bar{\mathbf{r}}_{2j}. \quad (4.89)$$

Then, in the argument of the second circ function of (4.88), we have

$$\begin{aligned} a\mathbf{r}'' + b\mathbf{r} - \bar{\mathbf{r}}_{1j} &= a(\mathbf{r}_j'' + \bar{\mathbf{r}}_{2j}) + b\mathbf{r} - \bar{\mathbf{r}}_{1j} \\ &= a\mathbf{r}_j'' + b\mathbf{r}, \end{aligned} \quad (4.90)$$

where the last step follows from (4.86) and the fact that $a = z_f/(L_b + z_f)$ if $z = z_f$. Equation (4.88) now reads

$$p_{fc}(\mathbf{r}; z_f) = \frac{n_l \dot{C}}{v_s} \sum_{j=1}^{M_b} \int_{-\infty}^{\infty} d^2 r_j'' \text{circ}\left(\frac{2r_j''}{D_2}\right) \text{circ}\left(\frac{2|a\mathbf{r}_j'' + b\mathbf{r}|}{D_1}\right). \quad (4.91)$$

But each term in the sum is independent* of j and identical with the single-bore PSF given by (4.75) (except for the minor generalization of differing aperture diameters, $D_1 \neq D_2$). We have therefore shown, not surprisingly, that

$$p_{fc}(\mathbf{r}; z_f) = M_b p_{sb}(\mathbf{r}; z_f). \quad (4.92)$$

It should be noted that $p_{fc}(\mathbf{r}; z_f)$ exhibits no umbra region. By use of (4.87), (4.91) is seen to represent the autocorrelation of a circ function rather than the cross correlation of two different circ functions.

4.4.6 Sensitivity and Resolution

An oft-used measure of sensitivity for a scanner is the planar sensitivity S . This parameter is defined as the count rate obtained when the scanner is viewing a uniform planar source of activity $1.0 \mu\text{Ci}/\text{cm}^2$. (See Appendix D for a discussion of radiation units.) In our notation, such a source is described by $f(\mathbf{r}) = \text{const}$. The value of the constant is fixed if we assume that each nuclear disintegration produces exactly one emitted gamma ray with an energy suitable for detection by the scanner. Then, since $1.0 \mu\text{Ci}$ corresponds to 3.7×10^4 disintegrations/sec, we have

$$f(\mathbf{r}) = 3.7 \times 10^4 \text{ emitted photons}/\text{cm}^2 \text{ sec}, \quad (4.93)$$

Different isotopes will give different values for the numerical constant in this equation since, in general, the number of usable gamma rays per disintegration will be different from one.

The count rate is given in terms of the PSF by

$$\text{count rate} = (v_s/n_l) p_c(\mathbf{r}; z) ** f(\mathbf{r}), \quad (4.94)$$

where $p_c(\mathbf{r}; z)$ can refer to either $p_{sb}(\mathbf{r}; z)$ or $p_{fc}(\mathbf{r}; z)$. We shall consider the single-bore case first.

Since $f(\mathbf{r})$ is a constant, the convolution in (4.94) becomes a simple integral over the PSF. The planar sensitivity is then given by

$$S_{sb} = \frac{v_s}{n_l} (3.7 \times 10^4) \cdot \int_{-\infty}^{\infty} p_{sb}(\mathbf{r}; z) d^2 r \quad (4.95)$$

* The fact that \mathbf{r}_j'' depends on $\bar{\mathbf{r}}_{2j}$ is of no concern since \mathbf{r}_j'' is a dummy variable of integration, and the integration is over the entire $\mathbf{r}_j'' = \text{plane}$.

or, from (4.75) and (4.72),

$$S_{sb} = \frac{3.7 \times 10^4}{4\pi(L_b + z)^2} \int_{-\infty}^{\infty} d^2r'' \int_{-\infty}^{\infty} d^2r \text{circ}\left(\frac{2r''}{D_b}\right) \text{circ}\left(\frac{2|ar'' + br|}{D_b}\right). \quad (4.96)$$

where now L_b and z must be expressed in centimeters.

The integral over \mathbf{r} in (4.96), which involves only the second circ function, is easily performed, with the result

$$\begin{aligned} S_{sb} &= \frac{3.7 \times 10^4}{4\pi(L_b + z)^2} \frac{\pi D_b^2}{4b^2} \int_{-\infty}^{\infty} d^2r'' \text{circ}\left(\frac{2r''}{D_b}\right) \\ &= \frac{3.7 \times 10^4}{4\pi(L_b + z)^2} \frac{\pi D_b^2}{4b^2} \frac{\pi D_b^2}{4}. \end{aligned} \quad (4.97)$$

With the aid of the definition of b , (4.70), S_{sb} reduces further to

$$S_{sb} = \frac{3.7 \times 10^4}{64} \frac{\pi D_b^4}{L_b^2} \frac{\text{counts/sec}}{\mu\text{Ci/cm}^2} \quad (4.98)$$

(all dimensions in centimeters). Note that this result is independent of z and the scan parameters v_s and n_1 . It does not matter how far you are from a uniform source or how fast you are moving past it.

It is a simple matter to modify the preceding derivation so that it applies to a focused collimator. The result is

$$S_{fc} = \frac{3.7 \times 10^4}{64} M_b \frac{\pi D_1^2 D_2^2}{L_b^2} \frac{\text{counts/sec}}{\mu\text{Ci/cm}^2} \quad (4.99)$$

(all dimensions in centimeters).

To put these expressions for sensitivity into proper perspective, it is useful to restate them in terms of the collimator's resolution distance defined, as usual, as the FWHM of the PSF. For the single-bore collimator, the resolution distance $\delta_{sb}(z)$ can be estimated from the approximate sketches given in Fig. 4.17, where the curvature of the PSF in the penumbra region is neglected. We find

$$\delta_{sb}(z) \approx D_b(1 + z/L_b). \quad (4.100)$$

Of course, if $z \rightarrow 0$, δ_{sb} will equal D_b without approximation.

If we regard D_b as the variable parameter and hold z and L_b fixed, we have

$$S_{sb} \propto \delta_{sb}^4. \quad (4.101)$$

Thus a twofold improvement in resolution (reduction in δ_{sb}) must come at the expense of a sixteenfold decrease in sensitivity. And even this drastic behavior understates the problem when noise is considered. Let us anti-

cipate a simple result from Chapter 10, where it is shown that the signal-to-noise ratio (SNR) in a scanner image is determined by the number of detected photons *per resolution element*, which we shall denote by N_δ . For a given source, we have

$$N_\delta \propto S_{sb} \cdot \delta_{sb}^2 \propto \delta_{sb}^6. \quad (4.102)$$

To keep the SNR constant when δ_{sb} is reduced by a factor of 2, therefore, means that either the source activity or the total scan time must be increased by a factor of 64.

A somewhat different result applies to a focused collimator. In the focal plane the PSF, as noted previously, is proportional to the autocorrelation of a circ function. Numerical evaluation of this autocorrelation (Gaskill, 1978, p. 304) shows that the resolution distance is given by

$$\delta_{fc} = 0.808 D_1(1 + z_f/L_b). \quad (4.103)$$

(The factor of 0.808 would become unity if we neglected the curvature of the PSF.) Furthermore, since the ratio D_1/D_2 is fixed by (4.87), we have

$$S_{fc} \propto M_b D_1^4 \propto M_b \delta_{fc}^4, \quad (4.104)$$

for fixed z_f and L_b .

The major difference from the single-bore case arises when we realize that M_b itself is a function of D_1 or δ_{fc} . The reason is that the total diameter of the detector crystal is usually fixed. Therefore, if each bore is made smaller, more bores can be fit into the detector area. Specifically, we have

$$M_b = \alpha_{pf}(D_{det}/D_2)^2, \quad (4.105)$$

where D_{det} is the diameter of the detector and α_{pf} is the packing fraction, i.e., the fraction of the total area of the crystal that is covered by the open part of the collimator. If all bores point to a common focal point, α_{pf} is also the fraction of the detector area that can be seen from the focal point. For a given minimum septal thickness, α_{pf} will be the largest for a hexagonal array of bores. Typically, α_{pf} lies between 0.5 and 0.8, depending on septal thickness and hence on photon energy.

From (4.87), (4.103), and (4.105), we now have

$$M_b \propto \delta_{fc}^{-2} \quad (4.106)$$

where D_{det} , L_b , z_f , and α_{pf} are regarded as fixed. The number of counts per resolution element, in this case, is given by

$$N_\delta \propto S_{fc} \delta_{fc}^2 \propto \delta_{fc}^4. \quad (4.107)$$

In other words, a constant SNR can be maintained when halving δ_{fc} by "merely" increasing the source activity or the scan time a factor of 16. The

situation is still drastic, but at least it is an improvement over the single-bore case.

The fourth-power law given in (4.107) is quite common in radiographic imaging. For example, the reader may wish to test his understanding of the arguments in this section by showing that (4.107) applies also to pinhole imaging.

4.4.7 The Ratemeter

In this section we consider the contribution of the count-rate meter to the overall PSF of a scanner (Rao and Wagner, 1967; Beck, 1968a). One can imagine a scanner with very fine collimator bores so that the collimator PSF is vanishingly narrow. (Never mind that the photon collection efficiency is also vanishingly small—statistical considerations are not our concern at this stage. Since this is a gedankenexperiment, the source can be infinitely intense.) When this hypothetical collimator is raster-scanned over a point source, photons can be detected only when the collimator is positioned directly over the point. However, this is not to say that the image will be an ideal point. Instead the ratemeter will have a nonzero output, and hence the displayed image will be nonzero for some time after the collimator has passed the true location of the point. In fact, the PSF in the scan direction is just the temporal impulse response of the ratemeter with appropriate scale factors. When the collimator is directly over the source, a brief burst of photons is admitted to the detector which produces an equally brief electrical signal, approximating an impulse, as the input to the ratemeter. The electrical signal emerging from the ratemeter is then, by definition, its impulse response. Of course, this impulse response would normally be calculated as a function of time, but we can easily convert it to a function of position if we know the scan speed.

A corollary result is that the ratemeter cannot degrade the image at all in the direction perpendicular to the scan motion. To see this, note that if our hypothetical collimator is displaced slightly so that the scan line does not intersect the source point, no photons are ever admitted to the detector and no input signal is ever applied to the ratemeter. Hence, its output also remains zero.

To restate the conclusions of the last two paragraphs more formally, suppose that the scanner is moving in the x direction at a uniform speed v_s . Then the ratemeter contribution to the PSF is given by

$$p_{rm}(\mathbf{r}) = (1/v_s) \delta(y) q_{rm}(x/v_s), \quad (4.108)$$

where $q_{rm}(t)$ is the temporal impulse response of the ratemeter regarded as an electrical filter. The leading factor of $1/v_s$ in (4.108) is required so that

$p_{rm}(\mathbf{r})$ will have dimensions of inverse area. The temporal impulse response $q_{rm}(t)$ has dimensions of inverse time so that $(1/v_s)q(x/v_s)$ has dimensions of inverse length. Of course, $\delta(y)$ also has dimensions of inverse length. With this definition, $f(\mathbf{r}) ** p_{tc}(\mathbf{r}) ** p_{rm}(\mathbf{r})$ represents the number of detected photons per unit area [with $f(\mathbf{r})$, as usual, being the number of emitted photons per unit area per unit time].

As an example, we shall now calculate the PSF for the RC ratemeter depicted in Fig. 4.15. For simplicity, we assume that the output impedance of the amplifier driving the RC network is zero, while the input impedance of the following amplifier is infinite. The same current $i(t)$ thus flows through R_1 and C_1 . From elementary circuit theory we then have

$$i(t) = C_1 \frac{dv_{out}(t)}{dt} \quad (4.109)$$

and

$$v_{in}(t) = i(t)R_1 + v_{out}(t). \quad (4.110)$$

Combining these equations, we find

$$R_1 C_1 \frac{dv_{out}}{dt} + v_{out} = v_{in}. \quad (4.111)$$

The left-hand side of this equation may be rewritten, with the aid of the usual integrating factor,

$$R_1 C_1 \exp\left(\frac{-t}{R_1 C_1}\right) \frac{d}{dt} \left[v_{out} \exp\left(\frac{t}{R_1 C_1}\right) \right] = v_{in}, \quad (4.112)$$

from which an integration and a little algebra yield

$$v_{out}(t) = \frac{1}{R_1 C_1} \exp\left(\frac{-t}{R_1 C_1}\right) \int_{-\infty}^t v_{in}(t') \exp\left(\frac{t'}{R_1 C_1}\right) dt'. \quad (4.113)$$

Now what we are really interested in is not this general result so much as the special case where $v_{in}(t')$ is the unit impulse $\delta(t')$ and $v_{out}(t)$ is the impulse response $q_{rm}(t)$. The integration is then essentially trivial, but we must not forget that an integral involving a delta function can be nonzero only if the argument of the delta function vanishes within the domain of integration. We thus have

$$\begin{aligned} q_{rm}(t) &= \frac{1}{R_1 C_1} \exp\left(\frac{-t}{R_1 C_1}\right) \int_{-\infty}^t \delta(t') \exp\left(\frac{t'}{R_1 C_1}\right) dt' \\ &= \begin{cases} (1/R_1 C_1) \exp(-t/R_1 C_1) & \text{if } t > 0 \\ 0 & \text{if } t < 0. \end{cases} \end{aligned} \quad (4.114)$$

The result that $q_{rm}(t) = 0$ if $t < 0$ should come as no surprise; it simply says that no output can be produced from an electrical filter before an input is applied. In this case the input is an impulse at $t = 0$.

The product $R_1 C_1$ has dimensions of time and is called the *time constant* of the filter. Basically, the counts are averaged over this time before being displayed.

A compact notation for use in (4.114) is the Heaviside unit step function, defined by

$$\text{step}(t) = \begin{cases} 1 & \text{if } t > 0 \\ 0 & \text{if } t < 0. \end{cases} \quad (4.115)$$

In terms of this function, (4.114) becomes

$$q_{rm}(t) = \frac{1}{R_1 C_1} \exp\left(\frac{-t}{R_1 C_1}\right) \text{step}(t) \quad (4.116)$$

and, with (4.108), our final result for the ratemeter PSF is

$$p_{rm}(\mathbf{r}) = \frac{1}{v_s R_1 C_1} \exp\left(\frac{-x}{v_s R_1 C_1}\right) \delta(y) \text{step}(x). \quad (4.117)$$

The FWHM of this function is $v_s R_1 C_1 \ln 2$ in the x direction and, of course, zero in the y direction. It is plotted in Fig. 4.22.

To complete the analysis, we should now calculate the ratemeter contribution to the scanner transfer function. This can be accomplished either by directly transforming (4.117) or by returning to the circuit model and expressing the voltage transfer ratio in the temporal frequency (v) domain. The latter approach yields

$$\frac{V_{out}(v)}{V_{in}(v)} = \frac{(2\pi i v C_1)^{-1}}{R_1 + (2\pi i v C_1)^{-1}} = \frac{1}{1 + 2\pi i v R_1 C_1}, \quad (4.118)$$

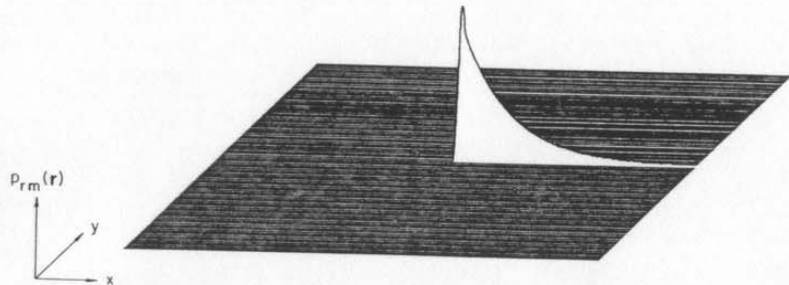


Fig. 4.22 Isometric plot of the ratemeter contribution to the scanner PSF.

where $V_{out}(v)$ and $V_{in}(v)$ are the temporal Fourier transforms of $v_{out}(t)$ and $v_{in}(t)$, respectively, and $i = \sqrt{-1}$ [not to be confused with the current $i(t)$]. The temporal frequency v is related to ξ , the x component of the spatial frequency, by

$$v = \xi v_s. \quad (4.119)$$

The spatial transfer function is thus

$$TF_{rm}(\rho) = P_{rm}(\rho) = [1 + 2\pi i \xi v_s R_1 C_1]^{-1}. \quad (4.120)$$

Note that this function is independent of η , the y component of ρ , since the ratemeter cannot degrade the image in the y direction.

Equation (4.120) is interesting because $P_{rm}(\rho)$ is a complex function. To interpret this result, it is helpful to rewrite it in modulus-phase form:

$$P_{rm}(\rho) = [1 + (2\pi \xi v_s R_1 C_1)^2]^{-1/2} \exp(i\phi_{rm}), \quad (4.121)$$

where

$$\phi_{rm} = -\tan^{-1}(2\pi \xi v_s R_1 C_1). \quad (4.122)$$

In other words, if a sinusoidal activity pattern with spatial frequency ξ were to be scanned with our hypothetical ideal collimator and with a ratemeter time constant of $R_1 C_1$, the contrast of the displayed image would be reduced by a factor of $[1 + (2\pi \xi v_s R_1 C_1)^2]^{-1/2}$ and the phase of the pattern would be shifted by ϕ_{rm} . The MTF, $|P_{rm}(\rho)/P_{rm}(0)|$, is plotted in Fig. 4.23.

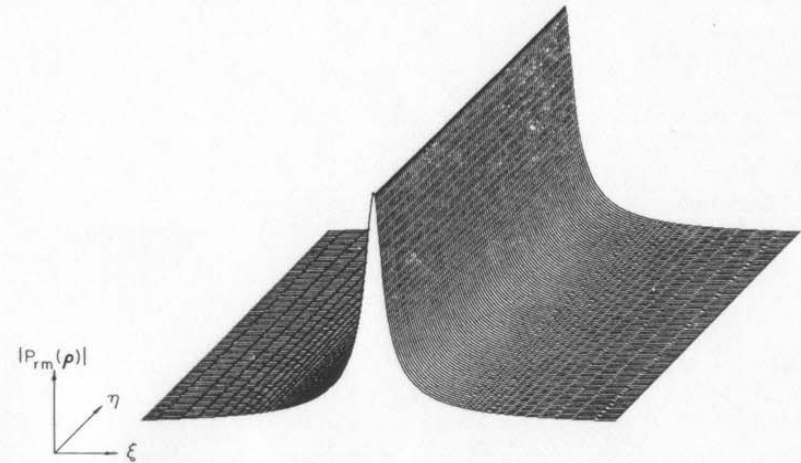


Fig. 4.23 Isometric plot of the ratemeter contribution to the scanner MTF. The origin ($\xi = 0, \eta = 0$) is at the center of the figure.

4.4.8 Image Display and Overall System Characterization

The most common way to display the image from a scintillation scanner is to use a modulated light source moving in synchronism with the scanner head to expose a piece of film. If the light intensity is modulated in proportion to the output of the ratemeter, then the film exposure is a linear function of the gamma-ray activity in the source, and the techniques of linear systems theory may be used to describe the film-exposing device. Of course, the film itself responds nonlinearly to the exposure, but this creates no real difficulty since the film characteristics are presumably known. The optical density of the developed film is thus easily calculated from the exposure, which in turn is calculated by successively convolving the gamma-ray source distribution $f(\mathbf{r})$ with the PSF's describing the collimator, the ratemeter, and the display.

There is one subtlety in this prescription. A convolution integral cannot be a rigorous description of the action of a scanner since the scanner detector does not systematically explore all possible points on the x - y plane as implied by a continuous integral. Rather the detector is usually swept continuously in the x direction but moved in discrete steps in the y direction. However the film exposure, which we shall call $E(x, y)$, is defined over the entire film plane (although it may be zero for some x - y values). The display spread function evidently enters our formalism somewhat differently than the collimator and ratemeter PSFs.

To pursue this point, let us lump the collimator and ratemeter PSFs into a single function $p_{\text{crm}}(\mathbf{r})$ defined by

$$p_{\text{crm}}(\mathbf{r}) = p_c(\mathbf{r}) ** p_{\text{rm}}(\mathbf{r}), \quad (4.123)$$

where $p_c(\mathbf{r})$ may be either $p_{\text{fc}}(\mathbf{r})$ or $p_{\text{sb}}(\mathbf{r})$ as appropriate. We adopt the viewpoint that the scanner head is stationary and the source moves continuously along a sequence of lines described by $y = y_k$, with k being an integer index. The interval between scan lines is n_l^{-1} where n_l , as previously defined, is the number of scan lines per unit length. The voltage output from the ratemeter, when the instantaneous shift of the source relative to the detector is (x_0, y_k) , is given by an ordinary convolution:

$$v_{\text{out}}(x_0, y_k) \propto \int_{-\infty}^{\infty} \int_{-\infty}^{\infty} dx' dy' p_{\text{crm}}(x', y') f(x_0 - x', y_k - y'). \quad (4.124)$$

Let us suppose that the light source illuminates a square aperture of side ε_a that is imaged at unit magnification onto the film. (Note that if $\varepsilon_a = n_l^{-1}$, the exposed scan lines will be contiguous.) Then, for the particular

relative shift (x_0, y_k) , the film exposure pattern is described by

$$E_{x_0 y_k}(x, y) \propto v_{\text{out}}(x_0, y_k) \text{rect}\left(\frac{x - x_0}{\varepsilon_a}\right) \text{rect}\left(\frac{y - y_k}{\varepsilon_a}\right). \quad (4.125)$$

The total film exposure $E(x, y)$ is obtained by summing (4.125) over all possible source-detector shifts; the sum becomes an integral over the continuous variable x_0 but remains a discrete sum over y_k . The result is

$$E(x, y) \propto \sum_k \int_{-\infty}^{\infty} dx_0 \text{rect}\left(\frac{x - x_0}{\varepsilon_a}\right) \text{rect}\left(\frac{y - y_k}{\varepsilon_a}\right) \cdot \int_{-\infty}^{\infty} \int_{-\infty}^{\infty} dx' dy' p_{\text{crm}}(x', y') f(x_0 - x', y_k - y'). \quad (4.126)$$

This equation looks very much like a repeated convolution except that *one* of the integrals has been replaced by a sum. But this is a nontrivial change. To see that (4.126) is not even approximately a continuous convolution, one has only to consider the limit $\varepsilon_a \rightarrow 0$. Then the film is exposed only along thin lines and is unexposed between lines. This is, of course, a very poor display format but, more important for the present discussion, it is one that cannot be obtained by convolving $f(x, y)$ with any realistic function. Instead, the proper description of (4.126) follows the lines of the sampling theory discussion given in Section 2.5; the scanner *samples* the image in the y direction.

It was shown in Section 2.5 that a band-limited function can be recovered from its samples by a low-pass filtering operation if the Nyquist condition, (2.82), is satisfied. For the present problem the function being sampled is $p_{\text{crm}}(\mathbf{r}) ** f(\mathbf{r})$, and the sampling rate $1/\Delta$ is just n_l . Let us assume that the collimator MTF is essentially zero for all y -directed spatial frequencies greater than η_{max} . (The ratemeter MTF does not enter this discussion since it influences only the x -directed spatial frequencies.) Then the Nyquist condition is $n_l > 2\eta_{\text{max}}$. No assumptions about $f(\mathbf{r})$ are needed.

The required low-pass filter may be an implicit rather than explicit part of the system. A physician viewing a scanner image will often unconsciously adjust his viewing distance so that his eye cannot resolve the scan lines. Or, even if he can see them, he has learned to ignore the scan lines and concentrate on the underlying image structure. The low-pass filter is thus the observer's eye or brain.

In any event, if n_l is large enough, it is safe to say that we are interested in only the low-frequency components of $E(x, y)$, which we shall denote by $E_{\text{lf}}(x, y)$. The derivation of $E_{\text{lf}}(x, y)$ parallels the derivation of (2.87). As far

as the y dependence is concerned, (4.126) has the form [cf. (2.69)]

$$\begin{aligned} E(x, y) &\propto \sum_k s(y_k) \text{rect}\left(\frac{y - y_k}{\varepsilon_a}\right) \\ &= \left[\sum_k s(y_k) \delta(y - y_k) \right] * \text{rect}\left(\frac{y}{\varepsilon_a}\right) \\ &= \left[s(y) \sum_k \delta(y - y_k) \right] * \text{rect}\left(\frac{y}{\varepsilon_a}\right), \end{aligned} \quad (4.127)$$

where

$$\begin{aligned} s(y_k) &\equiv \int_{-\infty}^{\infty} dx_0 \text{rect}\left(\frac{x - x_0}{\varepsilon_a}\right) \\ &\quad \times \int_{-\infty}^{\infty} \int_{-\infty}^{\infty} p_{\text{crm}}(x', y') f(x_0 - x', y_k - y') dx' dy'. \end{aligned} \quad (4.128)$$

Since the y_k values are evenly spaced, we can write $y_k = k/n_l$ and hence

$$\begin{aligned} \sum_k \delta(y - y_k) &= \sum_k \delta\left[y - \left(\frac{k}{n_l}\right)\right] \\ &= n_l \sum_k \delta(n_l y - k) = n_l \text{comb}(n_l y). \end{aligned} \quad (4.129)$$

A one-dimensional Fourier transform on $E(x, y)$ then yields

$$\begin{aligned} \mathcal{F}_y\{E(x, y)\} &\propto [S(\eta) * \text{comb}(\eta/n_l)] \text{sinc}(\varepsilon_a \eta) \\ &= \left[n_l \sum_k S(\eta - kn_l) \right] \text{sinc}(\varepsilon_a \eta). \end{aligned} \quad (4.130)$$

The low-pass filter serves to select the $k = 0$ term in this sum and reject all others. An inverse transform then gives

$$E_{\text{lf}}(x, y) \propto s(y) * \text{rect}(y/\varepsilon_a). \quad (4.131)$$

Combining (4.131) and (4.128) and rewriting them in convolution form, we now have

$$E_{\text{lf}}(x, y) \propto \left[\text{rect}\left(\frac{x}{\varepsilon_a}\right) \text{rect}\left(\frac{y}{\varepsilon_a}\right) \right] ** p_{\text{crm}}(x, y) ** f(x, y), \quad (4.132)$$

which we might have written down intuitively at the outset. In other words, if we consider only the low-frequency components, it is rigorously correct to ascribe a PSF to the film-exposing device even though (4.126) could not be written in convolution form.

Furthermore, the display PSF need not be simply the square aperture considered thus far. It can readily be modified to any positive-definite

function simply by inserting appropriate transparencies in the optical system. The film exposure system is thus a convenient place to control the overall PSF of a scanner (Tsui *et al.*, 1980). Of course, only smoothing and not sharpening operations are possible in the display since we are restricted to positive-definite PSFs. Still, it might be preferable to smooth the data with the display rather than with the ratemeter since the former provides a two-dimensional averaging, while the latter affects only the scan direction.

4.5 COLLIMATORS FOR SCINTILLATION CAMERAS

Fundamentally, collimators for use with scintillation cameras are no different from those used with scanners (Causier, 1974; Rotenberg and Johns, 1965; Miracle *et al.*, 1979). The typical parallel-hole camera collimator can be viewed either as an array of identical single-bore collimators as described in Sections 4.4.2 and 4.4.3, or equivalently as the focused collimator of Section 4.4.5 in the limit where the focal distance z_f approaches infinity. A magnifying camera collimator is nothing but a focused scanner collimator with z_f much greater than the actual object distance z (although in practice the camera collimator will have many more holes). Similarly, a minifying camera collimator is a focused scanner collimator where z_f is large and negative.

Nevertheless, the present section is not superfluous; we cannot simply rewrite the expression for the PSF of a scanner collimator and claim to have solved the corresponding problem for a camera. Nontrivial differences arise because a camera measures the x - y coordinates of each gamma ray that interacts with the scintillation crystal, while a scanner simply counts them.

In one sense the camera case is simpler because one less integration is involved. For the scanner we had to first calculate the x - y distribution of incident photons on the crystal face and then integrate it to get the total count rate. By simply deleting the last integration we should have the desired x - y distribution for a camera. This is indeed correct, but unfortunately, not very useful, because the PSF so determined is not shift-invariant. As illustrated in Fig. 4.24, the shape of the image of a point depends on the location of the point relative to the collimator. This is a serious problem because it means that the response to an arbitrary input cannot be written as a convolution, and a simple transfer function cannot be defined.

An ingenious artifice to avoid this difficulty, introduced by Hal Anger, is the "average PSF" obtained by averaging a point-source image over all possible source locations. This approach is detailed in Section 4.5.1 and given a more rigorous justification based on sampling theory in Section 4.5.2.

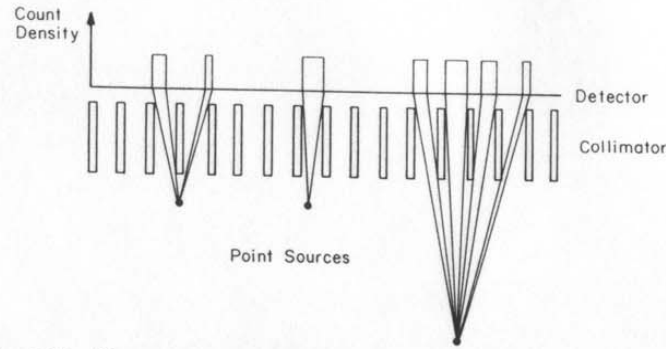


Fig. 4.24 Illustration of shift-variant imaging with a parallel-hole collimator.

The upshot of this discussion is that a shift-invariant PSF can indeed be defined and we can proceed in an orderly way to calculate the transfer function and to consider practical design tradeoffs.

4.5.1 The Average PSF

A problem that sometimes arises when a high-energy low-resolution collimator (one with large bores and thick septa) is used is that the shadows of the septa can be seen on the final image. Since this regular geometrical pattern can be annoying and may interfere with the diagnostic process, Wilks *et al.* (1969) constructed a device called a “collywobbler” to wobble the collimator back and forth during the exposure, blurring out the septal shadows. Since there was no relative movement of the object and the detector, the collywobbler did not substantially affect the image resolution.

The collywobbler was a mechanical realization of an earlier suggestion by Anger (1964) who calculated the PSF of a collimator by assuming that it was moving even if, in fact, it was not. Since moving the collimator alone is equivalent to moving the source and detector in synchronism while keeping the collimator fixed, Anger’s “mathematical collywobbler” calculation gave the average shape of the PSF, averaged over all possible locations of the source point. Thus, even though the Wilks collywobbler is not often used in practice, it is nevertheless a useful conceptual device.

The substance of the Anger calculation can be seen by modeling each bore of a parallel-hole collimator as a pair of circular apertures, just as we did in Section 4.4.3. For simplicity we assume for now that the image detector is exactly coplanar with the upper aperture; this restriction will be lifted in Section 4.5.3. We consider a unit point source located at the point \mathbf{r}_s and denote the resulting point spread function by $p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s)$. Two separate arguments \mathbf{r}'' and \mathbf{r}_s are required since the function is not shift invariant;

location in both the image plane and the source plane must be specified. In general, $p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s)$ will also depend on the z coordinate of the source point, but this dependence has been suppressed here in order to keep the notation from becoming any more unwieldy.

The function $p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s)$ can be obtained from $p_{\text{sb}}(\mathbf{r}_s; z)$ as given by (4.75) by four simple modifications:

- (1) The integration over \mathbf{r}'' must be deleted since we are dealing with an imaging rather than an integrating detector.
- (2) The factor of n_i/v_s , peculiar to the scanner, must be deleted and the exposure time T must be reinserted.
- (3) Each circ function must be displaced by an amount $\bar{\mathbf{r}}_k$, where the k th bore in the collimator is centered at $\mathbf{r} = \bar{\mathbf{r}}_k$.
- (4) A sum over all bores must be performed.

The result is

$$p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s) = C \sum_k \text{circ} \left[\frac{2|\mathbf{r}'' - \bar{\mathbf{r}}_k|}{D_b} \right] \text{circ} \left[\frac{2|a\mathbf{r}'' + b\mathbf{r}_s - \bar{\mathbf{r}}_k|}{D_b} \right], \quad (4.133)$$

where a and b still have the meanings given by (4.70).

We now want to average this expression over all possible positions of the collimator, with the source point \mathbf{r}_s and the observation point \mathbf{r}'' held fixed. To shift the collimator, we simply add a vector \mathbf{R} to each $\bar{\mathbf{r}}_k$ in (4.133). The average PSF, averaged over a disk of radius R_m , is then given by

$$\begin{aligned} \langle p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s) \rangle_{R_m} &= \frac{C}{\pi R_m^2} \int_{\text{disc}} d^2 R \sum_k \text{circ} \left[\frac{2|\mathbf{r}'' - \bar{\mathbf{r}}_k - \mathbf{R}|}{D_b} \right] \\ &\quad \times \text{circ} \left[\frac{2|a\mathbf{r}'' + b\mathbf{r}_s - \bar{\mathbf{r}}_k - \mathbf{R}|}{D_b} \right]. \end{aligned} \quad (4.134)$$

Now if we ignore the collimator boundaries and allow R_m to approach infinity, each term in the sum over k gives the same value for the integral. The number of such terms, i.e., the number of bores in the area πR_m^2 , is given by

$$K = \alpha_{\text{pf}} (2R_m/D_b)^2, \quad (4.135)$$

where α_{pf} is the packing fraction defined just as in the scanner case. Then, since $K/\pi R_m^2 = 4\alpha_{\text{pf}}/\pi D_b^2$, we have

$$\begin{aligned} \langle p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s) \rangle_{R_m} &= \frac{4\alpha_{\text{pf}}}{\pi D_b^2} C \int_{\infty} d^2 R \text{circ} \left[\frac{2|\mathbf{r}'' - \mathbf{R}|}{D_b} \right] \\ &\quad \times \text{circ} \left[\frac{2|a\mathbf{r}'' + b\mathbf{r}_s - \mathbf{R}|}{D_b} \right]. \end{aligned} \quad (4.136)$$

Note that R_m no longer appears in this result.

Equation (4.136) can be simplified somewhat by a change of variables,

$$\mathbf{R}' = \mathbf{R} - \mathbf{r}'', \quad (4.137)$$

which gives

$$\begin{aligned} \langle p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s) \rangle_{R_m} &= \frac{4\alpha_{\text{pf}}}{\pi D_b^2} C \int_{-\infty}^{\infty} d^2 R' \text{circ} \left[\frac{2R'}{D_b} \right] \\ &\times \text{circ} \left[\frac{2|(a-1)\mathbf{r}'' + b\mathbf{r}_s - \mathbf{R}'|}{D_b} \right]. \end{aligned} \quad (4.138)$$

But, from (4.70), $a + b = 1$, so that

$$(a-1)\mathbf{r}'' + b\mathbf{r}_s = b(\mathbf{r}_s - \mathbf{r}''). \quad (4.139)$$

With this substitution, (4.138) takes the form of the autoconvolution of a circ function (which is the same as the autocorrelation since the circ is an even function) evaluated at a "shift" of $b(\mathbf{r}_s - \mathbf{r}'')$, i.e.,

$$\langle p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s) \rangle_{R_m} = \frac{4\alpha_{\text{pf}}}{\pi D_b^2} C [g_1(\mathbf{r}) ** g_1(\mathbf{r})]_{\mathbf{r}=b(\mathbf{r}_s - \mathbf{r}'')}, \quad (4.140)$$

where, as before, $g_1(\mathbf{r})$ denotes $\text{circ}(2r/D_b)$. Equation (4.140) can be generalized to apply to a collimator with parallel but tapered bores by replacing $g_1(\mathbf{r}) ** g_1(\mathbf{r})$ by $g_2(\mathbf{r}) ** g_1(\mathbf{r})$, where g_1 and g_2 denote circ functions of diameter D_1 and D_2 , respectively.

We have now shown explicitly that \mathbf{r}_s and \mathbf{r}'' enter into $\langle p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s) \rangle$ only in the shift-invariant combination $\mathbf{r}_s - \mathbf{r}''$. We are thus justified in simplifying our notation and bringing it into line with that of previous sections by writing

$$\langle p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s) \rangle_{R_m} = \bar{p}_{\text{phc}}(\mathbf{r}'' - \mathbf{r}_s) = \bar{p}_{\text{phc}}(\mathbf{r}), \quad (4.141)$$

where $\mathbf{r} = \mathbf{r}'' - \mathbf{r}_s$. Because the magnification of the parallel-hole collimator is $+1$, this simple change of variables is sufficient to go from the point image in the \mathbf{r}'' plane, $\bar{p}_{\text{phc}}(\mathbf{r}'' - \mathbf{r}_s)$, to the point spread function in the \mathbf{r} plane. The overbar is retained as a reminder that we are dealing with an average PSF.

Compare $\bar{p}_{\text{phc}}(\mathbf{r})$, which is plotted in Fig. 4.25 with $p_{\text{sb}}(\mathbf{r})$ shown in Fig. 4.20. The latter function is not an autocorrelation, but rather the correlation of two different circ functions of different scales. It therefore has a flat top that we referred to as the umbra region. By contrast, $\bar{p}_{\text{phc}}(\mathbf{r})$ is precisely an autocorrelation and exhibits no umbra. This difference may appear strange at first since the integrand in (4.136) for $\bar{p}_{\text{phc}}(\mathbf{r})$ is so similar to that in (4.75) for $p_{\text{sb}}(\mathbf{r})$. To understand the difference, it is important to look at just what is being calculated. For $p_{\text{sb}}(\mathbf{r})$ the integration is over \mathbf{r}'' ; viewed as functions of

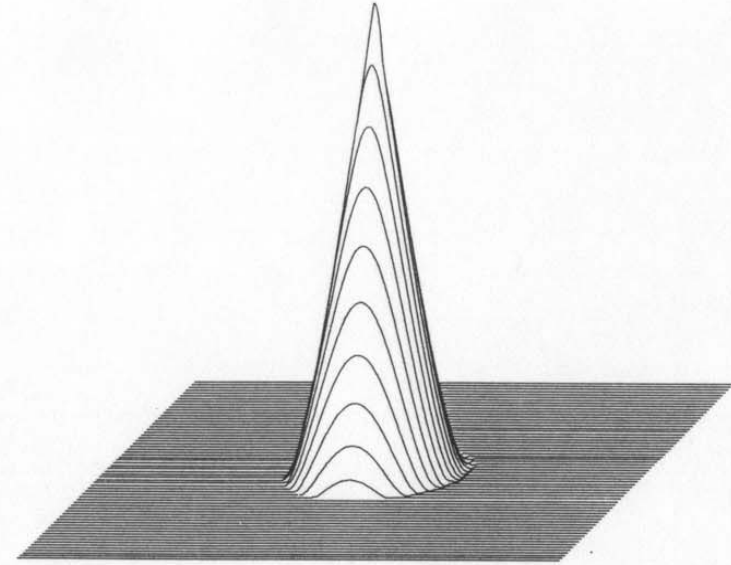


Fig. 4.25 Average PSF for a parallel-hole collimator. This function is the autocorrelation of a circ function.

\mathbf{r}'' the two circ functions have different scales. For $\bar{p}_{\text{phc}}(\mathbf{r})$ on the other hand, the integral is over the shift parameter \mathbf{R} ; as functions of \mathbf{R} the two circ functions of (4.136) have the same scale.

4.5.2 Sampling Theory Analysis

Let us back up to the stage of (4.133) in Section 4.5.1 where we had a general expression for the shift-variant PSF before any averaging had been applied. If, at this stage, the sum over k had been replaced with an integral over $\bar{\mathbf{r}}_k$, we could easily have written $p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s)$ as a convolution and, in fact, would have obtained (4.140), our final expression for $\bar{p}_{\text{phc}}(\mathbf{r})$. In other words, the averaging process is equivalent to replacing the sum in (4.133) by an integral.

We have encountered this same situation once before. In discussing the image-display portion of a scanner, we found that the film exposure, given by (4.126), had the form of a convolution except that one of the integrals had been replaced by a sum. In that case, we found that the difference between sum and integral disappeared if the sampling rate was adequate and we considered only the low-frequency components of the image. We shall now show that the same conclusion follows for the present problem.

Because of the various shifts and scale factors involved, this problem gets rather tedious in the space domain. A more orderly approach is to immediately transform (4.133) and carry out most of the manipulations in the frequency domain. To this end, let us rewrite (4.133)

$$p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s) = C \sum_k g_1(\mathbf{r}'' - \bar{\mathbf{r}}_k) \tilde{g}_1\left(\mathbf{r}'' + \frac{b}{a} \mathbf{r}_s - \frac{1}{a} \bar{\mathbf{r}}_k\right), \quad (4.142)$$

where $\tilde{g}_1(\mathbf{r})$ is the scaled circ function defined previously [see (4.73) and (4.78)]. We now compute the Fourier transform of this equation *with respect to the \mathbf{r}'' variable only*; \mathbf{r}_s is treated as a fixed parameter. Physically, this is equivalent to fixing the location of a source point at $\mathbf{r} = \mathbf{r}_s$, forming an image, and then performing a two-dimensional transform on the image. By use of the shift theorem of Fourier theory, (B.95), we have

$$\begin{aligned} P_{\text{phc}}(\boldsymbol{\rho}''; \mathbf{r}_s) &\equiv \mathcal{F}_2\{p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s)\} \\ &= C \sum_k [\exp(-2\pi i \boldsymbol{\rho}'' \cdot \bar{\mathbf{r}}_k) G_1(\boldsymbol{\rho}'')] \\ &\quad ** \left\{ \exp\left[-2\pi i \boldsymbol{\rho}'' \cdot \left(\frac{1}{a} \bar{\mathbf{r}}_k - \frac{b}{a} \mathbf{r}_s\right)\right] \tilde{G}_1(\boldsymbol{\rho}'') \right\}. \end{aligned} \quad (4.143)$$

Writing out the convolution integral in this equation in detail, we find

$$\begin{aligned} P_{\text{phc}}(\boldsymbol{\rho}''; \mathbf{r}_s) &= C \sum_k \int_{-\infty}^{\infty} d^2 \rho' \exp(-2\pi i \boldsymbol{\rho}' \cdot \bar{\mathbf{r}}_k) G_1(\boldsymbol{\rho}') \\ &\quad \times \exp\left[-2\pi i (\boldsymbol{\rho}'' - \boldsymbol{\rho}') \cdot \left(\frac{1}{a} \bar{\mathbf{r}}_k - \frac{b}{a} \mathbf{r}_s\right)\right] \tilde{G}_1(\boldsymbol{\rho}'' - \boldsymbol{\rho}'). \end{aligned} \quad (4.144)$$

Collecting together all terms involving $\bar{\mathbf{r}}_k$, we recognize that they are the Fourier transform of a sum of delta functions:

$$\begin{aligned} \sum_k \exp\left[-2\pi i \bar{\mathbf{r}}_k \cdot \left(\boldsymbol{\rho}' + \frac{1}{a} (\boldsymbol{\rho}'' - \boldsymbol{\rho}')\right)\right] &= \int_{-\infty}^{\infty} d^2 r \exp(-2\pi i \mathbf{r} \cdot \boldsymbol{\rho}) \sum_k \delta(\mathbf{r} - \bar{\mathbf{r}}_k) \\ &= \mathcal{F}_2\left\{\sum_k [\delta(\mathbf{r} - \bar{\mathbf{r}}_k)]\right\} \end{aligned} \quad (4.145)$$

where

$$\boldsymbol{\rho} = \boldsymbol{\rho}' + (1/a)(\boldsymbol{\rho}'' - \boldsymbol{\rho}'). \quad (4.146)$$

Now if the bore centers $\bar{\mathbf{r}}_k$ form a square array with spacing ε_b , the sum of delta functions is just a two-dimensional comb function:

$$\sum_k \delta(\mathbf{r} - \bar{\mathbf{r}}_k) = \frac{1}{\varepsilon_b^2} \text{comb}\left(\frac{\mathbf{r}}{\varepsilon_b}\right). \quad (4.147)$$

We are treating the array here as infinite even though real collimators are finite. This is a small error if the number of bores in the collimator is large.

The Fourier transform of this comb function is also a comb [see (B.48)],

$$\mathcal{F}_2\left\{\sum_k \delta(\mathbf{r} - \bar{\mathbf{r}}_k)\right\} = \text{comb}(\varepsilon_b \boldsymbol{\rho}) = \frac{1}{\varepsilon_b^2} \sum_k \delta(\boldsymbol{\rho} - \boldsymbol{\rho}_k), \quad (4.148)$$

where the $\boldsymbol{\rho}_k$ vectors also form a square array, but with spacing $1/\varepsilon_b$.

Equation (4.144) now becomes

$$\begin{aligned} P_{\text{phc}}(\boldsymbol{\rho}''; \mathbf{r}_s) &= \frac{C}{\varepsilon_b^2} \sum_k \int_{-\infty}^{\infty} d^2 \rho' \exp\left(2\pi i (\boldsymbol{\rho}'' - \boldsymbol{\rho}') \cdot \frac{b}{a} \mathbf{r}_s\right) \\ &\quad \times \delta(\boldsymbol{\rho} - \boldsymbol{\rho}_k) G_1(\boldsymbol{\rho}') \tilde{G}_1(\boldsymbol{\rho}'' - \boldsymbol{\rho}'). \end{aligned} \quad (4.149)$$

The delta function in this equation can be rewritten, using (4.146),

$$\delta(\boldsymbol{\rho} - \boldsymbol{\rho}_k) = \delta[\boldsymbol{\rho}' + (1/a)(\boldsymbol{\rho}'' - \boldsymbol{\rho}') - \boldsymbol{\rho}_k] \quad (4.150)$$

or, since $a = 1 - b$,

$$\begin{aligned} \delta(\boldsymbol{\rho} - \boldsymbol{\rho}_k) &= \delta[\boldsymbol{\rho}'(1 - 1/a) + (1/a)\boldsymbol{\rho}'' - \boldsymbol{\rho}_k] \\ &= (a^2/b^2) \delta[\boldsymbol{\rho}' + (a/b)\boldsymbol{\rho}_k - (1/b)\boldsymbol{\rho}'']. \end{aligned} \quad (4.151)$$

We thus find, after some algebra,

$$\begin{aligned} P_{\text{phc}}(\boldsymbol{\rho}''; \mathbf{r}_s) &= \frac{C a^2}{\varepsilon_b^2 b^2} \sum_k \exp[2\pi i (\boldsymbol{\rho}_k - \boldsymbol{\rho}'') \cdot \mathbf{r}_s] \\ &\quad \times G_1\left(-\frac{a}{b} \boldsymbol{\rho}_k + \frac{1}{b} \boldsymbol{\rho}''\right) \tilde{G}_1\left(\frac{a}{b} \boldsymbol{\rho}_k - \frac{a}{b} \boldsymbol{\rho}''\right). \end{aligned} \quad (4.152)$$

If ε_b is small enough, a condition to be defined more precisely below, then the various terms in this sum will not overlap significantly and a low-pass filter (which could be the scintillation camera detector itself) may be used to isolate the single term for which $\boldsymbol{\rho}_k = 0$. In the frequency domain, this filtered image may be written

$$[P_{\text{phc}}(\boldsymbol{\rho}''; \mathbf{r}_s)]_{\text{lf}} = \frac{a^2 C}{b^2 \varepsilon_b^2} \exp(-2\pi i \boldsymbol{\rho}'' \cdot \mathbf{r}_s) G_1\left(\frac{\boldsymbol{\rho}''}{b}\right) \tilde{G}_1\left(\frac{-a\boldsymbol{\rho}''}{b}\right). \quad (4.153)$$

But, since $g_1(\mathbf{r})$ is real and symmetric,

$$\tilde{G}_1(-a\boldsymbol{\rho}''/b) = \tilde{G}_1(a\boldsymbol{\rho}''/b) = (1/a^2)G(\boldsymbol{\rho}''/b).$$

An inverse transform thus yields

$$[p_{\text{phc}}(\mathbf{r}''; \mathbf{r}_s)]_{\text{lf}} = \frac{C}{\varepsilon_b^2} [g_1(\mathbf{r}') ** g_1(\mathbf{r}')]_{\mathbf{r}' = b(\mathbf{r}'' - \mathbf{r}_s)}. \quad (4.154)$$

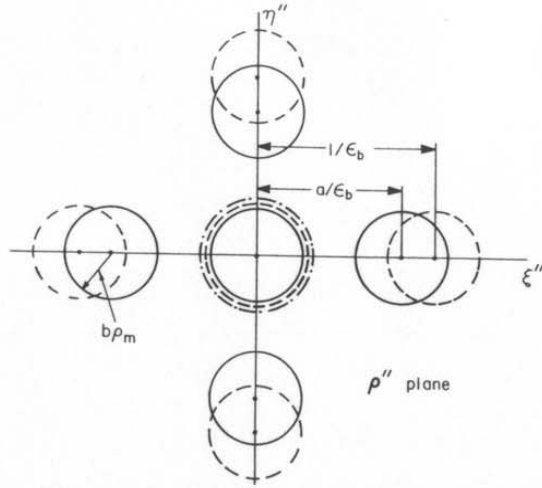


Fig. 4.26 Location of the various terms of Eq. (4.152) in the ρ'' plane. Solid circles: regions of support for $G_1[-(a\rho_k/b) + (\rho''/b)]$; dashed circles: regions of support for $\tilde{G}_1[(a\rho_k/b) - (a\rho''/b)]$; dot-dashed circle: passband of low-pass filter.

This result is in full accord with (4.140) since $\alpha_{pf}\epsilon_b^2 = \pi D_b^2/4$. Low-pass filtering is thus equivalent to “collywobbler averaging”.

An essential step in this derivation was the use of a low-pass filter to isolate a single term in (4.152). We now inquire under what condition this is possible. We need to consider only the zero-order term ($\rho_k = 0$) and the four surrounding first-order terms, all of which have $|\rho_k| = 1/\epsilon_b$. If none of the first-order terms overlap the zero-order terms, then none of the higher-order terms will either. The location and extent of the various orders is indicated in Fig. 4.26. In constructing this diagram the center of each region was first found by setting the argument of the corresponding function to zero, since $G_1(\rho'')$ is a maximum for $\rho'' = 0$. For example, $G_1[-(a\rho_k/b) + (\rho''/b)]$ in (4.152) has orders centered on the ξ'' axis at $\xi'' = \pm a/\epsilon_b$ (where ξ'' and η'' are the Cartesian components of ρ''). The diameter of the circular region is found by asserting that $G_1(\rho)$ has significant values only if ρ is less than some maximum value which we shall denote by ρ_m . From this it follows that $G_1(\rho''/b)$ is significant only within a circle of radius $b\rho_m$ in the ρ'' plane. Similar arguments for the orders lying along the η'' axis and for the \tilde{G}_1 factors in (4.152) then lead to the complete diagram of Fig. 4.26.

From the diagram it is seen that there is no overlap of orders if

$$a\rho_k \geq 2b\rho_m. \quad (4.155)$$

This condition will insure that the k th-order G_1 terms will not overlap either zero-order term. The condition for no overlap of the k th-order \tilde{G}_1 terms and the zero order is $\rho_k > 2b\rho_m$, but since $a < 1$, (4.155) is the more stringent condition.

If (4.155) is satisfied for the lowest-order term, $\rho_k = 1/\epsilon_b$, it will be satisfied for all orders. Therefore, using the definition of a and b from (4.70), we require

$$z/\epsilon_b \geq 2L_b\rho_m. \quad (4.156)$$

As a rough estimate, we may take $\rho_m = 1/D_b$. Furthermore, if the septa are thin, $D_b \approx \epsilon_b$. The results of this section are thus valid if

$$z \gtrsim 2L_b. \quad (4.157)$$

In clinical practice, z will usually be at least $2L_b$ since L_b is typically only 2–3 cm. We are thus justified in using the shift-invariant PSF, (4.154) or (4.140), to describe a camera collimator.

4.5.3 Modulation Transfer Function

Before writing down an expression for the modulation transfer function (MTF), we shall first generalize the PSF to allow for the possibility of a gap between the exit face of the collimator and the detector crystal. This is a simple modification because the photons continue to travel in straight lines as they traverse the gap. For a point source, the radiation pattern incident on the crystal is just a magnified version of the pattern emerging from the collimator. The magnification factor, by analogy with projection radiography, is

$$m_g = \frac{L_g + L_b + z}{L_b + z}, \quad (4.158)$$

where L_g is the gap length. The magnified point image is obtained from (4.140) by the substitution of \mathbf{r}''/m_g for \mathbf{r}'' in the argument of $p_{phc}(\mathbf{r}'')$, with a suitable amplitude scaling to conserve photons. The modified expression for the average PSF is thus

$$\bar{p}_{phc}(\mathbf{r}'') = \frac{4\alpha_{pf}}{\pi D_b^2} \frac{C}{m_g^2} [g_1(\mathbf{r}') ** g_1(\mathbf{r}')]_{\mathbf{r}' = b\mathbf{r}''/m_g}. \quad (4.159)$$

The leading factor of C/m_g^2 has a simple interpretation since

$$\frac{C}{m_g^2} = \frac{T}{4\pi(L_b + z)^2} \left(\frac{L_b + z}{L_b + z + L_g} \right)^2 = \frac{T}{4\pi(L_b + z + L_g)^2}. \quad (4.160)$$

In other words, since the distance from source to detector has been increased

from $L_b + z$ to $L_b + z + L_g$, the appropriate distance to use in the inverse-square law is now $L_b + z + L_g$.

Even though the point image is magnified when the gap is present, the magnification of the *collimator* is still +1. In other words, two points a distance x apart in the \mathbf{r} plane still produce two point images with a center-to-center spacing of x in the \mathbf{r}'' plane. The point-spread function is just $\bar{p}_{phc}(\mathbf{r})$, obtained from (4.159) by letting $\mathbf{r}'' \rightarrow \mathbf{r}$.

The Fourier transform of $\bar{p}_{phc}(\mathbf{r})$ is now easily performed. By use of the scaling law, (B.94), we find

$$\bar{P}_{phc}(\rho) = \frac{4\alpha_{pf}}{\pi D_b^2} \frac{C}{b^2} \left[G_1\left(\frac{m_g \rho}{b}\right) \right]^2. \quad (4.161)$$

Since $g_1(\mathbf{r})$ is the circ function of diameter D_b , we know from (B.114) that

$$G_1(\rho) = \frac{\pi D_b^2}{4} \frac{2J_1(\pi D_b \rho)}{\pi D_b \rho}. \quad (4.162)$$

The average MTF for the parallel-hole camera collimator is thus

$$\overline{\text{MTF}}_{phc}(\rho) \equiv \left| \frac{\bar{P}_{phc}(\rho)}{\bar{P}_{phc}(0)} \right| = \left| \frac{2J_1(\pi m_g D_b \rho / b)}{\pi m_g D_b \rho / b} \right|^2. \quad (4.163)$$

It is worth noting that $\bar{P}_{phc}(\rho)$ is everywhere real and positive. The problem of phase shifts in the transfer function discussed earlier does not occur here, and the MTF is a complete description of the system.

4.5.4 Resolution and Collection Efficiency

Having obtained an expression for the PSF, we may now readily compute the collimator resolution distance defined as usual as the FWHM of the PSF.

Since, by (4.159), the average collimator PSF is the autocorrelation of a circ function, we need to determine what shift is required between two identical circ functions to reduce their overlap area to one-half the area of either function separately. By numerically evaluating the autocorrelation, we find that the required shift is $0.808R$, where R is the radius of the circ function.

However, we note from (4.159) that the autocorrelation in \bar{p}_{phc} is calculated with the shift variable given by br''/m_g . To find the resolution distance δ_{phc} , we must set $r'' = \delta_{phc}/2$ and then demand that the shift be equal to $0.808D_b/2$. In other words,

$$b\delta_{phc}/2m_g = 0.808D_b/2, \quad (4.164)$$

or, using the definition of b from (4.70) and of m_g from (4.158), we have

$$\delta_{phc} = 0.808D_b \frac{L_g + L_b + z}{L_b}. \quad (4.165)$$

Several conclusions can be immediately drawn from this result. The first is that a gap between the collimator and detector (nonzero L_g) is bad. The detector should always be as close to the exit surface of the collimator as practical. Another important conclusion is that a parallel-hole collimator has its best resolution (smallest δ_{phc}) when the object is closest to the entrance face of the collimator (small z).

Finally, (4.165) shows that the collimator resolution is always improved by making the length of the bores, L_b , greater. We should not conclude from this, however, that a very large L_b is always desirable. The difficulty is that L_b also influences the collection efficiency of the collimator. This point is most easily seen by considering a point source in contact with the entrance face of the collimator (and not hidden by the septa). The fractional solid angle for photon collection is then given by

$$[\Omega/4\pi]_{z=0} = D_b^2/16L_b^2, \quad (4.166)$$

which obviously falls off rapidly if L_b is increased.

It is a little trickier to calculate the dependence of $\Omega/4\pi$ on L_b if $z \neq 0$ since in that case more than one collimator bore can collect photons from each object point. In fact, the graphical construction of Fig. 4.27 shows that the number of participating bores is given approximately by $\alpha_{pf}(L_b + z)^2/L_b^2$. Then, since the distance from the point source to the exit face of the collimator

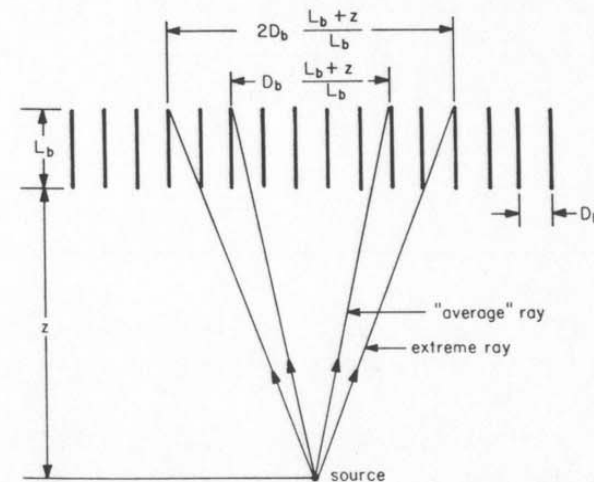


Fig. 4.27 Diagram for the calculation of collection efficiency of a parallel-hole collimator when $z \neq 0$.

is $L_b + z$, the fractional solid angle subtended by all bores is [cf. (4.166)]

$$\frac{\Omega}{4\pi} = \frac{D_b^2}{16(L_b + z)^2} \frac{\alpha_{pf}(L_b + z)^2}{L_b^2} = \frac{\alpha_{pf} D_b^2}{16L_b^2}. \quad (4.167)$$

In other words, if the septa are thin so that the packing fraction is near 1, the efficiency of a parallel-hole collimator is nearly independent of the source location and equal to the value for $z = 0$ given in (4.166).

The graphical arguments that led to (4.167) will now be replaced by a more rigorous analytical treatment. The key point to recognize is that the area integral of the PSF represents the mean number of counts collected from a unit point source. Since a unit point source is, by definition, one which on the average emits one photon per unit time, the integral of the PSF must be identical to $\Omega T/4\pi$. The calculation of the collection efficiency of a parallel-hole collimator thus reduces to the problem of integrating the autocorrelation of a circ function. [See (4.59).]

This integral might seem to be fairly difficult, but the central ordinate theorem of Fourier theory, (B.96), comes to our rescue. For any function $f(\mathbf{r})$ we have

$$\int_{-\infty}^{\infty} f(\mathbf{r}) d^2r = [\mathcal{F}_2\{f(\mathbf{r})\}]_{\rho=0} = F(0). \quad (4.168)$$

Therefore, letting $f(\mathbf{r})$ be $g_1(\mathbf{r}) ** g_1(\mathbf{r})$, we find

$$\int_{-\infty}^{\infty} [g_1(\mathbf{r}) ** g_1(\mathbf{r})] d^2r = [G_1(0)]^2. \quad (4.169)$$

But $G_1(0)$ may itself be determined by the central ordinate theorem:

$$G_1(0) = \int_{-\infty}^{\infty} g_1(\mathbf{r}) d^2r = \frac{\pi D_b^2}{4}. \quad (4.170)$$

We now apply these results, together with the scaling theorem (B.94) to the expression for \bar{p}_{phc} given in (4.159). The result is

$$\frac{\Omega T}{4\pi} = \int_{-\infty}^{\infty} \bar{p}_{phc}(\mathbf{r}'') d^2r'' = \frac{4\alpha_{pf}}{\pi D_b^2} \frac{C}{m_g^2} \left(\frac{m_g}{b}\right)^2 \left(\frac{\pi D_b^2}{4}\right)^2. \quad (4.171)$$

By use of the definitions of b and C from (4.70) and (4.72), respectively, we again arrive at (4.167). Note that m_g cancels out of $\Omega/4\pi$, as it must since the collection efficiency has already been determined once the photons emerge from the collimator; no photons are lost in traversing the gap.

Equation (4.167) for the efficiency and (4.165) for the resolution distance are the basic design equations for parallel-hole camera collimators. The trade-offs involved are illustrated in Fig. 4.28 where we plot δ_{phc} and $\Omega/4\pi$ for three hypothetical collimators. We see from this figure that the source

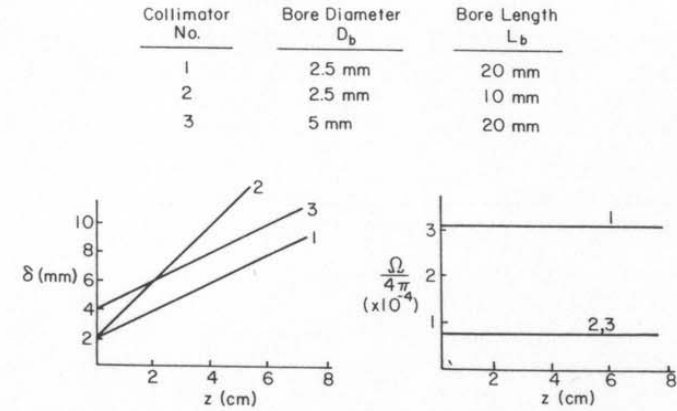


Fig. 4.28 Variation of resolution and efficiency with z for three hypothetical parallel-hole collimators.

distance z is an important consideration in collimator design. If we could place the collimator in contact with the source ($z = 0$), an obvious impossibility for sources within the body, then we could obtain any desired resolution without loss of efficiency simply by decreasing D_b and L_b in the same proportion. The drawback of this approach is that the choice of a small L_b leads to a collimator whose performance degrades rapidly as z is increased.

4.5.5 Comparison of the Parallel-Hole Collimator and the Pinhole

An important practical question that often arises is whether to use a pinhole or a collimator in a particular situation. This simple question turns out to be surprisingly slippery. As in any comparison, we must first state what is being held constant, what is being varied, and what is being compared. To limit the choices somewhat, let us rather arbitrarily fix the resolution and the field of view and compare collection efficiencies. For the parallel-hole collimator, the field of view is just equal to the detector diameter d'_{det} . The same FOV is obtained for the pinhole if $s_1 = s_2$ so that the magnification is unity [see (4.45)]. This choice has the additional virtue that detector resolution limitations affect the pinhole and collimator cameras in the same way since the magnifications are equal.

We now set $\delta_{ph} = \delta_{phc}$ and use (4.35) and (4.165) to eliminate d'_{ph} and D_b . Equations (4.33) and (4.167) may then be combined to yield

$$\frac{\Omega_{phc}}{\Omega_{ph}} = \frac{4\alpha_{pf}s_1^2}{(0.808)^2(L_g + L_b + z)^2}. \quad (4.172)$$

In this equation s_1 refers to the pinhole geometry while L_g , L_b , and z refer to the parallel-hole collimator. In practice, s_1 is limited by obliquity considerations as discussed in Section 4.2.6. However, if we ignore that problem for the moment, the best performance with both systems is obtained by putting the pinhole or the collimator as close to the source as possible, for example in contact with the patient's skin, thus making $s_1 = z$. By plugging in typical numbers for $\alpha_{pf}(\sim 0.5-0.8)$, $L_g(\sim 2-3 \text{ cm})$, $L_b(\sim 2-6 \text{ cm})$, and $z(\sim 2-15 \text{ cm})$, we see that the collimator usually has a modest advantage in collection efficiency over a pinhole. However, the large variability in the parameters precludes dogmatism.

Two limits are of some interest. If $z \gg L_g + L_b$ and $\alpha_{pf} \approx (0.808)^2$, we find that the collimator has a fourfold advantage. The opposite extreme of $L_g + L_b \gg z$ would seem to greatly favor the pinhole, but in fact this is not so, at least in medical applications. For such small z values the obliquity considerations for the pinhole, which were ignored in the formulation of (4.172), strongly reduce both the efficiency and the FOV of the pinhole camera. In practice, a pinhole will seldom if ever have an efficiency advantage over a parallel-hole collimator. The usefulness of the pinhole lies in the ease with which magnification can be changed, allowing the region of interest effectively to fill the available detector area.

An important similarity between pinhole and collimator imaging comes up when we contemplate decreasing the resolution distance of either system. If we improve the resolution of the pinhole by decreasing d'_{ph} while holding s_1 and s_2 fixed, (4.33) and (4.35) show that $\Omega_{ph} \propto d'^2_{ph} \propto \delta^2_{ph}$. Similarly, we may improve the resolution of the collimator by holding L_g , L_b , and z fixed and decreasing D_b . Then (4.165) and (4.167) show that $\Omega_{phc} \propto D_b^2 \propto \delta^2_{phc}$. Reducing the resolution distance thus requires a compensating increase in either patient dose or exposure time. In fact, by arguments similar to those adduced for scanners in Section 4.4.6, we can show (and shall do so in Chapter X) that the required dose or exposure time for constant signal-to-noise ratio varies inversely as the fourth power of the resolution distance [cf. (4.107)]. In other words, a twofold improvement in the resolution of the collimator or pinhole must be accompanied by a 16-fold increase in either the exposure time or the amount of radioactivity in the object if we wish to maintain constant SNR.

Precisely this same result was shown in Section 4.4.6 to apply to a scanner used with a multibore focused collimator. However, the result has even more serious implications for pinhole or collimator imaging with a scintillation camera because the resolution distance referred to in the fourth-power law is the one appropriate to the pinhole or collimator *alone*. There is a further image degradation, not present in a scanner, due to the image detector. Thus

even if we do reduce D_b or d'_{ph} by a factor of 2, the overall system resolution is improved by a smaller factor. The lesson to be drawn is that it is extraordinarily difficult to improve resolution in nuclear imaging.

4.5.6 Detector Considerations: Minifying and Magnifying Collimators

Although it was mentioned in Section 4.5.5, the image detector has not yet been included in our formulation. For a parallel-hole collimator, inclusion of the detector is trivial since the collimator has a magnification of unity. As in Section 4.2.5, we describe the detector either by a transfer function $D(\rho)$ or by a PSF, $d(r)$. The unit magnification eliminates the need for any scaling factors and we have directly

$$p_{det}(r) = d(r) \quad (4.173)$$

and

$$p_{tot}(r) = p_{phc}(r) ** p_{det}(r). \quad (4.174)$$

One conclusion to be drawn from this equation is that the final image resolution with a parallel-hole collimator can never be better than the resolution of the detector itself. Since the intrinsic resolution distance of typical scintillation detectors such as the Anger camera is usually about 4–8 mm, magnification techniques that enlarge the image onto the detector face are highly desirable. We have already discussed this approach in connection with pinhole imaging in Section 4.2.5. However, we also showed in Section 4.5.5 that pinholes are usually somewhat less efficient than collimators, especially when obliquity factors are taken into account. These considerations have led in recent years to the development of magnifying collimators as depicted in Fig. 1.22.

Conversely, there are some clinical applications where resolution is relatively unimportant but a large field of view is required. For these cases a minifying collimator as shown in Fig. 1.21 can be used. It is worth noting that a minifying collimator is an upside-down magnifying collimator, a fact that can be used to reduce the number of collimators a department must acquire.

In this section we shall not make any great distinction between a magnifying and a minifying collimator. Mathematically they are virtually indistinguishable and we shall use the subscript mc for both.

We assume that all bores in the collimator point to a common focal point a distance z_f from the entrance face of the collimator; z_f is a positive number for a magnifying collimator and a negative one for a minifying

collimator. In either case, the magnification is given by

$$m_{mc} = \frac{z_f + L_b + L_g}{z_f - z}, \quad (4.175)$$

where $m_{mc} > 1$ for a magnifying collimator and $m_{mc} < 1$ for a minifying one. (Note that z , L_b , and L_g are always *positive* numbers.) If $z_f \rightarrow \pm \infty$, we are back to the parallel-hole case and $m_{mc} \rightarrow 1$. Note also that very large magnifications can be obtained by setting $z \approx z_f$. However large minification ratios are more difficult since they require $z \gg |z_f|$.

The next step is to modify our previous results for collimator PSF, resolution, and efficiency so that they will apply to magnifying and minifying collimators. It is not so obvious that this step is possible since we have relied so heavily on the average-PSF concept introduced in Section 4.5.1. With a magnifying or minifying collimator we cannot form a reasonable average PSF by holding the source and detector fixed and translating the collimator over all possible positions since this corresponds to moving the image spot all over the detector. The resulting PSF would be huge and meaningless. Collywobblers do not work with magnifying or minifying collimators.

A closely related trick can, however, be employed. Suppose we hold the collimator fixed, move the source point through a vector distance \mathbf{R} , and move the detector by $m_{mc}\mathbf{R}$. Then the center of the image of the point remains stationary relative to the detector and integration over all \mathbf{R} yields a very reasonable average PSF. Of course, this is purely a mathematical device, not a practical way to remove collimator structure.

The remainder of the calculation closely parallels Section 4.5.1. We start with (4.88) for the PSF of a focused scanner collimator and modify it by deleting the integral over \mathbf{r}'' and replacing the factor of n_l/v_s with T . This leaves

$$p_{mc}(\mathbf{r}''; \mathbf{r}_s) = C \sum_j \text{circ}\left(\frac{2|\mathbf{r}'' - \bar{\mathbf{r}}_{2j}|}{D_2}\right) \text{circ}\left[\frac{2|a\mathbf{r}'' + b\mathbf{r}_s - \bar{\mathbf{r}}_{1j}|}{D_1}\right], \quad (4.176)$$

where, as in Section 4.4.5, $\bar{\mathbf{r}}_{1j}$ and $\bar{\mathbf{r}}_{2j}$ denote the center positions of the lower and upper apertures of the j th bore, and D_1 and D_2 are their diameters. Equations (4.86) and (4.87) are also assumed to still hold.

The averaging process described above may be written out explicitly by substituting $(\mathbf{r}'' - m_{mc}\mathbf{R})$ for \mathbf{r}'' and $(\mathbf{r}_s - \mathbf{R})$ for \mathbf{r}_s in (4.176), and then integrating over \mathbf{R} . The result is [cf. (4.134)]

$$\begin{aligned} \langle p_{mc}(\mathbf{r}''; \mathbf{r}_s) \rangle_{R_m} &= \frac{C}{\pi R_m^2} \int_{\text{disc}} d^2R \sum_j \text{circ}\left[\frac{2|\mathbf{r}'' - \bar{\mathbf{r}}_{2j} - m_{mc}\mathbf{R}|}{D_2}\right] \\ &\times \text{circ}\left[\frac{2|a(\mathbf{r}'' - m_{mc}\mathbf{R}) + b(\mathbf{r}_s - \mathbf{R}) - \bar{\mathbf{r}}_{1j}|}{D_1}\right], \quad (4.177) \end{aligned}$$

where the integral is over a disk of radius R_m , and we have assumed that the collimator-detector gap L_g is zero, a restriction that can be lifted later. If $R_m \rightarrow \infty$, all terms in the sum lead to the same value for the integral. To calculate the number of such terms, note that when the vector \mathbf{R} explores all points within the disk of radius R_m , the center of the first circ function in (4.177) sweeps out an area in the \mathbf{r}'' plane given by $\pi(m_{mc}R_m)^2$. The number of terms in the sum, K , is then just the number of bores of diameter D_2 that will fit in this area. Thus [cf. (4.135)],

$$K = \alpha_{pf}(2m_{mc}R_m/D_2)^2 \quad (4.178)$$

and

$$K/\pi R_m^2 = (4\alpha_{pf}/\pi D_2^2)m_{mc}^2. \quad (4.179)$$

The following change of variables in (4.177) is now useful:

$$\mathbf{R}' = m_{mc}\mathbf{R} - \mathbf{r}'' - \bar{\mathbf{r}}_{2j}. \quad (4.180)$$

Note that this change also requires a modification of the area element since $d^2R = (m_{mc})^{-2} d^2R'$. We can now use (4.86), (4.87), (4.175), and (4.179), plus a fair amount of algebra, to rewrite (4.177)

$$\begin{aligned} \langle p_{mc}(\mathbf{r}''; \mathbf{r}_s) \rangle &= C \frac{4\alpha_{pf}}{\pi D_2^2} \int_{\infty} d^2R' \text{circ}\left(\frac{2R'}{D_2}\right) \text{circ}\left[\frac{2}{D_2} \left| b \frac{D_2}{D_1} \left(\mathbf{r}_s - \frac{\mathbf{r}''}{m_{mc}} \right) - \mathbf{R}' \right| \right] \\ &= C \frac{4\alpha_{pf}}{\pi D_2^2} [g_2(\mathbf{r}') ** g_2(\mathbf{r}')]_{\mathbf{r}' = b(D_2/D_1)(\mathbf{r}_s - \mathbf{r}''/m_{mc})}, \quad (4.181) \end{aligned}$$

where

$$g_2(\mathbf{r}') = \text{circ}(2r'/D_2). \quad (4.182)$$

All that remains is to refer this average PSF back to the original object scale and to recast our notation in a form that is more evidently shift invariant. We can combine these steps by defining

$$\begin{aligned} \bar{p}_{mc}(\mathbf{r} - \mathbf{r}_s) &\equiv m_{mc}^2 \langle p_{mc}(m_{mc}\mathbf{r}; \mathbf{r}_s) \rangle \\ &= C \frac{4\alpha_{pf}}{\pi D_2^2} m_{mc}^2 [g_2(\mathbf{r}') ** g_2(\mathbf{r}')]_{\mathbf{r}' = b(D_2/D_1)(\mathbf{r}_s - \mathbf{r})}. \quad (4.183) \end{aligned}$$

There is virtually no difference between the functional form of this equation and that of the corresponding equation for the parallel-hole case, (4.140). The factor of D_2/D_1 in the shift variable is of minor import since, by (4.87), $D_2 \approx D_1 \approx D_b$ if $z_f \gg L_b$, a condition that is certainly satisfied for any practical collimator. The conclusion is that a magnifying or minifying collimator has essentially the same PSF and resolution as a parallel-hole

collimator with the same values of the parameters L_b , D_b , and z . Similarly, it should not require an elaborate calculation to convince the reader that the results of Section 4.5.3, where a collimator-detector gap was allowed and the transfer function was calculated, are still applicable.

On the other hand, it is worthwhile to reconsider the results of Section 4.5.4 for the collection efficiency. Equation (4.183) differs from its counterpart, (4.140), in one important respect—the leading factor of m_{mc}^2 . Therefore, by retracing the analysis that led up to the efficiency expression for the parallel-hole case, (4.167), we find that the efficiency of a magnifying or minifying collimator is

$$\frac{\Omega}{4\pi} = \frac{D_b^2 m_{mc}^2}{16L_b^2} \alpha_{pf}. \quad (4.184)$$

In other words, a magnifying collimator becomes *more* efficient as the source is moved away from the collimator face while a minifying collimator becomes less efficient.

To conclude this section, we shall state the result for the composite PSF of a system consisting of a scintillation detector and either a magnifying or minifying collimator. The result is

$$p_{tot}(\mathbf{r}) = p_{det}(\mathbf{r}) ** p_{mc}(\mathbf{r}), \quad (4.185)$$

where

$$p_{det}(\mathbf{r}) = m_{mc}^2 d(m_{mc}\mathbf{r}). \quad (4.186)$$

The proof of this result follows the lines of Section 4.2.5 [cf. (4.44)].

The importance of (4.186) is that by use of a magnifying collimator ($m_{mc} > 1$) we can make $p_{det}(\mathbf{r})$ effectively narrower and reduce the image degradation due to the detector. Of course, the price must be paid in field of view.

4.6 FURTHER COMPLICATIONS

A linear, shift-invariant system is a mythical beast. The analyses given so far in this chapter must fail, to a greater or lesser degree, when applied to real radiographic systems which can be neither exactly linear nor exactly shift invariant. The purpose of this section is to catalog the factors that cause the breakdown of our simple models and to comment briefly on some of them.

The factors neglected so far include:

1. scattered radiation;
2. statistical fluctuations;

3. shift-variant imaging due to:
 - a. the obliquity ($\cos^3 \theta$) factor;
 - b. nonparallelism of source and detector planes;
 - c. anisotropic emission;
4. septal penetration;
5. patient motion;
6. problems associated with three-dimensional objects;
7. spectral effects;
8. detector limitations, including
 - a. quantum efficiency;
 - b. nonlinearities;
 - c. geometrical distortions.

The first two items on this list, scattered radiation and statistical fluctuations, are enormously important in the analysis of radiographic systems. A separate chapter is devoted to each later in this book. Detector limitations are discussed in some detail for specific detectors in Chapter 5. Spectral effects are discussed in Chapters 7 and 11. The remaining topics are treated in this section.

4.6.1 Shift Variance

Real imaging systems are always shift-variant if for no other reason than their finite size; a point whose image entirely misses the detector cannot produce the same response as one in the center of the field of view. Several other, more subtle, sources of shift-variant behavior were mentioned and then ignored in the development of the general model in Section 4.1.

One justification for ignoring these effects is that, with the exception of the detector-boundary problem, they vary slowly with the position of the object point. Astronomers are fond of talking about an “isoplanatic patch,” by which they mean an ill-defined (but scarcely nebulous) patch of sky over which the shape of a star image is “essentially constant.” The source of the shift variance in astronomy—atmospheric inhomogeneities—is absent in radiographic imaging, but the principle is still applicable.

Before treating specific sources of shift variance, a brief comment on notation is required. We have already used two slightly different notations to denote the point response of an imaging system. For a general shift-variant system the response measured at point \mathbf{r} due to an object at \mathbf{r}_0 was denoted by $p(\mathbf{r}; \mathbf{r}_0)$. For a shift-invariant system the response function was written $p(\mathbf{r} - \mathbf{r}_0)$. For application of the isoplanatic patch concept, still a

third notation is useful. We acknowledge that the response depends strongly on the difference $\mathbf{r} - \mathbf{r}_0$ and only weakly on the absolute object position \mathbf{r}_0 by writing it $p[\mathbf{r} - \mathbf{r}_0, \mathbf{r}_0]$. To avoid confusion with $p(\mathbf{r}; \mathbf{r}_0)$, we shall use square brackets instead of parentheses and a comma instead of a semicolon in this new notation.

Of the systems discussed so far, shift variance is the least troublesome for the scintillation scanner. In this case only the boundary of the raster pattern causes any significant deviation from the true shift invariance. If we agree not to consider points within, say, twice the FWHM of the PSF of the edge of the field of view, then it is an excellent approximation to ignore the shift-variant behavior.

Shift variance may also be ignored, at least insofar as the image-forming operation is concerned, with a camera-collimator combination. Away from the boundary, the collimator may be treated as shift-invariant if we interpret the PSF in terms of either the "collywobbler-average" function of Section 4.5.1 or the filtered image of Section 4.5.2. Of course, the camera *detector* can respond differently to different source points even though the *collimator* is shift-invariant. Typically an Anger camera has poorer resolution at the edge of the field of view, shows some degree of geometric distortion, and has a sensitivity that varies by perhaps $\pm 10\%$ over the field. The source of these difficulties is discussed in Chapter 5.

Pinhole cameras are only slightly more complicated in this regard. The $\cos^3 \theta$ factor reduces the amplitude of the PSF as the edge of the field is approached, but the shape of the PSF is virtually unchanged over the field if the aperture plate is thin. (Recall that a circular pinhole projected from any angle produces a circular image if the detector plane is parallel to the aperture plane.) A thick aperture plate does result in a shape change for large θ , as indicated in Fig. 4.9, but this effect can be minimized by tapering the pinhole. In other words, the shift-variant point response for a pinhole can, to a good approximation, be factored as

$$p_{\text{ph}}[\mathbf{r} - \mathbf{r}_0, \mathbf{r}_0] = \cos^3 \theta(\mathbf{r}_0) p_{\text{ph}}(\mathbf{r} - \mathbf{r}_0), \quad (4.187)$$

where $p_{\text{ph}}(\mathbf{r} - \mathbf{r}_0)$ was calculated in Section 4.2.

The case in which shift variance is most important is transmission radiography. Practical x-ray tubes almost always have a tilted anode, as shown in Fig. 1.6, in order to reduce the projected area of the focal spot.

To analyze the tilted-anode geometry and to simultaneously allow for the fact that bremsstrahlung emission is far from isotropic, we introduce the concept of *photon radiance*, denoted by $L(\mathbf{r}_s, \hat{\mathbf{n}}_0)$, where \mathbf{r}_s is a three-dimensional vector specifying position on the source and $\hat{\mathbf{n}}_0$ is a three-dimensional unit vector pointing from the source point to the object point of interest. The photon radiance is defined such that $L(\mathbf{r}_s, \hat{\mathbf{n}}_0) da_s d\Omega$ is the number of pho-

tons per second emitted by a source element of area da_s into the solid angle $d\Omega$ in the direction $\hat{\mathbf{n}}_0$. This definition differs from the usual definition of radiance in optics in two respects. First, it is expressed in terms of photon flux density per steradian rather than energy flux density per steradian. These two quantities are related by the photon energy. The second difference is more subtle. In optics, the area involved in the definition of radiance is usually taken as the *projected* area of the source projected onto a plane normal to the direction of propagation. With this definition, diffuse optical radiators (Lambertian surfaces) have constant radiance, independent of orientation. There is no analog of diffuse radiators in radiology, so a definition in terms of actual source area rather than projected area is more natural.

Suppose that the x-ray anode is a plane tilted at an angle θ_a measured from the z axis as shown in Fig. 4.29. The vector \mathbf{r}_s is confined to this plane. The normal to the plane is defined by a unit vector $\hat{\mathbf{n}}_s$ given by

$$\hat{\mathbf{n}}_s = (0, \cos \theta_a, \sin \theta_a). \quad (4.188)$$

Therefore,

$$\mathbf{r}_s \cdot \hat{\mathbf{n}}_s = 0. \quad (4.189)$$

To make contact with our previous theory, we must project the photon radiance onto the x - y plane and thereby determine the emission function $f(\mathbf{r})$ defined in Section 4.1.1. Here, \mathbf{r} is a two-dimensional vector in the x - y plane, or, equivalently, a three-dimensional vector whose z component is zero. The photons which are emitted from point \mathbf{r}_s in the direction of $\hat{\mathbf{n}}_0$ will pass through the x - y plane at point \mathbf{r} only if the vector $\mathbf{r} - \mathbf{r}_s$ is parallel to $\hat{\mathbf{n}}_0$, or

$$\mathbf{r} - \mathbf{r}_s = \alpha \hat{\mathbf{n}}_0, \quad (4.190)$$

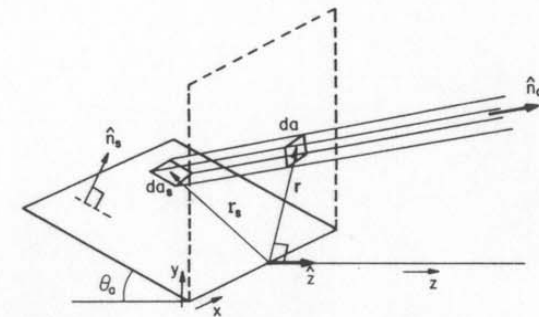


Fig. 4.29 Geometry for calculating the shift-variant PSF in transmission radiography with a tilted-anode x-ray tube.

where α is a scalar. Equations (4.189) and (4.190) can be satisfied simultaneously only if

$$\alpha = \frac{\mathbf{r} \cdot \hat{\mathbf{n}}_s}{\hat{\mathbf{n}}_0 \cdot \hat{\mathbf{n}}_s}, \quad (4.191)$$

from which we find

$$\mathbf{r}_s = \mathbf{r} - \left[\frac{\mathbf{r} \cdot \hat{\mathbf{n}}_s}{\hat{\mathbf{n}}_0 \cdot \hat{\mathbf{n}}_s} \right] \hat{\mathbf{n}}_0. \quad (4.192)$$

Thus $f(\mathbf{r})$ must be proportional to $L(\mathbf{r} - \alpha \hat{\mathbf{n}}_0, \hat{\mathbf{n}}_0)$. Two considerations are necessary to fix the constant of proportionality. The first is that $f(\mathbf{r})$ represents an emission into 4π steradians while $L(\mathbf{r}_s, \hat{\mathbf{n}}_0)$ represents emission into one steradian; a factor of 4π is therefore needed. The second point is that we must relate the area element d^2r in the plane $z = 0$ to the area element da_s in the actual source plane. This step is accomplished by projecting both da_s and d^2r onto a plane normal to $\hat{\mathbf{n}}_0$ and demanding that the projected areas be equal. In this way, all photons that are emitted by the element da_s in the direction $\hat{\mathbf{n}}_0$ must also pass through d^2r . This then requires that

$$(\hat{\mathbf{n}}_0 \cdot \hat{\mathbf{n}}_s) da_s = (\hat{\mathbf{n}}_0 \cdot \hat{\mathbf{z}}) d^2r, \quad (4.193)$$

where $\hat{\mathbf{z}}$ is a unit vector parallel to the z axis and hence normal to the plane containing d^2r . But notice that $\hat{\mathbf{n}}_0 \cdot \hat{\mathbf{z}}$ is just $\cos \theta$ where, as before, θ is the angle between the z axis and the line along which the x rays travel. Similarly we define

$$\hat{\mathbf{n}}_0 \cdot \hat{\mathbf{n}}_s \equiv \cos \theta_s. \quad (4.194)$$

For the two functions $f(\mathbf{r})$ and $L(\mathbf{r}_s, \hat{\mathbf{n}}_0)$ to describe the same emission patterns, we must have

$$L(\mathbf{r} - \alpha \hat{\mathbf{n}}_0, \hat{\mathbf{n}}_0) da_s d\Omega = f(\mathbf{r}) d^2r d\Omega / 4\pi \quad (4.195)$$

or, with (4.193) and (4.194),

$$f(\mathbf{r}) = 4\pi \frac{\cos \theta}{\cos \theta_s} L(\mathbf{r} - \alpha \hat{\mathbf{n}}_0, \hat{\mathbf{n}}_0). \quad (4.196)$$

Of course, $f(\mathbf{r})$ is now also a function of $\hat{\mathbf{n}}_0$ even though this dependence is not exhibited explicitly.

We shall illustrate this general result by returning to the disk focal spot of Section 4.3.1. In this case we assume that the high-energy electrons bombard a circular region on the anode, so that

$$L(\mathbf{r}_s, \hat{\mathbf{n}}_0) = L_0(\hat{\mathbf{n}}_0) \text{circ}(2r_s/d_{fs}), \quad (4.197)$$

where $L_0(\hat{\mathbf{n}}_0)$ describes the angular dependence of the x-ray emission and is independent of \mathbf{r}_s . Equation (4.196) now becomes

$$f(\mathbf{r}) = 4\pi \frac{\cos \theta}{\cos \theta_s} L_0(\hat{\mathbf{n}}_0) \text{circ} \left[\frac{2|\mathbf{r} - \alpha \hat{\mathbf{n}}_0|}{d_{fs}} \right]. \quad (4.198)$$

This expression for $f(\mathbf{r})$ describes an effective focal-spot distribution that is appropriate to those x rays that are emitted in the direction $\hat{\mathbf{n}}_0$. Note that $f(\mathbf{r})$ is actually a very complicated function of $\hat{\mathbf{n}}_0$ since θ , θ_s , and α all depend on $\hat{\mathbf{n}}_0$. Moreover, α is a function of \mathbf{r} also. However, the important features of the solution may be discerned by studying two special cases.

First, to verify that (4.198) is reasonable, suppose that the anode is actually parallel to the plane $z = 0$. Then $\theta_a = \pi/2$, $\mathbf{r} \cdot \hat{\mathbf{n}}_s = 0$, $\alpha = 0$, and $\theta_s = \theta$. The effective focal spot is then a simple circ function as expected:

$$f(\mathbf{r}) = 4\pi L_0(\hat{\mathbf{n}}_0) \text{circ}(2r/d_{fs}) \quad \text{if } \theta_a = \pi/2. \quad (4.199)$$

Next we consider a general anode angle θ_a but assume that the object point lies on the z axis. The relevant vectors in component form are then

$$\begin{aligned} \hat{\mathbf{n}}_0 &= (0, 0, 1) && \text{(object point on } z \text{ axis),} \\ \hat{\mathbf{n}}_s &= (0, \cos \theta_a, \sin \theta_a), \\ \mathbf{r} &= (x, y, 0), \end{aligned} \quad (4.200)$$

from which, after a little algebra, we obtain

$$|\mathbf{r} - \alpha \hat{\mathbf{n}}_0| = [x^2 + (y^2/\sin^2 \theta_a)^2]^{1/2}. \quad (4.201)$$

The circ function in (4.198) is nonvanishing within a region whose boundaries are determined by setting (4.201) equal to $d_{fs}/2$. This region is an ellipse with major axis d_{fs} and minor axis $d_{fs} \sin \theta_a$. In other words, the apparent dimension of the focal spot in the y direction is reduced by the factor $\sin \theta_a$, improving the resolution in that direction.

This same procedure can be used to find the shape of the effective focal spot for any object point. In all cases, it turns out to be an ellipse, but the algebra required to substantiate that statement is somewhat tedious. For this reason, and also because the disk focal spot is very artificial to begin with, the point will not be pursued further here.

We shall close this section by presenting a general expression for the shift-variant PSF in the tilted-anode geometry. To accomplish this end, we need to rewrite (4.196) in such a way that its \mathbf{r} dependence is more evident. In particular, the \mathbf{r} dependence of α must be exhibited. A useful vector identity here is the so-called **BAC-CAB** rule,

$$\mathbf{A} \times (\mathbf{B} \times \mathbf{C}) = \mathbf{B}(\mathbf{A} \cdot \mathbf{C}) - \mathbf{C}(\mathbf{A} \cdot \mathbf{B}), \quad (4.202)$$

which enables us to write

$$\mathbf{r} - \alpha \hat{\mathbf{n}}_0 = \frac{1}{\hat{\mathbf{n}}_0 \cdot \hat{\mathbf{n}}_s} [\mathbf{r}(\hat{\mathbf{n}}_0 \cdot \hat{\mathbf{n}}_s) - \hat{\mathbf{n}}_0(\mathbf{r} \cdot \hat{\mathbf{n}}_s)] = \frac{1}{\cos \theta_s} [\hat{\mathbf{n}}_s \times (\mathbf{r} \times \hat{\mathbf{n}}_0)]. \quad (4.203)$$

The shift-variant PSF is now found by substituting (4.196) and (4.203) into (4.54) and reinstating the $\cos^3 \theta$ factor. The final result is

$$p_{fs}[\mathbf{r} - \mathbf{r}_0, \mathbf{r}_0] = 4\pi \frac{C}{a^2 b^2} \frac{\cos^4 \theta}{\cos \theta_s} L \left\{ \frac{\hat{\mathbf{n}}_s \times [(\mathbf{r} - \mathbf{r}_0) \times \hat{\mathbf{n}}_0]}{-b \cos \theta_s}, \hat{\mathbf{n}}_0 \right\}. \quad (4.204)$$

4.6.2 Septal Penetration

In this section we shall be concerned with photons that penetrate some distance through nominally opaque material and are detected when they should be blocked (Mather, 1957; Beck, 1968a,b). This phenomenon is more important in nuclear medicine than in diagnostic radiology for two reasons. First, gamma rays of interest in nuclear medicine are usually more energetic and hence more penetrating than diagnostic x rays. And second, the very act of image formation in nuclear medicine consists of blocking unwanted photons. Small amounts of penetration can thus be very important when compared to the small number of photons that are deliberately passed.

The first point to be made is that penetration can be described by adding a new term to the geometrical PSF calculated previously (Harris *et al.*, 1964; Beck, 1964b; Mather, 1957). This statement follows because all detected photons can be divided into two mutually exclusive classes: those that have penetrated through the nominally opaque material and those that did not encounter any opaque material in the first place. For a point source the detected photons of the latter class constitute the geometrical PSF of the previous sections. The photons of the former class produce another image which we shall call the *penetration PSF*.

The penetration PSF for a pinhole camera is easily calculated. Since it will generally be shift-variant we must fix the source point \mathbf{r}_s and the observation point \mathbf{r}'' and then determine what path a photon must travel to get from \mathbf{r}_s to \mathbf{r}'' . If the path goes through the clear aperture of the pinhole, we are not interested since this photon contributes to the geometrical PSF rather than the penetration PSF. If, however, the path includes a thickness $t(\mathbf{r}'', \mathbf{r}_s)$ of absorbing material, we must calculate the probability that the photon will pass through the material unimpeded and go on to the detector. If the linear attenuation coefficient of the material is μ , this probability is simply $\exp[-\mu t(\mathbf{r}'', \mathbf{r}_s)]$. Scattering in the material can usually be neglected, especially if the detector is capable of energy discrimination.

As an example, consider a simple pinhole drilled through a lead plate of thickness t_0 . For simplicity we assume that $s_1 = s_2$ and $t_0 \ll d'_{ph}$. If the plate is parallel to the detector, the path length $t(\mathbf{r}'', \mathbf{r}_s)$ is given by

$$t(\mathbf{r}'', \mathbf{r}_s) = t_0 / \cos \theta(\mathbf{r}'', \mathbf{r}_s), \quad (4.205)$$

where, as before, $\theta(\mathbf{r}'', \mathbf{r}_s)$ is the angle of the ray measured from the normal to the detector plane. By a straightforward extension of the arguments given in Section 4.2, the penetration PSF is found to be [cf. (4.36)]

$$p_{pen}[\mathbf{r} - \mathbf{r}_s, \mathbf{r}_s] = C(b/a)^2 \exp[-\mu t_0 / \cos \theta(\mathbf{r}'', \mathbf{r}_s)], \quad (4.206)$$

where $\mathbf{r} = -a\mathbf{r}''/b$, and the expression is valid everywhere except within the geometrical image of the pinhole. (If t_0 were comparable to the pinhole diameter, this expression would also be in error near the edge of the geometrical image.)

For penetration to be negligible the integral of $p_{pen}[\mathbf{r} - \mathbf{r}_s, \mathbf{r}_s]$ over the \mathbf{r} plane must be small compared to the corresponding integral of $p_{ph}(\mathbf{r} - \mathbf{r}_s)$ given by (4.36). Roughly speaking, this requires that

$$\frac{\pi d_{det}^2}{4} \exp(-\mu t_0) \ll \frac{\pi d_{ph}^2}{4} \left(\frac{s_1 + s_2}{s_1} \right)^2. \quad (4.207)$$

Let us turn now to a somewhat more difficult problem—the calculation of the penetration PSF for a camera with a parallel-hole collimator. One effect of penetration in this case is to reduce the effective bore length. Even if the septa are very thick, gamma rays can still penetrate through the corners of the septa, thereby increasing the angular field of view of each individual bore. Since the mean penetration length is μ^{-1} , many authors make an approximate correction for this effect by replacing L_b with $L_b - \mu^{-1}$ in the equations for resolution, (4.165), and collection efficiency, (4.167). [In (4.165) this replacement applies only to the denominator. The numerator $L_g + L_b + z$ is the total distance from source to detector and is therefore constant.] Since μL_b must surely be large compared to unity in any usable collimator, this correction is a small one.

A more serious penetration problem occurs as the incidence angle is increased. Then the pathlength through any one septum decreases rapidly but the number of septa in the path increases correspondingly. The overall effect is to produce a broad, low-amplitude PSF very much as in the pinhole case.

A simple yet quite reasonable estimate of the total penetration can be obtained by just ignoring the fine structure of the collimator (Newell *et al.*, 1952). In other words, we imagine that the absorbing atoms are uniformly distributed through the volume of the collimator rather than arranged in discrete septa. The effective density of absorbing atoms is then given by the

actual density times $(1 - \alpha_{pf})$. This approximation is a poor one for small values of the incidence angle θ , but rapidly improves as θ is increased. At the extreme, if $\theta = 0$ then a photon can in reality penetrate a septum only by traversing the full bore length L_b ; the probability of this occurrence is $\exp(-\mu L_b)$, a very small number. The model of a uniform distribution of absorber, however, predicts a probability of penetration at $\theta = 0$ of $\exp[-\mu L_b(1 - \alpha_{pf})]$. This is still a small number in practice, but is much larger than $\exp(-\mu L_b)$. The real justification for the model is that we are usually more interested in the total penetration, i.e., the integral of the PSF, than in the details of the shape of the PSF. Since the largest contribution to the integral will come from rays that cross several septa, the behavior near $\theta = 0$ is of little concern.

With these preliminaries we can now write down an expression for the penetration PSF of a parallel-hole collimator. By analogy with (4.206), we have

$$p_{\text{pen}}[\mathbf{r}'' - \mathbf{r}_s, \mathbf{r}_s] = T[4\pi(L_b + L_g + z)^2]^{-1} \exp\left[\frac{-\mu L_b(1 - \alpha_{pf})}{\cos \theta(\mathbf{r}'', \mathbf{r}_s)}\right]. \quad (4.208)$$

Once again, the penetration PSF is a broad, slowly varying function. To find the total penetration we must integrate (4.208) over the detector plane. This step can be carried out numerically or even analytically if a small-angle approximation for $\theta(\mathbf{r}'', \mathbf{r}_s)$ is valid.

Although such approximate techniques may give a useful indication of the penetration performance of a collimator for a scanner or camera, the only reliable way to get detailed information about penetration seems to be computerized ray tracing (Rotenberg and Johns, 1965; Jahns, 1981; Miracle *et al.*, 1979).

4.6.3 Patient Motion

Patient motion, an important practical problem in both diagnostic radiology and nuclear medicine, is easy to graft onto our formalism. As a highly idealized example, suppose the patient moves at constant velocity v during an exposure of time T taken with a scintillation camera. Then the image of a point is uniformly smeared over a line of length vT . We can describe this situation by a PSF for patient motion given by

$$p_{\text{pm}}(\mathbf{r}) = \frac{1}{vT} \text{rect}\left(\frac{x}{vT}\right) \delta(y), \quad (4.209)$$

where $\mathbf{r} = (x, y)$ and the x axis is parallel to \mathbf{v} . The normalizing factor $1/vT$ ensures that $p_{\text{pm}}(\mathbf{r})$ approaches $\delta(\mathbf{r})$ if $v \rightarrow 0$. The overall system response is now found by convolving $p_{\text{tot}}(\mathbf{r})$, given by (4.174), with $p_{\text{pm}}(\mathbf{r})$.

Note that we did not specify above whether a pinhole, a parallel-hole collimator, or a magnifying or minifying collimator was used. It was not necessary to do so since we have been careful to refer all PSFs back to the original object scale. When a patient moves a distance vT , the corresponding PSF has width vT without need for any scale factors and without regard for the magnification of the rest of the system. Equation (4.209) is thus as applicable to projection radiography as it is to nuclear medicine.

One system that does behave somewhat differently with respect to patient motion is the scintillation scanner. In that case the effect of patient motion is better described as an image distortion rather than as a blur. Our previous example of a patient moving at constant velocity would result in a skewing of the scan raster in general. If \mathbf{v} were parallel to the rapid-scan direction, the uniform patient motion would be exactly equivalent to an alteration of the scan velocity v_s . To take a more realistic example, suppose the patient moves during a single scan line and remains stationary during the remainder of the scan. Then the image would be distorted along that one line and unaffected elsewhere, although the sections of the scan taken before and after the motion would not necessarily match at their interface. Such a discontinuity is a common and easily identifiable sign of patient motion in scanner images.

Although patient motion is easy to treat analytically, it is not so easy to deal with in practice and, indeed, may often constitute the ultimate limitation to image quality. This is especially true if the motion is due to the natural cardiac and respiratory cycles. There are really only two possible ways to control image blur due to these movements. Either the exposure time can be made so short that no significant motion occurs, or "gated" imaging can be employed. One important example of the latter approach is gated liver imaging in nuclear medicine. Liver images are particularly susceptible to motion blur since the liver is adjacent to the diaphragm. However, if a transducer is used to monitor the patient's respiration, the scintillation camera can be electronically gated off except during the relatively quiet period of full expiration. Of course, total imaging time must then be increased to record the same number of total counts, but the image quality is significantly improved.

4.6.4 Three-Dimensional Objects

Our entire analysis so far has been a kind of "Radiology in Flatland" (Abbott, 1952). We have consistently described gamma-ray-emitting objects by a two-dimensional distribution of source activity, while objects of interest

in diagnostic radiology have been treated as absorbing planes. A full treatment of three-dimensional objects requires the methods developed in Chapters 7 and 9, but a few comments are presented here primarily in an effort to convince the reader that the foregoing sections of this chapter were more than an exercise in futility.

Consider first the nuclear medicine case where a three-dimensional object can be described by a three-dimensional source activity function, $f(\mathbf{r}, z)$. Here, \mathbf{r} is still a two-dimensional vector in a plane a distance z from the collimator face or pinhole plane. A three-dimensional volume element is thus specified by $dv = d^2r dz$. The activity function is defined in such a way that $f(\mathbf{r}, z) d^2r dz$ is the number of photons per unit time emitted by material within the volume element $d^2r dz$ located at coordinates (\mathbf{r}, z) or, equivalently, (x, y, z) .

If the radiation were not appreciably absorbed within the patient's body, we could now use all of our previous results simply by replacing $f(\mathbf{r})$ with $f(\mathbf{r}, z) dz$ and then integrating over z . For example, (4.13) becomes

$$h(\mathbf{r}'') = T \int_0^\infty dz [4\pi(z + s_2)^2]^{-1} \int_\infty d^2r f(\mathbf{r}, z) g(a\mathbf{r}'' + b\mathbf{r}), \quad (4.210)$$

where

$$a = z/(z + s_2) \quad (4.211)$$

and

$$b = s_2/(z + s_2). \quad (4.212)$$

(Of course, z is identical to our previous parameter s_1 , but the new designation emphasizes that it is a variable rather than a constant.)

However, (4.210) is not yet completely satisfactory because self-absorption may not be negligible. Furthermore, the body has very inhomogeneous attenuation properties, a fact that is essential to the success of diagnostic radiology but is a distinct nuisance in nuclear medicine. As discussed more fully in Chapter 7, a ray traversing this inhomogeneous medium is attenuated by a factor

$$\exp\left(-\int_S^D \mu(\mathbf{r}', z') dl'\right), \quad (4.213)$$

where $\mu(\mathbf{r}', z')$ is the linear attenuation coefficient at point (\mathbf{r}', z') , and the line integral runs from the source point S to the detector point D . Incorporating this factor in (4.210), we have

$$h(\mathbf{r}'') = T \int_0^\infty dz \int_\infty d^2r \frac{\exp\left(-\int_S^D \mu(\mathbf{r}', z') dl'\right)}{4\pi(z + s_2)^2} f(\mathbf{r}, z) g(a\mathbf{r}'' + b\mathbf{r}), \quad (4.214)$$

where the three-dimensional coordinates of S are (\mathbf{r}, z) . The important qualitative point about (4.214) is that calculation of the two-dimensional image $h(\mathbf{r}'')$ in general requires the knowledge of two separate three-dimensional distributions, $f(\mathbf{r}, z)$ and $\mu(\mathbf{r}, z)$.

Often it is valid to replace $\mu(\mathbf{r}, z)$ in (4.214) by a constant. For example, if only soft tissue intervenes between S and D , it is quite reasonable to replace $\mu(\mathbf{r}, z)$ by $\mu_{\text{H}_2\text{O}}$, the attenuation coefficient of water. This approximation does not, however, completely circumvent the problem since the path length from S to D depends on \mathbf{r} , z , and the external contours of the patient's body. Perhaps the best that can be said in general is that a nuclear medicine image does not really measure $f(\mathbf{r}, z)$, but rather $f(\mathbf{r}, z) \exp(-\int_S^D \mu dl)$. The exponential factor may or may not approximate a constant, depending on photon energy, depth of the organ being imaged and obesity of the patient. For example, a lung scan of a plump woman may show regions of apparently reduced activity due entirely to absorption in the breasts. On the other hand, if a liver scan is performed with a parallel-hole collimator on a slender patient, it would be very reasonable to regard the exponential factor as a constant multiplier for each plane z . And finally, for high-energy photons such as the 360-keV gamma rays from ^{131}I and superficial organs like the thyroid, very little error is made in ignoring absorption altogether.

The problem of three-dimensional objects becomes even more untidy in the transmission radiography case. If we represent a volume absorber by a stack of N absorbing planes, the generalization of (4.13) is

$$h(\mathbf{r}'') = C \int_\infty d^2r f(\mathbf{r}) \prod_{i=1}^N g_i(a_i \mathbf{r}'' + b_i \mathbf{r}), \quad (4.215)$$

where $g_i(\mathbf{r}')$ is the transmission of the i th plane at point \mathbf{r}' ,

$$a_i = 1 - b_i = \frac{z_i}{z_i + s_2}, \quad (4.216)$$

and z_i is the distance of the i th plane from the source plane.

Equation (4.215) is most easily interpreted if the focal-spot distribution can be approximated by a delta function,

$$f(\mathbf{r}) \approx f_0 \delta(\mathbf{r}), \quad (4.217)$$

in which case,

$$h(\mathbf{r}'') = C f_0 \prod_{i=1}^N g_i(a_i \mathbf{r}''). \quad (4.218)$$

In other words, the measured image $h(\mathbf{r}'')$ consists of a *multiplicative* (and hence nonlinear) superposition of images of each of the planes, with the magnification for the i th plane given by $1/a_i$.

When a screen-film system is used as the image detector, a further simplification is possible. As discussed in Chapter 5, the optical density D in the developed film is usually a linear function of the logarithm of the exposure, i.e.,

$$D(\mathbf{r}'') = D_0 + \gamma \log[h(\mathbf{r}'')], \quad (4.219)$$

where D_0 and γ are constants characteristic of the film. The logarithm converts the multiplicative superposition of (4.218) into an additive one:

$$D(\mathbf{r}'') = D_0 + \gamma \log(Cf_0) + \gamma \sum_{i=1}^N \log[g_i(a_i \mathbf{r}'')]. \quad (4.220)$$

In a peculiar sense, then, we have salvaged the linear systems approach to transmission radiography even with three-dimensional objects. We need only to regard the logarithm of the transmission, rather than the transmission itself, as the input to the system and to regard the optical density $D(\mathbf{r}'')$ as the output to obtain a linear input-output relation.

Of course, all of this was possible only because we assumed a delta-function source. The situation is far more complicated when we have a general source function and a three-dimensional (or multiplanar) object. Without really attempting a full solution, we can suggest the nature of the difficulty by rewriting (4.215). Suppose we are interested in one particular plane, say the j th. Then the factors in the N -fold product in (4.215) can be regrouped as

$$h(\mathbf{r}'') = C \int_{\infty} d^2r \left(f(\mathbf{r}) \prod_{i \neq j}^N g_i(a_i \mathbf{r}'' + b_i \mathbf{r}) \right) g_j(a_j \mathbf{r}'' + b_j \mathbf{r}). \quad (4.221)$$

The point spread function appropriate to the j th plane is calculated as in Section 4.3 by letting $g_j(\mathbf{r}')$ be a delta function,

$$g_j^{\delta}(\mathbf{r}') = \delta(\mathbf{r}' - \mathbf{r}_1). \quad (4.222)$$

The resulting image is given by

$$h^{\delta}(\mathbf{r}'', \mathbf{r}_1) = \left(\frac{C}{b_j} \right) f \left[\frac{\mathbf{r}_1}{b_j} - \frac{a_j \mathbf{r}''}{b_j} \right] \prod_{i \neq j}^N g_i \left(a_i \mathbf{r}'' + \frac{b_i}{b_j} (\mathbf{r}_1 - a_j \mathbf{r}'') \right). \quad (4.223)$$

In other words, the PSF is determined not only by the actual source function $f(\mathbf{r})$, but also by the details of the absorbing structures in all other planes. For example, a sharp-edged absorber in one plane can partially obscure the focal spot for some values of \mathbf{r}' and hence improve the apparent system resolution. The PSF is, of course, highly shift-variant because of parallax among the various planes.

One important limit should be mentioned. When the three-dimensional object is relatively structureless and has low contrast (e.g., soft tissue), then the effect of the product term in (4.223) is merely to modulate the overall intensity of the source distribution without seriously affecting the details of its shape. The imaging system is still shift-variant, but a relatively large isoplanatic patch can be defined. In this case we are justified in using the planar models of Section 4.3 to calculate PSF, MTF, etc.